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Abstract: With the integration of power electronic converters and components, an accurate thermal design becomes essential. Hence, precise thermal models for components are needed for their optimal design. This paper focuses on the development of an analytical model for the design thermal resistance of planar magnetic cores (PMC). Based on computational fluid dynamic (CFD) simulations, the PMC design thermal resistance variation is studied, according to ambient temperature and level of losses. Then, a polynomial equation is developed to model those variations and coefficients are deduced for all the sizes of PMC. This analytical model, useful for designers, is finally validated with thermal measurements on a planar transformer prototype.

Keywords: planar magnetics; thermal resistance; modeling; design

1. Introduction

Reducing power electronic converter volume and increasing its efficiency are two main objectives when developing a power converter [1,2]. These criteria are essential, especially in embedded and transportation systems. They can lead to serious thermal constraints on power components. Regarding high frequency (HF) passive magnetic components (i.e transformers and inductors), volume, losses and thermal management are of major concern for designers. They need to be optimized in order to reach objectives of power density. Planar magnetic components are one solution for the reduction of magnetic component's size. They present lower losses and higher surface area to volume ratio compared to conventional wound components [3, 4]. They are particularly suitable for Electric Vehicle (EV) applications [5-7].

In order to evaluate the temperature's rise of a planar component in a design stage, a single equivalent thermal resistance can be used. Some expressions of such thermal resistance for planar magnetic cores (PMC) are given in the literature [2, 8-14]. It can be computed based on the external area of the component [8, 9] or from the volume of the core [10-12]. These expressions only depend on geometrical dimensions of the core and windings. They do not consider working conditions such as ambient temperature or dissipated power inside the component. Other models take into consideration power losses as well as the external area of the component [2, 13, 14]. The ambient temperature is never considered even if this parameter has great impact on heat transfer due to convection and radiation phenomena.

In this paper, an analytical expression for the thermal resistance of PMC is developed in order to take into account impact of losses and ambient temperature. For this study, planar magnetics are considered in natural air cooling with no heatsink. Such cooling so-

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lution is the first hypothesis fixed by designers when dealing with planar magnetics. Indeed, it is cost effective and well adapted to planar magnetics that present high power density compared to wound component.

Combinations of EE and E/Plate (PLT) cores are studied for cores' sizes 32, 38, 43, 58 and 64 [15] with Computational Fluid Dynamic (CFD) simulations. Then, a polynomial model is developed and coefficients are deduced for each combination and size of ferrite cores. The developed model is dedicated to design step or optimization process. It enables to quickly size, as fairly as possible, the thermal behavior of PMC.

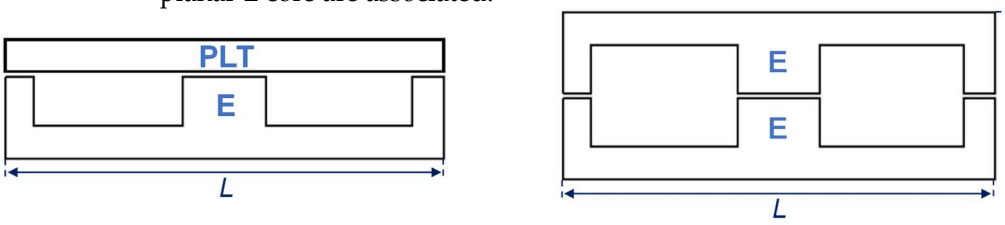
The paper is organized as follows: In Section II, some of the models available in the literature are first compared, based on the analysis reviewed in [16]. Then, in section III the methodology for the computation of equivalent thermal resistance depending on power loss and ambient temperature is detailed. CFD simulations for all the size of EE and E/PLT planar cores are performed using Icepack and Fluent softwares [17] in order to study the variation of their thermal resistance according to both parameters. Then, the obtained curves are compared to thermal resistance model usually used in design process to highlight benefits of such thermal resistance variation modelling. In section IV, the analytical model is developed and polynomial coefficients are deduced for each size of planar cores. Finally, the analytical model is compared to CFD results and an experimental validation is performed on a 360VA planar transformer prototype made with E/PLT 38 ferrite core.

2. Thermal resistance for the design of planar magnetics

As mentioned in the introduction, planar magnetics present some advantages compared to conventional wound magnetic components. One of their main advantage is linked to their particular geometry, linked to the use of planar cores, that increases cooling performance due to their higher surface to volume ratio [3, 4].

2.1. Planar EE and E/PLT cores

Planar magnetic cores are made of a 2-halve ferrite core (Figure 1). For E/PLT (Figure 1a), the E part is combined with a plate (PLT) one while for EE (Figure1b), two similar planar E core are associated.



(**a**) (**b**)

Figure 1. Cross section of planar cores: (**a**) E/PLT; (**b**) EE.

The width L refers to the size of the planar core. Thus, a E64 or a PLT64 has a width of 64 mm. Based on [15], lengths of standard planar cores are set up in [16]. From these data, two geometrical parameters can be deduced:

- The external area: A_{ext}. Its value is computed by summing all the external surfaces of the core and the windings;
- The effective volume: V_e. This value defines a hypothetical ring core having the same magnetic properties than the planar core [15].

As it will be detailed in the next section, these values of A_{ext} and V_e are used in many thermal resistance models from the literature.

2.2. Can a single global thermal resistance be used for planar magnetics?

Regarding PMC thermal modelling, temperature inside the component is quite homogeneous due to their large footprint compared to their weak thickness. As a consequence, a unique global thermal resistance can be used to model the planar component temperature rise (Figure 2). Then, the temperature rise ΔT is linked to the power dissipated inside the component P_d and the thermal resistance R_{th}:

$$\Delta T = R_{th} \times P_d \quad (1)$$

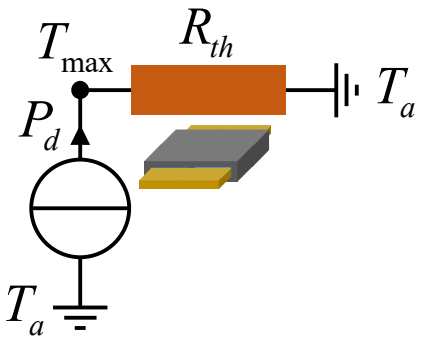


Figure 2. Planar magnetic thermal modeling with single global thermal resistance.

In order to highlight this attribute, a planar transformer made with EE64 planar core [15] is studied in free air convection condition with Finite Element Analysis (FEA). FEA is performed with Ansys Mechanical [17]. Thermal conductivities used for the FEM simulation are listed in Table 1. For the windings, copper and insulator are considered as a homogenous material with two different thermal conductivities [18]: a transverse one (K_{xy}) and a normal one (K_z). Their computations are based on [19]. For the magnetic core, thermal conductivity is the same in the three space directions. In the following sections, the same values will also be set for CFD modelling.

Table 1. Thermal conductivities.

Part of the planar component	Direction (x,y,z)	Thermal conductivity [W m^{-2} K^{-1}]
Winding – Transverse direction	xy	237
Winding – normal direction	z	0.5
Ferrite core	xyz	4

Other simulation conditions are listed below:

1. Total losses inside the transformer (13W) are divided in two parts: 6.5W for the winding and 6.5W for the core;
2. Thermal connection between the winding and the core is perfect;
3. Ambient temperature is set to 25°C;
4. A heat exchange coefficient of 14 W.K^{-1}.m^{-2} is applied to all the external area of the transformer [20].

