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Wireless Powering Efficiency of Deep-Body Implantable Devices

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Abstract—The wireless power transfer (WPT) efficiency to implanted bioelectronic devices is constrained by several frequency-dependent physical mechanisms. Recent works have developed several mathematical formulations to understand these mechanisms and predict the optimal operating conditions. However, the existing approaches rely on simplified body models, which are unable to capture important aspects of WPT. Therefore, this article proposes the efficiency analysis approach in anatomical models that can provide insightful information on achieving the optimum operation conditions. First, this approach is validated with a theoretical spherical wave expansion (SWE) analysis, and the results for a simplified spherical model and a human pectoral model are compared. The results show that although a magnetic receiver outperforms an electric one for near-field operation and both the sources could be equally use in the far-field range, it is in the mid-field that the maximum efficiency is achieved with an optimum frequency between 1 and 5 GHz depending on the implantation depth. The receiver orientation is another factor that affects the efficiency, with a maximum difference between the best and worst case scenarios around five times for the electric source and over 13 times for the magnetic one. This approach is used to analyze the case of a deep-implanted pacemaker wirelessly powered by an on-body transmitter and subjected to stochastic misalignments. We evaluate the efficiency and exposure, and we demonstrate how a buffered transmitter can be tailored to achieve maximum powering efficiency. Finally, design guidelines that lead to optimal implantable WPT systems are established from the results obtained with the proposed approach.

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Index Terms—Biomedical electronics, implantable devices, pacemakers, radiation efficiency, wireless power transfer (WPT).

I. INTRODUCTION

WIRELESS power transfer (WPT) has been the subject of many works and publications mainly due to its technological and commercial appeal. It was founded in the works of Nikola Tesla, who first proposed the use of electromagnetic waves to wirelessly power electric devices. Even though the theoretical aspects have been studied throughout the years and are well-consolidated, the physical realization and the proposition of different techniques for its application have seen renewed interest with the rise of portable electronic devices [1].

One way to classify the WPT techniques that use electromagnetic waves as the energy carrier is by the radiation region that comprises the distance between the transmitter and the receiver. For instance, the near-field techniques are based on the near-field coupling between antennas that can be either inductive or capacitive [2].

Consequently, due to the short distance between antennas, these techniques can achieve high efficiency, and they are able to deliver high power levels [3]. This efficiency can be even further increased by electromagnetic resonance [4]. On the other side, the radiative or far-field techniques can cover a wide distance range with the drawback of lower efficiency. Therefore, they usually use highly directive antennas to reduce the power dispersed in free space and thus increase the received power [5]. A new mid-field WPT technique has been proposed to achieve higher efficiency than the far-field techniques and larger distance ranges than their near-field counterparts. In the mid-field WPT, the distance between the transmitter and the receiver is in the order of a wavelength, and, in this case, the electromagnetic fields are composed of reactive and propagating components [6], [7].

In the context of biomedical engineering, the application of WPT for implantable bioelectronic and biosensor devices is envisaged to monitor physiological processes [8], drug delivery [9], and organ stimulation through electric signals [10], to name a few. Therefore, different WPT techniques have already been applied for wireless powering bioelectronic implants [11]. For instance, near-field WPT is used for subcutaneous pacemakers [12], [13], [14], neural and spinal

cord stimulators [15], [16], [17], cochlear [18], and ocular implants [19], among other. All these applications share the same characteristic of having a small implantation depth. Conversely, far-field techniques are used for ultralow-power implants usually applied for biotelemetry [8]. However, for powering deep-implanted devices, the mid-field WPT is mostly used. For example, it has been applied for cardiac implants and pacemakers [20], [21], [22], gastrointestinal endoscopy capsules [23], [24], and neural implants [25].

Several physical, technical, and legal aspects impose limitations on the in-body WPT application. First, the body tissues are composed of dynamic, highly heterogeneous, dispersive, and lossy media that deteriorate the efficiency of WPT techniques which in other applications present a reasonable efficiency. The two prominent factors that reduce WPT efficiency are the electromagnetic wave attenuation in these lossy tissues, which increases with the operating frequency, and the reflection at the interface between different media [26]. Moreover, the miniaturized implantable receivers are usually both physically and electrically small, further reducing the maximum achievable efficiencies [27], not to mention other sources of losses such as impedance mismatching, misalignments, and internal resonances in the body organs. Another major concern is the human body exposure to electromagnetic fields, which must comply with regulatory limits for human use [28]. Therefore, the WPT system parameters—such as operating frequency, nature of the source, and implantation depth—must be judiciously chosen to achieve the highest efficiency possible, taking into account the exposure-level regulations.

Several models have been proposed to mathematically assess the maximum radiation efficiency and optimal frequency for implantable bioelectronic devices. Simplified analytical models can help making conclusions about the optimal parameters of the system independently of the source and receiver design [29]—these conclusions are difficult to make with the 3-D full-wave simulations because it cannot search through the entire design space. The planar stratified heterogeneous model [30], [31] is a simple approach that allows an analytical formulation that includes the wave reflection between different layers. In this model, the equivalence principle replaces a volumetric surface current distribution (SCD) for an in-plane electric current density source that produces the same electromagnetic fields. Although this model is mathematically more straightforward and provides physical insight of the problem under analysis, it considers the human body as planar and infinite media. Therefore, it disregards the effects of the human body's shape and dimensions on radiation performance. Besides, the assumption of an infinite medium may lead to inaccuracies in the maximum efficiency prediction.

On the other hand, the spherical wave expansion (SWE) [32], [33], [34] is a semi-analytical approach that represents the human body as a spherical model composed of a homogeneous or concentric multilayered medium. In this case, the source is represented by an electric or magnetic dipole encapsulated by a small sphere positioned anywhere inside the spherical phantom. Then, the electric and magnetic

fields are decomposed in vector spherical harmonics, and, from orthogonality relationships, the problem is mathematically solved by a linear system. From the computational point of view, this approach is less costly than a full-wave analysis and can lead to insightful results once the implantation depth mainly influences the level of achievable power density just outside the body. Furthermore, due to the high electric permittivity of the biological tissues, the near-field region is shorter than in free space; therefore, the radiation pattern of mm-sized implantable antennas is less sensitive to the shape of the phantom itself [34]. However, this approach is difficult to implement for more complex sources and realistic body models. Apart from that, the standing wave pattern in spherical models differs from the anatomical-shaped ones. Therefore, this difference is also verified in the WPT efficiency values obtained with both the phantoms. For this intent, a full-wave computation needs to be carried out to solve the inhomogeneous wave equation numerically given an arbitrary finite-sized source [27].

This work aims to investigate the electromagnetic energy exchange between an optimal on-body transmitter and an implantable receiver, as well as to analyze the influence of the system's parameters on WPT efficiency. We develop a general 2-D-axisymmetric (2-DA) full-wave approach, providing the best case scenario for the energy transfer efficiency as a function of frequency, implantation depth, and nature of the receiver, i.e., electric or magnetic. The basis for this problem formulation and some results for a simplified spherical phantom model have been presented in [35]. However, the proposed approach is further extended and validated with a theoretical model based on SWE in this article. Then, both the methods are used to evaluate the frequency-dependent radiation efficiency for several implantation depths considering electric and magnetic receivers, and these results surpass the efficiency levels previously presented in the literature with other approaches.

Previous studies on modeling electromagnetic wave propagation in the human body mainly focused on wireless communications with implantable antennas [33], [36], medical treatments based on electromagnetic waves such as hyperthermia [37], [38], [39], [40], or dosimetry [41]. However, the investigation of wave propagation for WPT applications [20], [30] involves a specific focus on the electromagnetic interaction between an on-body transmitter and an in-body receiver. Therefore, the optimal operating conditions identified for in-body biotelemetry and hyperthermia applications might differ. Specifically, for the in-body biotelemetry, the goal is to maximize the omnidirectional radiation performance through the high-contrast tissue-air interface [26]. For hyperthermia, the main objective is to control the local and nonlinear [i.e., $\hat{\epsilon}(\mathbf{E})$] absorption of energy close to the source [38]. As a result, most deep-body implantable devices operate in the MedRadio band (401–457 MHz) [42]; the optimal band for hyperthermia is between 130 and 500 MHz [43], whereas for WPT, the maximum efficiency is achieved around 1–3 GHz [30], [31], [35], [44]. This work studies the electromagnetic exchange in an in-/on-body WPT system, derives, and demonstrates the optimal operating conditions in terms of efficiency and