Figure 3 presents the computed thermal distribution. Figure 3a presents the thermal distribution on the external surface of the planar transformer. Figure 3b and Figure 3c show the temperature inside the transformer along two cutting planes.

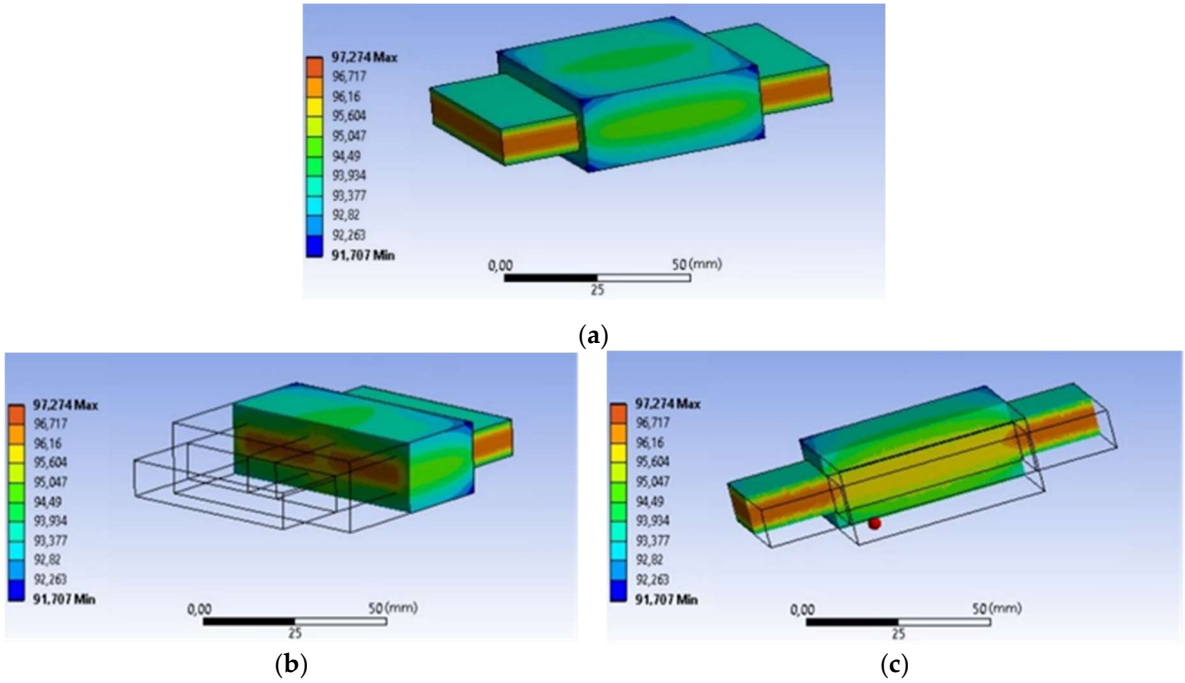


Figure 3. Example of EE64 core-based planar transformer temperature distribution: (**a**) 3D view; (**b**) Transverse section; (**c**) Longitudinal cut.

The temperature inside the transformer is quite homogenous. Indeed, temperature is between 91.7°C and 97.3°C. Compared to HF wound components, the temperature distribution is more homogenous in planar magnetics, as it is shown in [4]. Such temperature distribution (Figure 3) clearly justify the use of equivalent thermal resistance for fast estimation of temperature rise (1). In a planar transformer design process. losses can be non-uniform in the winding, but in steady state, the temperature of the winding is quite homogenous thanks to the significant area to volume ratio. Then, the difference between the temperature with uniform losses and non-uniform winding losses is small. This hypothesis is valid for natural convection cooling, which is the subject of this paper. For liquid cooled transformers, strong gradient of temperature can appear.

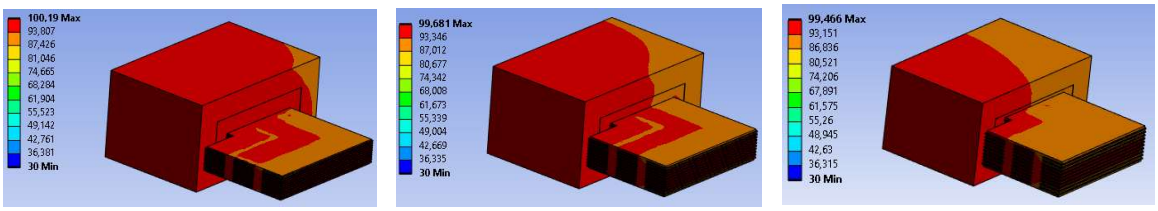
This example (Figure 3) is consistent with planar transformers with reduced core's airgap. Losses are uniformly distributed inside the component. This hypothesis is important. In general, the same hypothesis is considered when designing magnetics. If the losses are not uniform in the component, more complex models with electro-thermal coupling are needed. In the following, this uniform loss distribution hypothesis will be kept. The airgap (Figure 1) between E parts or E and PLT is negligible.

2.3. Impact of parameters on the planar component temperature distribution

In this section, the impact of layers' thickness and loss repartition on the temperature distribution is discussed. A E/PLT58 core-based planar transformer, with 10 layers, serves as an example for the analysis and the comparison. The transformer temperature distribution is computed with FEA [17].

First, the impact of the insulator thickness is studied. The conductors' thickness is fixed to 0.2mm while their width is 4mm. Three insulator thickness values (0.2 mm, 0.3 mm and 0.4mm) are tested (Table 2). The thermal conductivity is 380 $W.m^{-2}.K^{-1}$ for the copper tracks and 0.15 $W.m^{-2}.K^{-1}$ for the insulating layers. Only a quarter of the transformer is simulated thanks to the symmetry (Figure 4). The copper and core losses are both equal to 1.5 W for the transformer quarter.

The analysis of these test cases shows a limited impact on the temperature distribution, as illustrated for in Figure 4. The maximal temperature value presents a small variation (less than 1°C). Then, the hypothesis of using a fix value for the winding equivalent thermal conductivity can be justified. This hypothesis is only valid for a well-built transformer with a good thermal coupling between winding and core (i.e. with a thermal interface material to fill the window area). In the case of liquid cooled or other strong cooling systems, the variation of the conductivity can have a more significant impact.



(a) **(b)** **(c)**

Figure 4. Simulation of E/PLT58 core-based planar transformer: (**a**) case 1; (**b**) case 2; (**c**) case 3.

Table 2. E/PLT58 planar transformer with various insulator thickness.

Parameters	Case 1	Case 2	Case 3
Copper thickness (mm)	0.2	0.2	0.2
Insulator thickness (mm)	0.2	0.3	0.4
Transverse K_{xy} ($W.m^{-2}.K^{-1}$)	190.1	152.1	126.8
Normal K_z ($W.m^{-2}.K^{-1}$)	0.30	0.25	0.22
Maximal temperature (°C)	100.19	99.68	99.46

Then, the impact of the loss distribution between the core and the winding is also studied. Based on the Case 1 (Table 2), with 0.2mm for the copper and the insulator thicknesses, three other cases have been studied:

- Case 4, where the total losses are localized in the core;
- Case 5, where the losses are split between the core and the winding;
- Case 6, where the losses are localized only in the winding.

From Table 3, one can say that the loss distribution between the transformer parts also has a limited impact. Indeed, the difference on the maximal temperature is lower than 4.4°C. In the worst case, where the total losses are localized in the winding (case 6), only an error of 6% is induced, compared to the reference case where the losses are equally distributed between the core and the winding (case 5). This error is reduced to 3.6% when the losses are localized only inside the core (case 4), because it is more exposed to the air compared to the winding. This last case will be used, in this paper, for the experimental validation. Then, using the hypothesis of an equally distributed losses between core and winding can be justified.