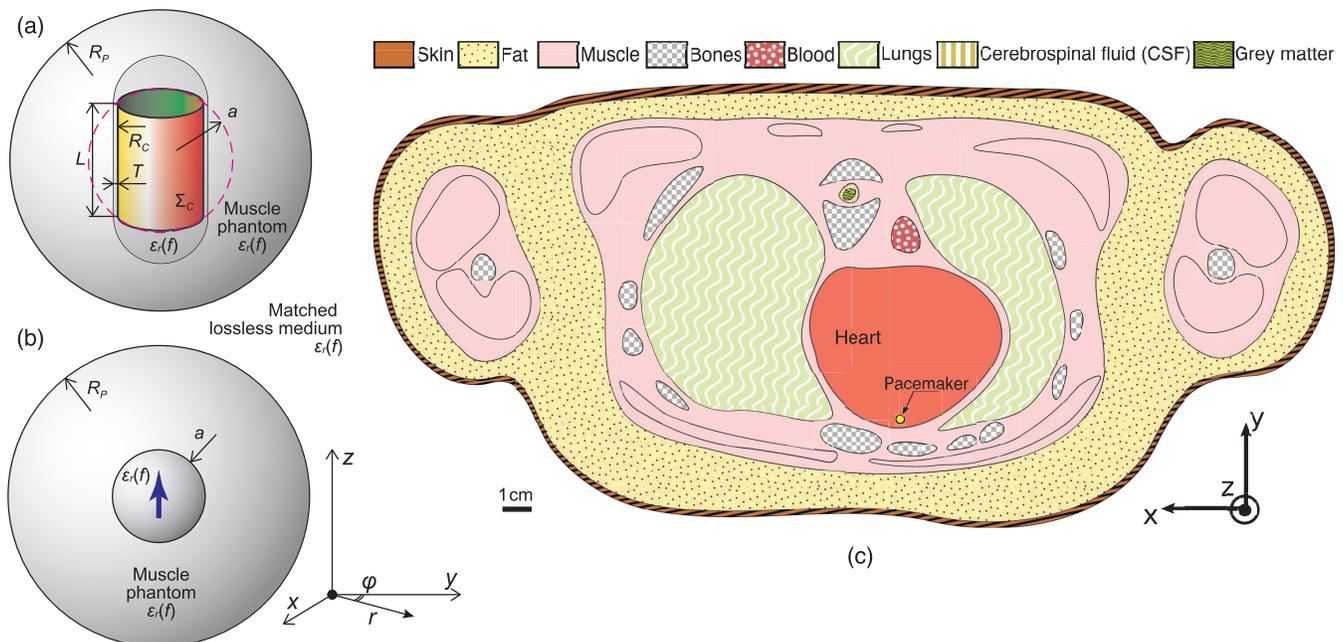


Fig. 1. Geometrical representation of the problem under analysis. (a) and (b) Simplified spherical model (not to scale). A muscle-equivalent spherical phantom with radius R_p and dispersive complex permittivity $\hat{\epsilon}_r(f)$, surrounded by a lossless matched medium with $\epsilon_r(f)$, encloses the implant. Both (a) and (b) share the same axis and are surrounded by the same matched medium. For (a) 2-DA model, this implant is insulated by a capsule-shaped volume with $\epsilon_r(f)$ and the receiving electric or magnetic antenna is modeled as their corresponding current distribution \mathbf{J}_s on the cylindrical aperture, whereas for (b) SWE model, the source is a lossless bubble with $\epsilon_r(f)$ and radius a , and the receiver is an elementary electric or magnetic dipole. (c) Anatomical 2-D model of a human pectoral region comprising nine dispersive tissues. An on-body source represents the transmitter, and the receiver is a deep-tissue pacemaker implanted inside the heart at a depth of 37 mm from the closest skin interface and filled by a lossless dielectric with $\epsilon_r(f)$, matched to the wave impedance in the myocardium.

exposure as a function of implantation depth and nature of the power source antenna.

Moreover, this study applies for the first time the 2-DA full-wave formulation to assess the WPT efficiency in an anatomical scenario considering a deep-implanted mm-sized pacemaker in a transverse cut model for the human pectoral. The proposed approach has the advantage of taking into account the complexities of the human body regarding its shape, dimensions, and electromagnetic heterogeneity, being less computationally costly than a tridimensional full-wave analysis. In this way, it is possible to analyze the real-life application of WPT for powering a cardiac stimulator as presented in [20]. In addition, different configurations for electric and magnetic on-body sources are investigated, and the results for the anatomical model are compared with the simplified spherical phantom. Finally, the origin for the losses is discussed from these results, and ways to mitigate them and achieve maximum efficiency are investigated from the parametric analysis of the on-body transmitter that wirelessly powers the implanted pacemaker.

II. EFFICIENCY ANALYSIS WITH SIMPLIFIED SPHERICAL MODELS

The problem under analysis consists of a WPT system composed of an implantable bioelectronic device that acts as a receiver and a transmitter structure conformal to the surface of the body. To determine the achievable WPT efficiency, the human body is modeled as a dispersive homogeneous spherical phantom of radius R_p with complex permittivity

$\hat{\epsilon}_r(f)$ equivalent to the human muscle tissue [45], as shown in Fig. 1(a). The phantom radius R_p is directly related to the implantation depth, and its evaluated range embraces most deep-body implantable WPT applications. Inside this phantom, the implantable device is represented as a lossless $\epsilon_r(f)$ capsule-shaped volume that is matched to the wave impedance in the surrounding tissue and has length L and radius R_c . This spherical model allows the results obtained with the proposed approach be compared with the semi-analytical solutions based on SWE. In addition, this simplified model disregards the shape complexities and heterogeneities leading to more general results that are better suitable for an initial analysis of implantable WPT systems.