Table 3. Simulation results for different loss repartition (copper and core).

Parameters	Case 4	Case 5	Case 6
Core losses (W)	3	1.5	0
Copper losses (W)	0	1.5	3
Maximal temperature (°C)	102.7	100.2	104.56
ΔT (°C)	72.7	70.2	74.6
R_{th} (°C/W)	6.1	5.9	6.2
Error (%)	3.6	0	6.2

2.4. Comparison of planar magnetic core thermal resistance modelling

As mentioned in the introduction, some thermal resistance models are available in the literature [2, 8-14]. Some of these models are specific for the design of planar magnetics while others are more generic for the design of HF wound magnetics. Most of these models are only based on the geometrical dimensions of the core: External area (A_{ext}) and effective volume (V_e). Some also consider the power losses inside the magnetic device. The Table 4 lists these different models that are reviewed in [16].

Table 4. Thermal resistance models.

Application note / Authors	Reference	R_{th} Model	Parameters
Magnetic Designer / Muldoon	[8, 9]	R_{th_magDes}	External area - A_{ext}
Ferroxcube application note	[10]	$R_{th\_ANFerrox}$	Effective volume - V_e
Ferroxcube Soft Ferrite Design Tool (SFDT)	[11]	R_{th_SFDT}	Effective volume - V_e
Hurley, Wölfe	[12]	R_{th_Hur}	Effective volume - V_e
Van den Bossche, Valchev	[13]	R_{th_BosVal}	External area - A_{ext} Losses in the component - P_d
McLyman	[14]	R_{th_McL}	External area - A_{ext} Losses in the component - P_d
Zhang, Ngo	[2]	R_{th_ZhaNgo}	External area - A_{ext} Losses in the component - P_d

In order to compare these different models, a maximal power loss value (P_{max}) is defined according to the E/PLT and EE core size, to limit the temperature's rise to 80°C inside the planar component. These values are reported in Table 5. In the next sections, all the model will be evaluated on a power range from 1W to P_{max}.

Table 5. Maximal power loss values.

E/PLT core	P_{max}	EE core	P_{max}
E/PLT32	4	EE32	6
E/PLT38	6	EE38	7
E/PLT43	7	EE43	9
E/PLT58	13	EE58	16
E/PLT64	17	EE64	19

The thermal resistance models (Table 4) are compared, in Figure 5, for E/PLT32 and EE64 planar cores.

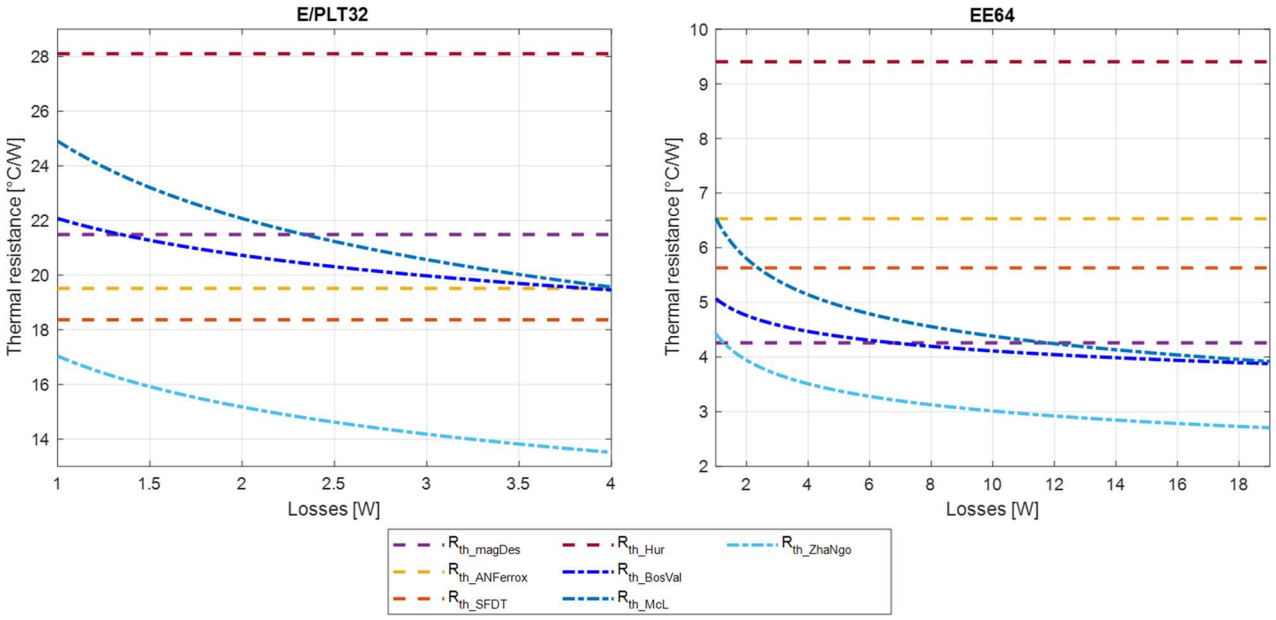


Figure 5. Comparison of R_{th} models for E/PLT32 and EE64 cores.

For E/PLT32, thermal resistance values vary from 17°C/W (R_{th_ZhaN}) to 28°C/W (R_{th_Hur}) for 1W losses while for 4W, models give values between 13.5°C/W (R_{th_Zha}) and 28°C/W (R_{th_Hur}). For EE64, values are between 4.2°C/W (R_{th_magDes}) and 9.4°C/W (R_{th_Hur}) for 1W losses while for 19W, models give values between 2.7°C/W (R_{th_ZhaNgo}) and 9.4°C/W (R_{th_Hur}). These values can lead to significant difference temperature estimations. As an example, for the E/PLT32 core both models give a 11°C difference for 1W and 58°C for 4W. For the EE64, these values are respectively 5.2°C and 127°C. The range variation of models is wide and can lead to significant error in thermal design of planar magnetics.

Four of the presented models are constant with losses. The three others decrease as the power losses increase. No one varies with ambient temperature.

In the following, a CFD study of E/PLT and EE planar cores is performed. The goal is to examine variation of thermal resistance according to power losses and ambient temperature. The results will be compared to 4 models from the literature: R_{th_magDes}, R_{th_SFDT}, R_{th_BosVal} and R_{th_McL}.

3. Study of thermal resistance variation according to power losses and ambient temperature

In this section, the thermal resistance variation of E/PLT and EE planar cores is studied with CFD simulations.

3.1. Study methodology

For each planar core, CFD simulations are performed according to both parameters:

1. The total losses (P_d) that vary from 1 W to P_{max} (Table 5) by step of 1W;
2. The ambient temperature (T_{amb} that takes discrete values: 20°C, 30°C, 40°C, 50°C and 60°C.

For each simulation, the thermal resistance value (2) is calculated from the extracted maximal temperature (T_{max}), obtained in steady-state:

$$R_{th}(P_d, T_a) = \frac{T_{max} - T_a}{P_d} \quad (2)$$

Each E/PLT and EE core-based planar device is modelled according to their core dimensions [15] and considering the windings' length outside the core to be equal to the width of the winding window. The gaps between windings and magnetic core are set according to dimensions shown in Figure 6.