To eliminate losses due to reflection at the interface between the body and the external medium and thereby ensure the maximum WPT efficiency, the permittivity of the region around the phantom is considered as the real part of $\hat{\epsilon}_r(f)$, i.e., the external medium is lossless $\epsilon_r(f)$ and matched to the wave impedance in the muscle. In this way, the on-body transmitter is well-matched to the tissue, which can be physically realized using a high dielectric constant layer. This model disregards any impedance mismatching in the antennas and any system-level losses in electronic circuitry.

To mathematically formulate the problem, an equivalent problem can be proposed based on reciprocity [46]. For this intent, the radiation source is modeled as the electric current density distribution \mathbf{J}_s inside the phantom, as indicated in Fig. 1(a). The reciprocity principle can be applied since the medium is assumed linear. Consequently, the radiated fields

induce a power flow in the lossy phantom and, from energy conservation, the transmitted power P_t is given by

$$P_t = P_r + P_d + i2\omega(\overline{W_m} - \overline{W_e}) \quad (1)$$

where P_r and P_d are, respectively, the received and dissipated powers, and $\overline{W_m}$ and $\overline{W_e}$ are the time-averaged magnetic and electric energies, respectively.

From the time-harmonic electric \mathbf{E} and magnetic \mathbf{H} fields, as well as the source electric \mathbf{J}_s and magnetic \mathbf{M}_s current densities, each one of the total power components can be calculated as follows:

$$P_t = \oint_{\Omega_s} \left(\frac{1}{2} \mathbf{E} \times \mathbf{H}^* \right) \cdot d\mathbf{s} \quad (2a)$$

$$P_r = \oint_{\Omega_p} \left(\frac{1}{2} \mathbf{E} \times \mathbf{H}^* \right) \cdot d\mathbf{s} \quad (2b)$$

$$P_d = \frac{1}{2} \int_{\Omega_p} \sigma |\mathbf{E}|^2 dv \quad (2c)$$

where σ is the phantom's electric conductivity which is related to the imaginary part of the phantom's complex permittivity $\Im[\hat{\epsilon}_r(f)]$ through $\sigma(f) = 2\pi\epsilon_0 f \Im[\hat{\epsilon}_r(f)]$. The integration domains Ω_s and Ω_p indicate that the integral is performed on the surface of the source and the phantom, respectively. Besides, the integrals (2a)–(2c) can be considerably simplified due to the problem's axial symmetry. Finally, the WPT efficiency η is defined as

$$\eta \equiv \frac{\Re(P_r)}{\Re(P_t)} = 1 - \frac{\Re(P_d)}{\Re(P_t)} \quad (3)$$

with \Re being the real part of the complex variable inside the brackets.

Hereafter, the implantable bioelectronic device is referred to as the receiver antenna, whereas the transmitter antenna is the radiating on-body structure.

A. Full-Wave 2-DA Analysis

To numerically evaluate the WPT efficiency using the proposed approach, this model was implemented using the full-wave 2-DA formulation available in COMSOL Multiphysics (assuming no variation in the fields in the φ direction). The electric and magnetic sources with size $L = 1$ cm and $R_c = L/3$ are considered in this computation, which corresponds to the standard encapsulation size used for implantable and ingestible bioelectronic devices [42]. Each source is represented by the electric $\mathbf{J}_s^E(r, \varphi, z)$ and magnetic $\mathbf{J}_s^H(r, \varphi, z)$ surface current densities given by [27]

$$\mathbf{J}_s^E = \left[0, 0, \cos\left(\frac{\pi z}{L}\right) \right] \quad (4a)$$

$$\mathbf{J}_s^H = [0, 1, 0]. \quad (4b)$$

Then, the WPT efficiency in (3) can be calculated from the evaluated integrals in (2a)–(2c).