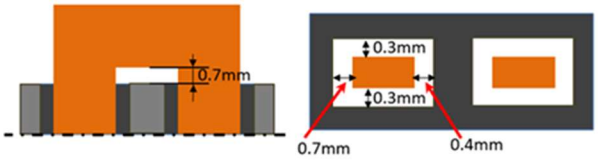


Figure 6. Gaps between winding and magnetic core for CFD simulation

3.2. CFD Simulation parameters

Geometry of the problem is described with Ansys Icepack [17]. Fluent is used to solve the CFD equations. In order to obtain valid results, some modelling parameters need to be set.

As mentioned in section 2.2, planar windings are supposed to be homogeneous and thermal conductivities listed in Table 1 are applied to CFD modeling. Regarding emissivity, ferrite and winding ones are fixed to typical values, 0.9 and 0.45, respectively.

In natural convection, the simulation domain needs to be carefully set. In this study, the domain is filled with air. It needs to be large enough to allow air movement while avoiding reverse flow [21]. Figure 7a and Figure 7b present simulation domain that vary with component's size. Two boundary conditions (BC) are fixed:

1. Temperature of the external area of the domain is fixed to T_a.
2. Air pressure is set to atmospheric pressure: $P_{atm} = 10^5 Pa$

The CFD simulation meshing is a key point of modeling. Indeed, fluid equations are nonlinear and they can lead to convergence difficulties. Here, the mesh is hexahedral (cartesian). Figure 7c and Figure 7d present mesh for both parts of the component: magnetic core (Figure 7c) and winding (Figure 7d). As an example, the size of the mesh is set to 648358 elements for the smallest core (E/PLT32) while it is expanded to 5954862 elements for the biggest one (EE64). Computation time varies from 30 minutes to 4h for one operating point.

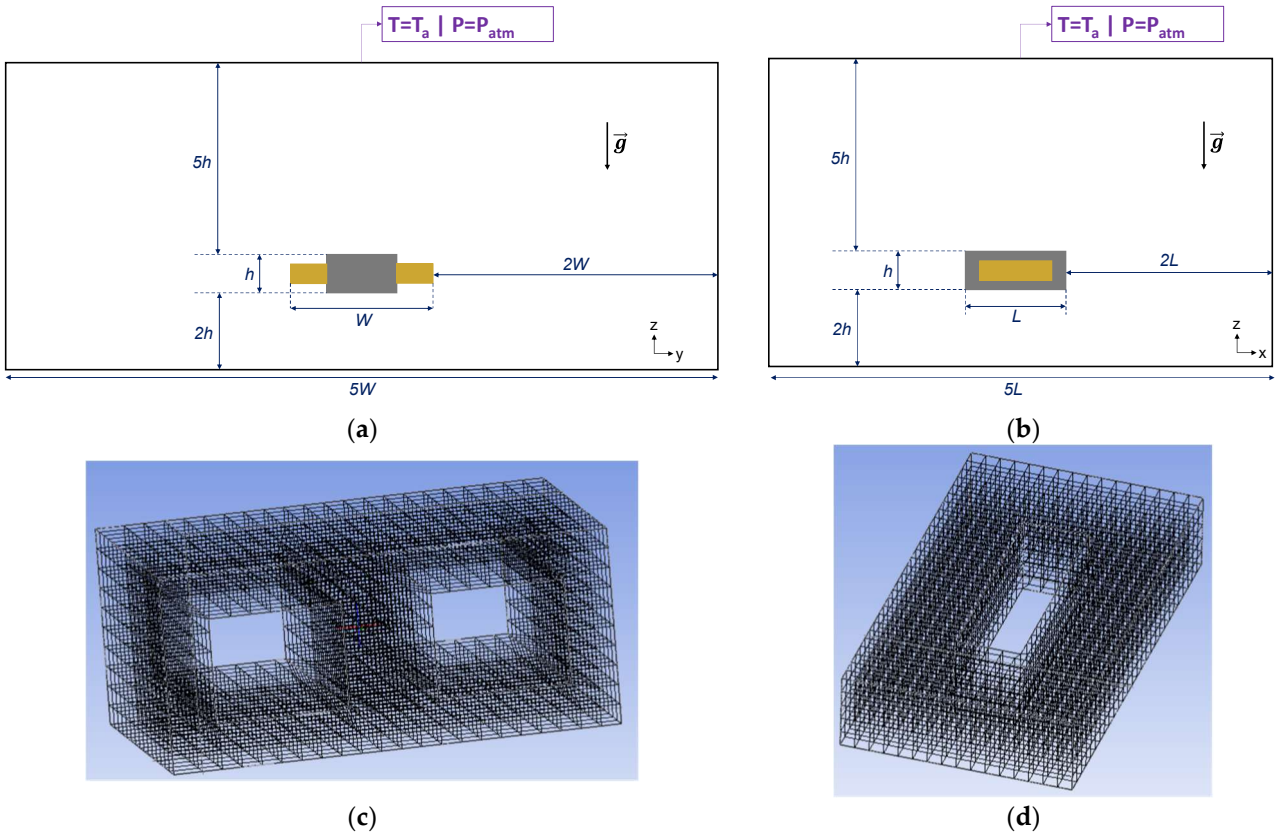


Figure 7. CFD simulation parameters: (**a**) YZ plane simulation domain; (**b**) XZ plane simulation domain; (**c**) Magnetic core meshing; (**d**) Winding meshing.

CFD equations are solved based on finite volume method (FVM) [22]. Figure 8 shows an example of temperature distribution computed for a E/PLT38 core with P_d=6W and T_a=30°C. In this figure, it could be noticed that the air movement is due to temperature gradient. Indeed, the hot air is rising and the cool air is falling. Then, the air above the transformer is hotter and, conversely, the air at the bottom is cooler.

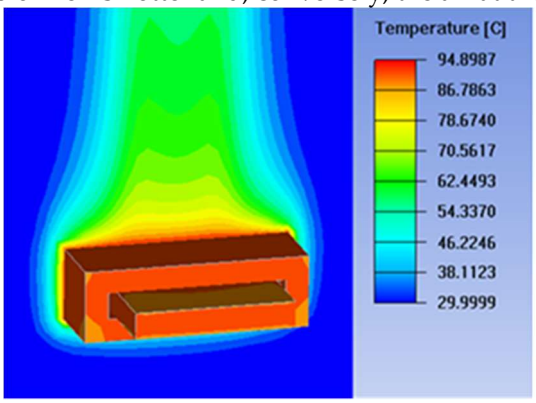


Figure 8. Example of temperature distribution for E/PLT38 (P_d=6W and T_a=30°C)

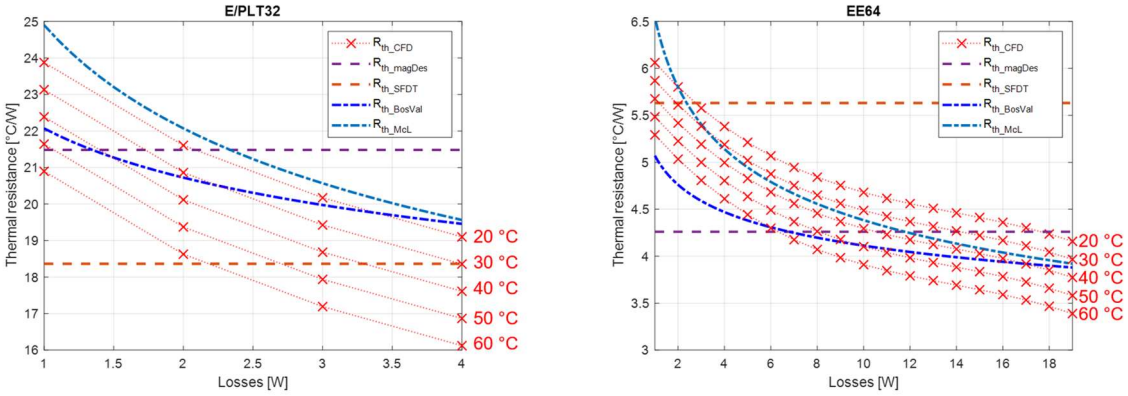
3.3. Results and analysis

Figure 9 presents the thermal resistance variations, obtained with CFD, for both cores E/PLT32 (Figure 9a) and EE64 (Figure 9b). These variations are plotted according to power losses and ambient temperature. As mentioned before, the results are compared to four models from the literature: R_{th_magDes}, R_{th_SFDT}, R_{th_BosVal} and R_{th_McL}.