B. SWE Analysis

The results from a semi-analytical approach based on spherical wave modal expansion are used as a reference to validate the proposed model. In this model depicted in Fig. 1(b), the

electromagnetic fields \mathbf{E} and \mathbf{H} in a spherical structure free of charges can be expressed using vector spherical harmonics \mathbf{M} and \mathbf{N} [46]

$$\begin{Bmatrix} \mathbf{E} \\ -i\eta\mathbf{H} \end{Bmatrix} = \sum_{n,m} a_{mn} \begin{Bmatrix} \mathbf{M}_{mn} \\ \mathbf{N}_{mn} \end{Bmatrix} + b_{mn} \begin{Bmatrix} \mathbf{N}_{mn} \\ \mathbf{M}_{mn} \end{Bmatrix} \quad (5)$$

with

$$\mathbf{M}_{mn} = \nabla \times \mathbf{r}\psi_{mn} \quad (6a)$$

$$\mathbf{N}_{mn} = \frac{1}{k} \nabla \times \nabla \times \mathbf{r}\psi_{mn} \quad (6b)$$

where k denotes the wavenumber of the considered media, \mathbf{r} is the unit position vector in the r -direction, and ψ_{mn} is the solution to the Helmholtz differential equation

$$\psi_{mn} = \frac{1}{kr} Z_n(kr) P_n^m(\cos\theta) e^{im\varphi}. \quad (7)$$

The Schelkunoff-type spherical Bessel or Hankel functions are denoted by Z_n , whereas P_n^m are the associated Legendre functions of the first kind [47]. From the orthogonality relationships for spherical harmonics, (5) becomes a linear system whose solution provides the modal representation for the electromagnetic fields. More details about this implementation can be found in [33].

The integrals in (2a)–(2c) can be evaluated from the spherical model coefficients and vectors and, thus, the efficiency can be obtained through (3). This theoretical approach can also be applied to off-centered sources [32], [33].

C. Experimental Validation

To experimentally evaluate the WPT efficiency of devices deeply implanted in lossy media, the measurement setup described in Fig. 2 is proposed. It consists of a transmitter positioned on the outside wall of a cubic glass tank filled with water. The choice of water as the medium for the measurements is based on the fact that its dielectric properties are well-characterized across all the analyzed frequency bands; therefore, it is best suitable for validating the proposed approach. In contrast, the receiver is placed inside the tank at a distance d from the transmitter, with aligned polarization. For these measurements, two kinds of transmitters were used: 1) a dipole and 2) a loop antenna with the dimensions shown in Fig. 2(b) and (c), respectively. On the other side, the receiver design is described in [44]. The results obtained with this experiment setup are expected to be representative of wirelessly powered devices implanted in biological media primarily composed of soft human tissues. At the same time, the glass permittivity can numerically approximate those of hard tissues.

The scattering parameters were measured using a two-port vector network analyzer (VNA) calibrated in the frequency range from 100 MHz to 5 GHz, in which the transmitter was connected to port 1 and the receiver to port 2. Based on these measurements, the WPT efficiency η can be calculated as

$$\eta = \frac{|S_{21}|^2}{1 - |S_{11}|^2} \quad (8)$$

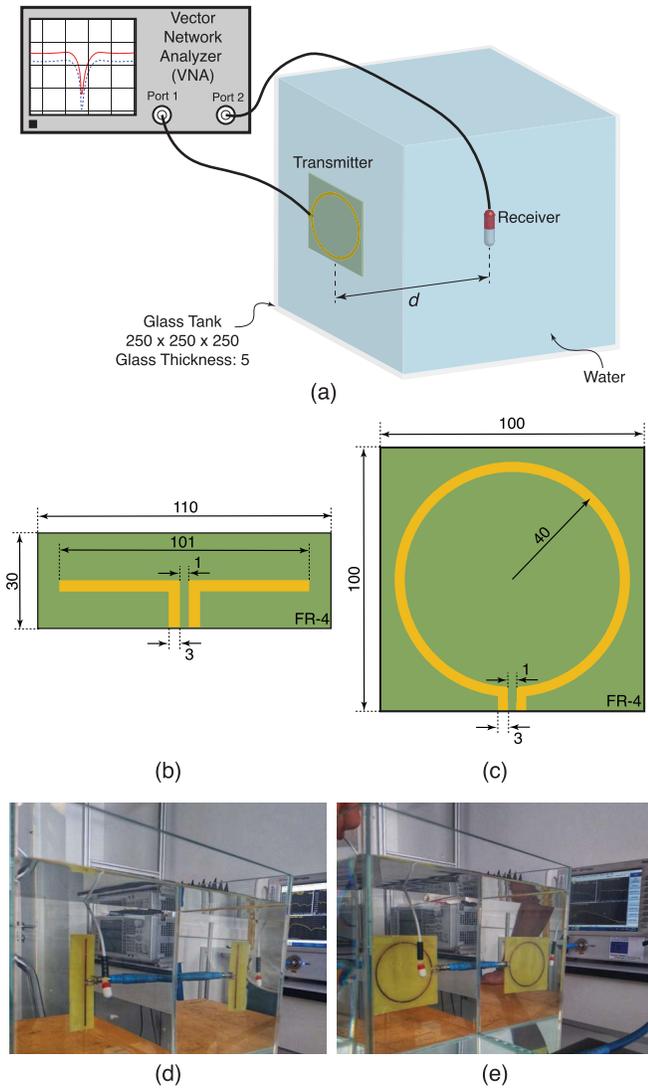


Fig. 2. Experimental evaluation of WPT efficiency in lossy media. (a) Transmitter is positioned outside a cubic glass tank filled with water, whereas the receiver designed in [44] is inside the tank at a distance d from the transmitter. Then, the scattering parameters are measured with a two-port VNA considering (b)–(d) electric (dipole antenna) and (c)–(e) magnetic (loop antenna) transmitters. All the dimensions are in millimeters.