Looking at the curves, two main comments can be made: The planar component thermal resistances decrease when power losses increase. Their values also decrease with the

rise of the ambient temperature. These comments are the same for all the other size of E/PLT and EE planar cores.

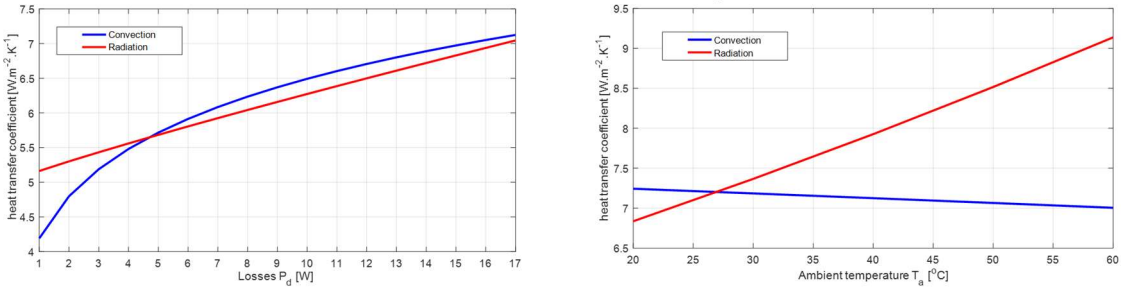
For the E/PLT32 core (Fig.10a), thermal resistance values decrease from 23.8°C/W to 19.1°C/W for 20°C ambient temperature and losses that vary from 1W to 4W. At 60°C, values are between 20.9°C/W and 16.1°C/W. For the EE64 core (Fig.10b), values are much smaller. While losses vary from 1W to 19W, the thermal resistance values decrease from 6°C/W to 4.1°C/W at 20°C. For a 60°C ambient temperature, values are between 5.3°C/W and 3.4°C/W.



(**a**) (**b**)

Figure 9. Variation of thermal resistance according to losses and ambient temperature – CFD results: (**a**) E/PLT32; (**b**) EE64.

In order to explain those variations, the evolution of convection and radiation global heat transfer coefficients, computed for all the external area of the component with losses and ambient temperature, is plotted on Figure 10a and Figure 10b, respectively. From Figure 10a, it can be seen that both heat exchange coefficients increase with losses and so the thermal resistance decrease. For the variation due to the ambient temperature increase (Figure 10b), convection heat exchange coefficient decreases while radiation heat coefficient increase. The latter has a greater slope so the resulting global heat exchange coefficient has a positive slope, increasing with ambient temperature. As a consequence, the thermal resistance also decreases with this parameter.



(**a**) (**b**)

Figure 10. Variation of thermal resistance according to losses and ambient temperature – CFD results: (**a**) E/PLT32; (**b**) EE64.

Comparisons between CFD simulation results and the ones computed from the literature's model (Figure 9) show that values are in the same level of magnitude. However, variations due to the power losses and ambient temperature induce significant differences that can lead to errors in the operating temperature estimation of a real component. If the temperature is underestimated (i.e. thermal resistance is undervalued), an excessive heating can appear inside the component and can cause its destruction. On the opposite side, if the temperature is overestimated (i.e. thermal resistance is overstated), one component's

design can be distorted. As a consequence, some design solutions can be replaced even if it was fully able to endure constraints of the system.

In order to highlight benefits of such thermal resistance model that considers power losses and ambient temperature, the temperature differences obtained with models from the literature and results from CFD based simulations are calculated for each value of power losses (3):

$$T_{diff} = \left(R_{th\_lit} - R_{th\_CFD}\right) \times P_d \quad (3)$$

where R_{th_CFD} the thermal resistance computed with CFD simulations, P_d the power losses and R_{th_lit} the four different resistances from the literature: R_{th_magDes}, R_{th_SFDT}, R_{th_BosVal} and R_{th_McL}.

Temperature differences are displayed in Figure 11 for E/PLT32 and EE64 at 20°C and 60°C, to show under and over estimation of models in comparison with the CFD simulation results. If the temperature difference is negative, models underestimate the component's temperature and if the difference is positive, models overestimate the temperature.

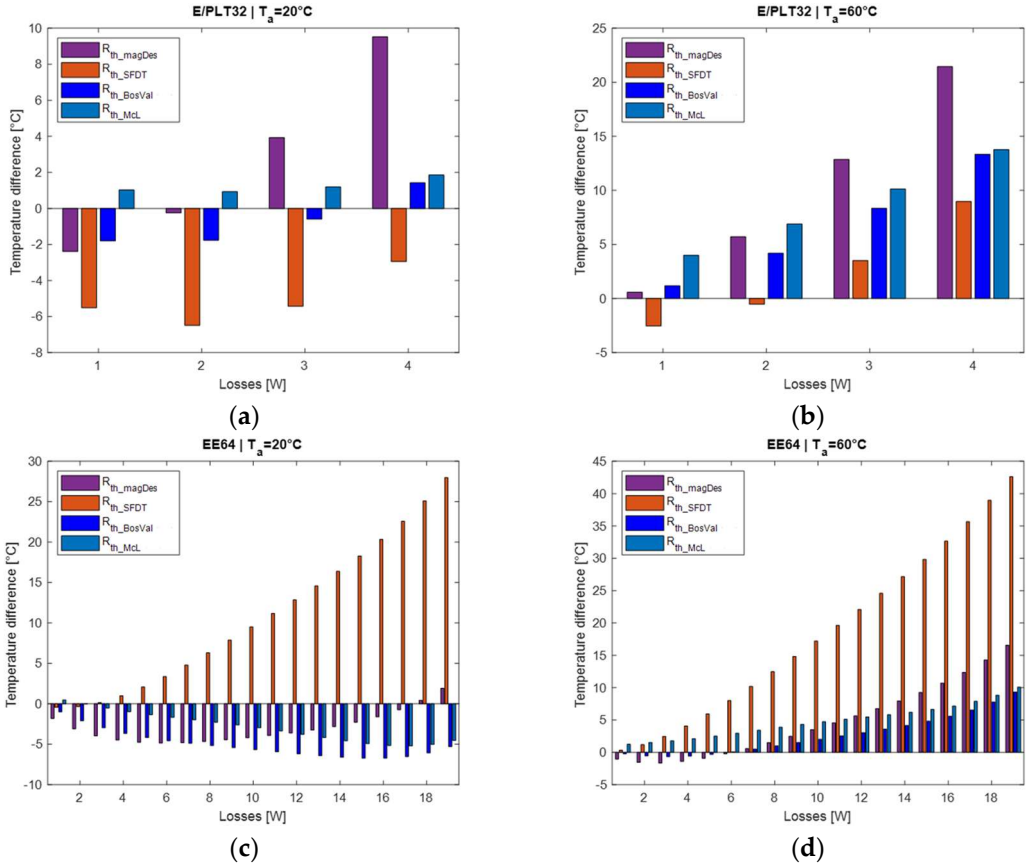


Figure 11. Comparison of temperature estimation difference obtained with CFD simulation and models from the literature: (**a**) E/PLT32 at 20°C; (**b**) E/PLT32 at 60°C; (**c**) EE64 at 20°C; (**d**) EE64 at 60°C.

For a small core (E/PLT32), thermal resistance values are highly disparate. However, due to the small amount of losses, temperature differences are limited. At 20°C (Figure 11a), differences between model and CFD results are limited in the range -6.5°C to 9.2°C. At 60°C (Figure 11b), due to the high decrease of the thermal resistance with the ambient temperature, differences raise to be between -2.5°C and 21.1°C. This increase leads to more significant overestimation. For a big core (EE64), differences between models are smaller but the high level of losses induce more important estimated temperature differences. For

example, at 20°C (Figure 11c), the differences are between -7°C and 27.5°C while, at 60°C (Figure 11d), the differences are included between -1.6°C and 42.1°C.

Generally, constant models (R_{th_magDes}) and R_{th_SFDT}) are close to CFD results but only for a limited power loss variation range. Moreover, the differences increase while the ambient temperature increases. For the two models accounting for power loss variation (R_{th_BosVal} and R_{th_McL}), the ambient temperature's change induces more important errors in temperature's estimation.

This analysis clearly shows the benefits of using a more precise thermal resistance model accounting for power losses and ambient temperature. As it is shown in Figure 9, the latter parameter has a non-negligible impact and can lead to significant overestimation in planar magnetic design. With such model accounting for losses and temperature, the design of a planar component can be done more precisely avoiding potential destruction of the component if the temperature is underestimated and over-sizing of components in order to endure constraint of the power converter and its environment.

4. Analytical modelling of thermal resistance's variation

In a planar component design process, the use of complex and time consuming CFD simulations might be problematic. Analytical modeling is generally preferred in order to have fast results, more suitable with design and optimization tasks. For designers, considering the variation of thermal resistance according to power losses and ambient temperature is a major step toward optimized planar components.

In order to make it easy and fast for engineers in their planar components' developments, an analytical modelling of the thermal resistance variation is developed for all the E/PLT and EE planar cores, based on these CFD results.

To model the variation of the thermal resistance according to power losses and ambient temperature, a polynomial equation is adopted (4):

$$R_{th}(P_d, T_a) = a_3 {P_d}^3 + a_2 {P_d}^2 + a_1 P_d + b T_a + c \quad (4)$$

where a_3, a_2, a_1, b, and c are the coefficients to be identified.

Coefficients for each planar E/PLT and EE cores are determined from CFD results using regression with least squares method [23]. The obtained coefficients are listed in Table 6 for the E/PLT cores and in Table 7 for the EE ones. For the different cores, this polynomial modeling is restricted to:

- Power range: $P_d \in [1W; P_{max}]$ (Table 5);
- Ambient temperature: $T_a \in [20°C; 60°C]$.

Table 6. Coefficients for E/PLT cores.

Size	a_3	a_2	a_1	b	c
E/PLT32	-0.0785	0.8908	-4.379	-0.0744	28.943
E/PLT38	-0.0232	0.3585	-2.306	-0.0527	18.942
E/PLT43	-0.0129	0.225	-1.618	-0.0437	16.019
E/PLT58	-0.00164	0.0486	-0.5765	-0.0268	9.335
E/PLT64	-0.00066	0.0251	-0.3761	-0.0219	7.558

Table 7. Coefficients for EE cores.

Size	a_3	a_2	a_1	b	c
EE32	-0.0317	0.4889	-3.125	-0.0604	24.815
EE38	-0.0146	0.2537	-1.8109	-0.0448	17.146
EE43	-0.00642	0.1376	-1.189	-0.036	13.563
EE58	-0.00087	0.0309	-0.4331	-0.0223	7.977
EE64	-0.00045	0.0191	-0.312	-0.0192	6.7406

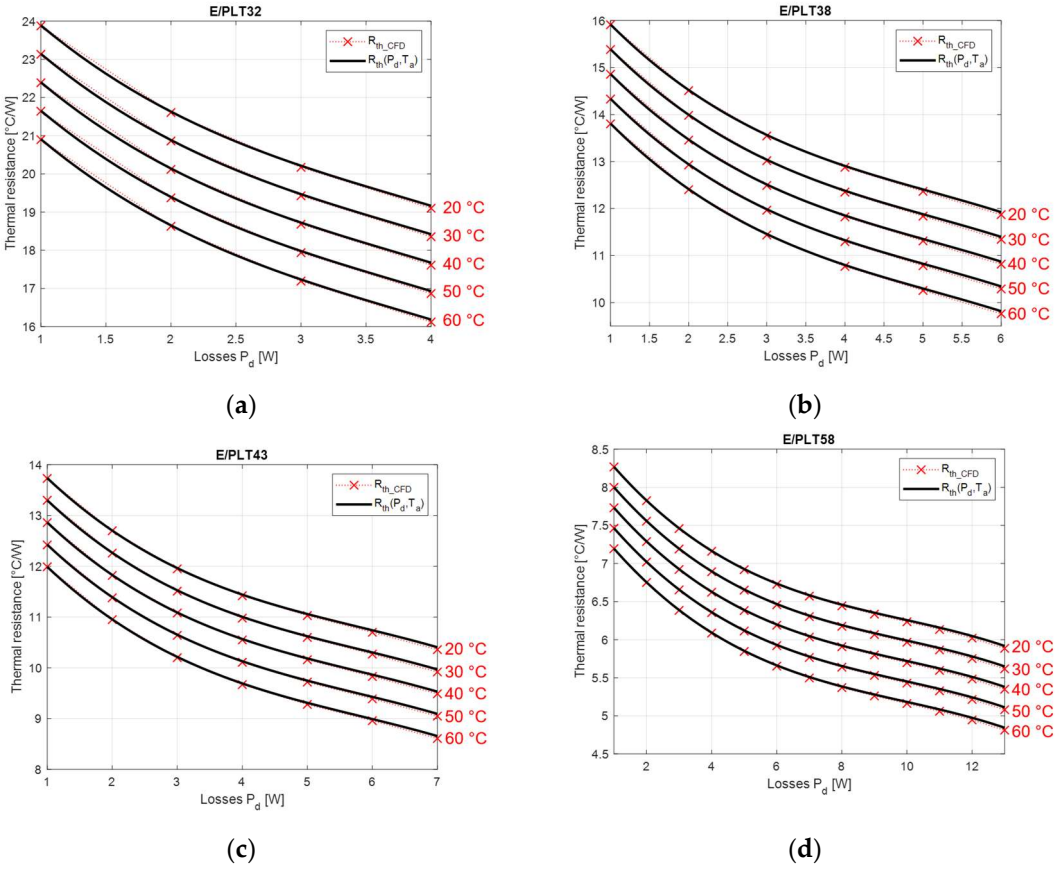
In both tables, the b coefficient is negative that is consistent with the drop of thermal resistance with the ambient temperature. Moreover, odd coefficients a_3 and a_1 also have negative values in order to ensure decrease of thermal resistance with power losses.

5. Validation and discussion

In this section, the analytical modeling is compared to the CFD simulation results and measurement on a 360VA E/PLT38 core based planar transformer. Then, the results are discussed to highlight the benefits of using such model in a design stage and also its limitations.