in which the forward transmission coefficient S_{21} is de-embedded from the input reflection coefficient S_{11} . These measurements were carried out for distances d ranging from 50 to 200 mm.

D. Results and Discussion

The WPT efficiencies for the electric η_E and magnetic η_H sources were evaluated from the electromagnetic fields calculated through the 2-DA model and the SWE model. In Fig. 3, the efficiency for both the sources is shown as a function of the frequency for different phantom radius R_p , which is asymptotically equivalent to the variation in the implantation depth. Besides, the chosen range comprises most of the applications for wireless-powered implants, from subcutaneous to deeply implanted devices. In addition, the measured efficiencies defined as $\eta = |S_{21}|^2$ from different

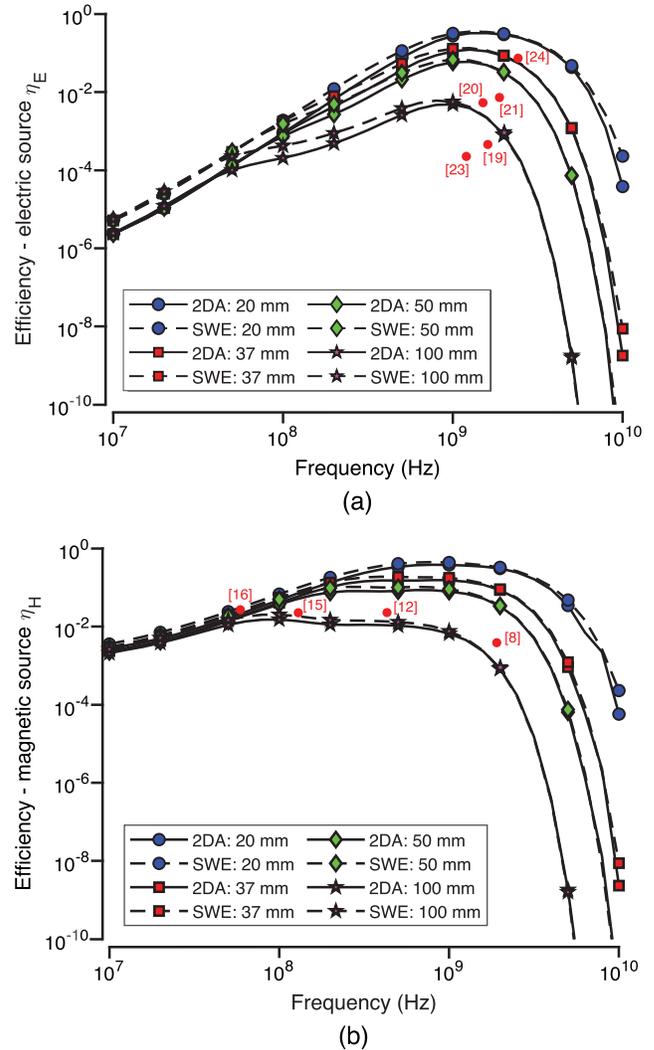


Fig. 3. WPT efficiency for an (a) electric η_E receiver and (b) magnetic η_H receiver as a function of frequency and phantom radius R_p (asymptotically equivalent to implantation depth) evaluated through the 2-DA and the SWE models. The red dots indicate the efficiency of physically realized WPT systems proposed in the literature and detailed in Table I.

TABLE I
COMPARISON BETWEEN DIFFERENT IMPLANTABLE WPT SYSTEMS
PROPOSED IN THE LITERATURE

Reference	Source Type	Frequency	Implantation depth	Efficiency
[8]	Magnetic	1.9 GHz	20 mm	0.35%
[14]	Magnetic	433 MHz	20 mm	2.03%
[16]	Magnetic	131 MHz	18 mm	2.01%
[17]	Magnetic	60 MHz	16 mm	2.40%
[20]	Electric	1.6 GHz	55 mm	0.04%
[21]	Electric	1.5 GHz	55 mm	0.45%
[22]	Electric	1.87 GHz	60 mm	0.61%
[24]	Electric	1.2 GHz	58 mm	0.02%
[25]	Electric	2.4 GHz	10 mm	8%

WPT approaches in the literature are indicated in Fig. 3 and they are detailed in terms of source type, operating frequency, and implantation depth in Table I.

First, the results obtained from the two approaches previously described are compared. As can be seen in Fig. 3,

TABLE II

MAXIMUM EFFICIENCY AND OPTIMUM FREQUENCY FOR THE 2-DA MODEL AS A FUNCTION OF THE PHANTOM'S RADIUS (ASYMPTOTIC TO THE IMPLANTATION DEPTH)

R_p (mm)	Electric Receiver	Magnetic Receiver
20	35.44% at 1.26 GHz	44.92% at 794.3 MHz
37	13.43% at 1.26 GHz	19.01% at 398.1 MHz
50	6.83% at 1 GHz	10.44% at 631 MHz
100	0.49% at 1 GHz	2.04% at 100 MHz

the efficiency evaluated with the 2-DA model agrees with the one calculated with SWE, especially at the vicinity of the optimum frequency where the error between them is 0.64% for the electric receiver and 2.07% for the magnetic one. However, for lower frequencies, an offset between them is noticeable mainly due to the difference in the source formulation. Apart from that, the maximum efficiencies theoretically calculated with the proposed model corroborate with those experimentally achieved in previous works.

Regarding the efficiency behavior over the frequency, for near-field operations at lower frequencies, the magnetic source outperforms the electric one for all the evaluated implantation depths. For instance, Table II shows that the optimum frequency for the magnetic receiver is below the far-field region, roughly starting at 1 GHz. In addition, at the near-field region, η_E sharply increases until reaching its maximum, whereas η_H initially increases and then reaches a plateau at the maximum efficiency. Conversely, both the receivers present similar decaying behavior in the far-field region, and η_E asymptotically approaches η_H at frequencies above the optimum one for the electric receiver.

As the reflection losses can be disregarded, this overall behavior for both the receivers can be explained by the fact that in low frequencies, the near-field losses are higher, whereas in the far-field region, the attenuation losses become more significant [32]. Thus, the optimum frequency corresponds to the tradeoff point between both the loss mechanisms. Moreover, once the near-field losses affect more electric than magnetic sources, the efficiency at low frequencies is significantly lower for this receiver.

The analysis carried out in this article considers fixed dimensions for the receiver. However, a further study on the peak efficiency and optimum frequency dependence on the receiver dimensions is presented in [27]. It has shown that the receiver length L is the parameter that impacts the efficiency the most; for instance, the larger the electric source, the higher the efficiency. On the other hand, for a magnetic source, the peak efficiency is reached within the range $1.5Rc < L < 3Rc$. In addition, the fundamental limit on the electrically small antennas efficiency states that a reduction in the receiver size will also lead to a reduction in its radiation efficiency. Therefore, the receiver size considered in the previous analysis not only is in the range that leads to maximum efficiency but also corresponds to the size of practical implementation of implantable and ingestible antennas [42].

The experimental results for the maximum efficiency and the optimum frequency considering an electric (dipole antenna) transmitter and a magnetic (loop antenna) transmitter

TABLE III

MEASURED MAXIMUM EFFICIENCY AND OPTIMUM FREQUENCY AS A FUNCTION OF THE DISTANCE d BETWEEN TRANSMITTER AND RECEIVER

d (mm)	Electric Transmitter (Dipole)		
	Optimum Frequency	Max. Efficiency (Water)	Max. Efficiency (1 g/l NaCl)
50	1.15 GHz	9.96×10^{-4}	3.51×10^{-4}
100	1 GHz	2.02×10^{-4}	1.03×10^{-4}
150	953.6 MHz	7.48×10^{-5}	1.75×10^{-5}
200	879.3 MHz	3.69×10^{-5}	5.62×10^{-6}
d (mm)	Magnetic Transmitter (Loop)		
	Optimum Frequency	Max. Efficiency (Water)	Max. Efficiency (1 g/l NaCl)
50	867 MHz	1.53×10^{-3}	9.72×10^{-5}
100	743.2 MHz	7.40×10^{-4}	3.46×10^{-5}
150	706 MHz	2.49×10^{-4}	1.42×10^{-5}
200	693.7 MHz	2.02×10^{-4}	7.52×10^{-6}

are presented in Table III for distances d between the transmitter and the receiver from 50 to 200 mm. The measurements agree with the theoretical conclusions obtained with the proposed model and the SWE approach, showing that as the distance between the transmitter and the receiver (implantation depth) increases, the optimal frequency decreases for both the sources. However, while the electric transmitter leads to an efficiency peak around 1 GHz which corresponds to the mid-field region, the magnetic transmitter achieves maximum efficiency for near-field operation. Moreover, the measurements were carried out in a solution with 1 g of sodium chloride (NaCl) per liter. Although there are no significant changes in the optimum frequency, the increase in the medium conductivity leads to a reduction in the efficiency. The difference in the efficiency values is due to the fact that the theoretical ones represent the maximum achievable efficiency taking into account only the intrinsic loss of the channel. In contrast, other losses such as the scattering phenomena at the interface between the phantom and external media affect the experimental results (note that the antenna reflection losses are deembedded from the results; see Section II-C).