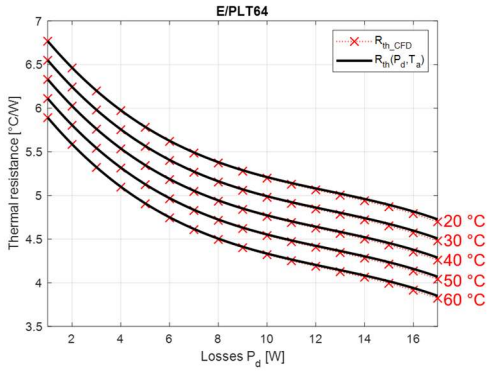
5.1. Comparison with CFD simulation results

Thermal resistances calculated with polynomial formula (4) are compared to results from CFD simulations in Figure 12 and Figure 13 for E/PLT and EE cores, respectively. Analytical formulation correctly reproduces variations of thermal resistances for all the sizes of E/PLT and EE planar cores. Maximal error doesn't go beyond 1% inside the loss and temperature ranges.



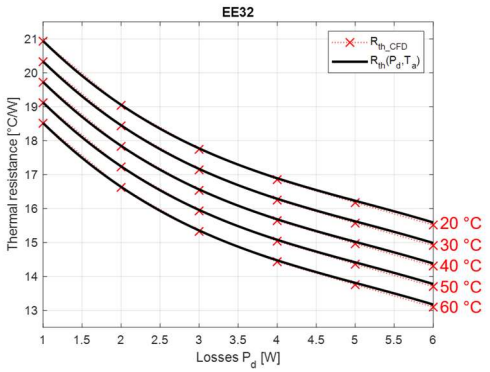
(**a**) (**b**)

(**c**) (**d**)

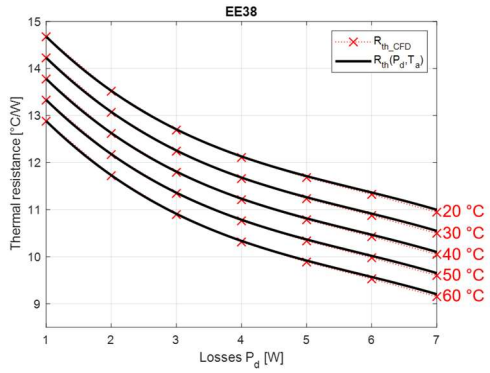


(**e**)

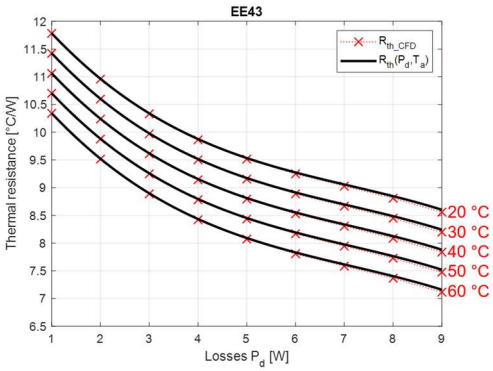
Figure 12. Comparison of thermal resistance variation: Analytical model vs CFD for E/PLT cores: (**a**) E/PLT32; (**b**) E/PLT38; (**c**) E/PLT43; (**d**) E/PLT58; (**e**) E/PLT63.



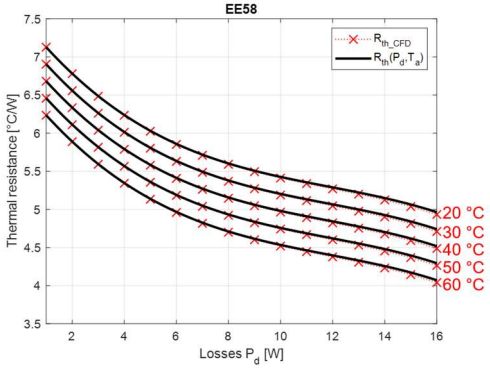
(**a**)



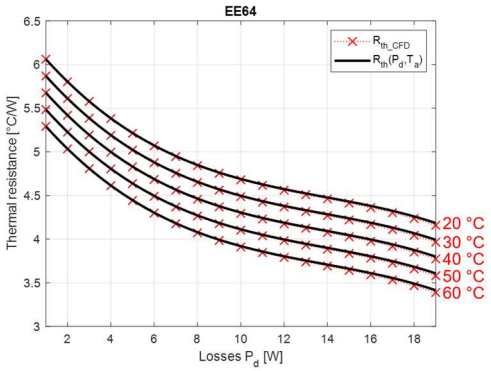
(**b**)



(**c**)



(**d**)



(**e**)

Figure 13. Comparison of thermal resistance variation: Analytical model vs CFD for EE cores: (**a**) EE32; (**b**) EE38; (**c**) EE43; (**d**) EE58; (**e**) EE63.

5.2. Experimental validation

In order to validate the thermal resistance model, a prototype of planar transformer based on E/PLT38 core 3F3 magnetic material is developed. The prototype is designed for 360VA. The nominal voltage at primary winding is 40V and its operating frequency is 100kHz. Its maximum losses are 6W.

The prototype is a two winding transformer made of 12 copper layers separated by Kapton layers as insulator. The six first layers form the three turns of primary winding (two parallel layers by turn) while the six other layers are all parallelized to form the secondary winding. The design of this prototype is presented in [24].

For testing validity of the thermal resistance model, the losses inside the component need to vary from 1W to its maximal power (Table 5). In order to generate different loss values, the transformer prototype is tested with secondary in open circuit. In this configuration, losses are mainly core ones. They can be tuned by acting on the sinusoidal voltage (V_p) and its frequency (f) at the primary winding, as is shown in Steinmetz model [25]. In power converters, voltages and currents are usually non-sinusoidal. In this case, other models must be considered to compute the core losses. The Revised Generalized Steinmetz Model (RGSE) is one of the most accurate models and can consider a DC offset in the case of HF inductors [26,27].

$$P_{core} = \left(\frac{k_c (c_2 T^2 + c_1 T^2 + c_0)}{4.44\, S_c\, N_p} f^{\alpha-\beta}\, {V_p}^{\beta} \right) V_e \quad (5)$$

where k_c, c_0, c_1, c_2, α and β are coefficients given by manufacturer [10], T is the core temperature, V_e is the effective volume of the core, S_c is the cross-sectional area of the core.

In practice, these both parameters are useful for tuning the loss values. The voltage parameter is set to tune the main power while the frequency parameter is used to adjust the desired value.

Figure 14 presents the principle and the equipment for the thermal resistance variation measurements. The sinusoidal voltage is generated by Function Waveform Generator Agilent 33250A [28]. The signal is amplified with power amplifier 75A250A [29]. Losses are evaluated with oscilloscope (Tektronix DPO 4034 [30]) measurements. In order to accurately estimate those losses inside planar transformer, probes need to generate very small delays [31]. Current in primary winding is measured with LEM PR50 current probe [32] while voltage's measurement is achieved with Tektronix P5100A voltage probe [33]. These probes have a bandwidth of 50 MHz and 500 MHz respectively. They are large enough to observe fundamental and predominant harmonics. With these probes, delay is

below 9 ns and the measurement error is below 7% for a 40V-100 kHz frequency voltage excitation applied to the planar device.

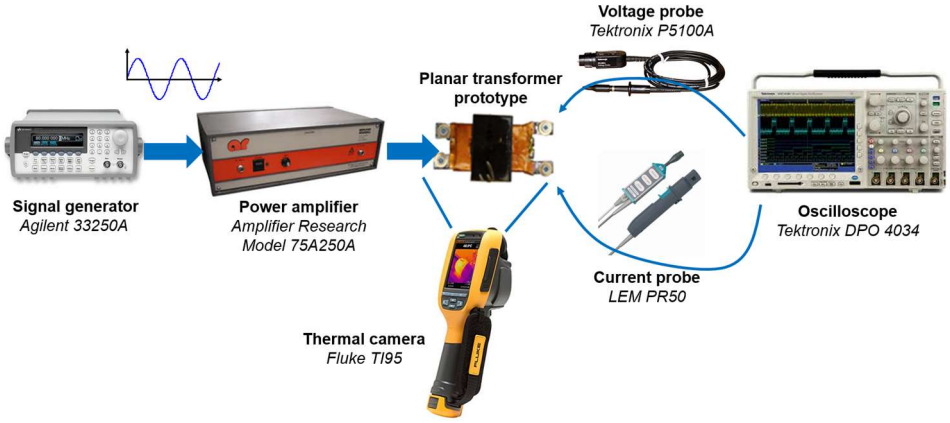


Figure 14. Principle and measurement equipment for the experimental characterization of the thermal resistance variation

Temperatures are measured with a thermal camera Fluke TI95 [34]. That camera has a tunable emissivity and a sensitivity of 0.1°C between 25 and 30°C. The thermal camera was first calibrated using thermocouples in order to tune the emissivity values. The emissivities of 0.9 and 0.45 for the magnetic core and the winding were confirmed.

Six tests are performed with various power values (1W, 2W, 3W, 4W, 5W and 6W) for two different ambient temperature values (22°C and 30 °C). Thermal resistance is then extracted from the maximal measured temperature of the component according to (3), considering the measured power and the ambient temperature. Figure 15 shows an example of thermal image obtained for 6W loss and 22°C ambient temperature. The obtained temperature is quite homogenous on the core's surface. The maximal temperature is located on the top area of the magnetic core because losses are located inside the core.

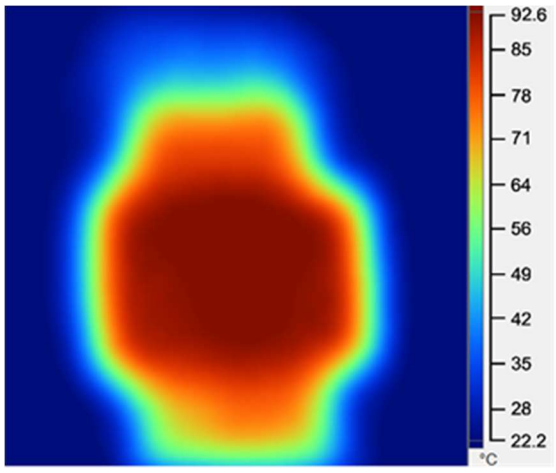
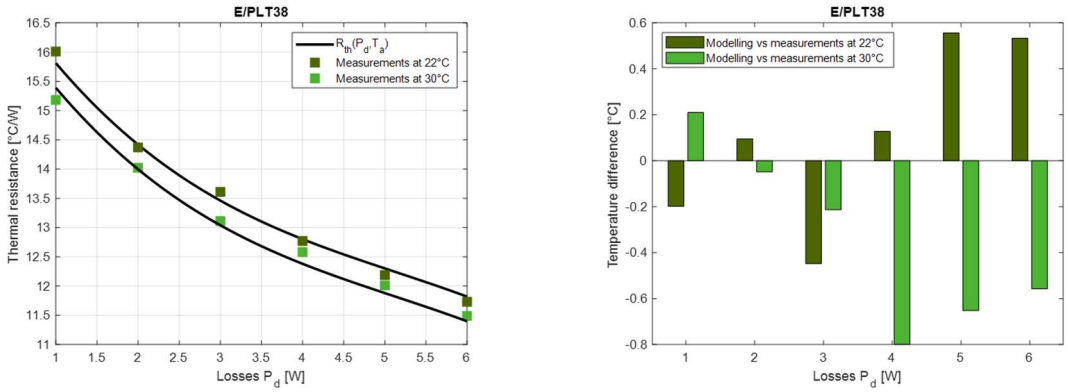


Figure 15. Thermal image of for E/PLT38 core (6W losses and 22°C ambient temperature)

Figure 16a presents the comparison between the thermal resistances evaluated with these tests and the ones calculated with the analytical modelling (4). The temperature differences (6) obtained with the modelling and the measurements are plotted on Figure 16b:

$$T_{diff} = \left(R_{th}(P_d, T_a) - R_{th\_meas}\right) \times P_d \quad (6)$$

where $R_{th}(P_d, T_a)$ the thermal resistance calculated with the model, P_d the power losses and R_{th_meas} the thermal resistance measured.



(**a**) (**b**)

Figure 16. Comparison of analytical modelling and experimental measurements for E/PLT38 core: (**a**) Thermal resistance; (**b**) Temperature difference.

The experimental results of thermal resistance are consistent with CFD results and its analytical modelling. The test configuration with only core losses does not affect the results. Indeed, the loss distribution (i.e. only copper losses or shared between core and winding) does not bring significant difference on the maximal temperature. The difference is below 3°C.

As expected, thermal resistances decrease with ambient temperature and power losses. The maximum difference between thermal resistance from measurements and the analytical calculation is approximatively 3%.

5.3. Discussion

The developed model is easy to use and it does not need important processing power. It enables a fairly sizing of planar magnetics in natural convection with no heatsink. It can also be included is optimization process. Similar models could be developed for other planar cores (ER, EQ) or other customized cores with low profiles.

However, such model is limited to design stage. Indeed, the latter does not permit to obtain temperature distribution inside the component. Hot spots inside windings or magnetic core cannot be considered. To address this issue, more complex model can be used in 2D [35-37], in 3D [24], [38] or with FEA based modelling [39-41].

Other models based on Artificial Intelligence (AI) [42-44] can also be used to accurately estimate temperature distribution. Indeed, AI is a promising tool, especially suitable for the design of HF magnetic components and their thermal management [44]. For example, AI models can lead to more efficient thermal management and automatic heatsink design, as it was developed, in [45], for the heatsink optimization of air-cooled power modules. AI-based models are fast but their development needs a lot of data and cannot be used in a simple computation tool.

6. Conclusions

In this paper, a thermal sizing model for planar magnetics is developed. Based on CFD simulation, a global thermal resistance is computed in natural convection with no heatsink. The variation of this resistance is tested according to two parameters: the power losses inside the planar component and the ambient temperature. Thermal resistance values of EE and E/PLT core based planar transformer are computed and compared to models from the literature, in order to highlight benefits of such model.

Then, an analytical modelling considering both parameters (i.e power losses and ambient temperature) is developed based on polynomial equation. This analytical model is compared with CFD results. Finally, the thermal resistance model is also compared to measurement on a 360VA planar transformer prototype.

Such a model can be very useful for designers. It enables to precisely calculate the increase of temperature, avoiding problems linked to underestimation or over-sizing of magnetic components. The developed model is very fast and can enable to explore planar component design solutions in a design process. It can also be used in an optimization process, combined with other analytical models.

The methodology developed in this paper can be extended to other planar core geometries, such as ER or EQ ones. Some investigation must be done to validate the adaptation of such a polynomial model for these geometries.

The future developments of AI approaches should enable to improve the thermal design of HF magnetics. Such AI-based design will provide solutions that will enhance the performances of planar components and their integration into power converters.

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