III. EFFICIENCY ASSESSMENT USING THE ANATOMICAL PECTORAL MODEL

To analyze the WPT efficiency in a more realistic scenario, we implemented a 2-D heterogeneous model of the human pectoral region presented in Fig. 1(c) with nine dispersive media with complex permittivity equivalent to those in the different human tissues [45]. Based on the wirelessly powered pacemaker proposed in [20], the receiver is represented by a circular region with a radius of 1 mm inside the heart with implantation depth d equal to 37 mm from the closest skin interface.

Similarly, as described for the spherical model in Section II, the electric permittivity of the region external to the body is the same as a lossless skin $\epsilon_{\text{skin}}(f)$, whereas the lossless medium inside the pacemaker $\epsilon_{\text{muscle}}(f)$ is also perfectly matched to the wave impedance of the myocardium. In this way, the reflection losses can be disregarded.

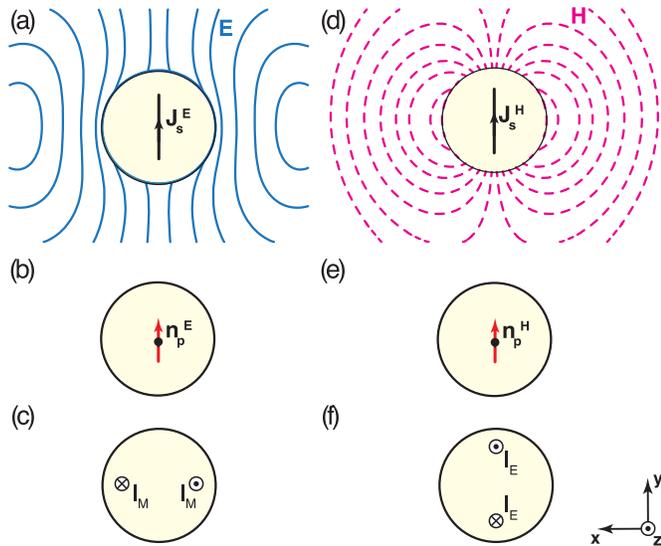


Fig. 4. Different receiver configurations are used for the realistic model analysis. An electric receiver can be defined through (a) surface electric current distribution \mathbf{J}_s^E , (b) EPD \mathbf{n}_p^E , and (c) out-of-plane MC I_M . Alternatively, a magnetic receiver can be modeled as (d) surface MC distribution \mathbf{J}_s^H , (e) MPD \mathbf{n}_p^H , and (f) out-of-plane LC I_E . The contour lines depict the electric \mathbf{E} and magnetic \mathbf{H} field distributions in arbitrary units.

For the analysis of this problem as a 2-D model, it is assumed that the implantable receiver and the on-body transmitter are perfectly aligned, and therefore, the z -axis invariance is valid, i.e., $\mathbf{E}(x, y, z) = \mathbf{E}(x, y)e^{ik_z z}$, where k_z is the out-of-plane propagation constant. Moreover, due to the high tissue dispersivity, the radiated power is attenuated at short distances from the transmitter. Therefore, the computational cost can be reduced by analyzing only the cross section of the body region in which the receiver is implanted.

The same approach described in Section II was applied to the 2-D pectoral model to calculate the maximum WPT efficiency in a realistic scenario and compare these results with those obtained with the simplified spherical model. The reciprocity theorem is again invoked for calculation purposes, and the radiation source is considered inside the heart. This premise is still valid once the different media are linear and there is no polarization mismatch. Consequently, the obtained efficiency calculated with (3) is valid for the original problem of powering the implantable device.

However, differently from the 2-DA case, different receiver configurations and orientations can be used in the realistic planar model, as shown in Fig. 4. The first possibility is to assign an SCD over the line of length L (in the 2-D simulation) for the electric $\mathbf{J}_s^E(x, y, z)$ and magnetic $\mathbf{J}_s^H(x, y, z)$ receivers according to

$$\mathbf{J}_s^E = \begin{cases} \cos\left(\frac{\pi y}{L}\right) \text{ A/m } \hat{\mathbf{y}}, & \text{if vertically oriented} \\ \cos\left(\frac{\pi x}{L}\right) \text{ A/m } \hat{\mathbf{x}}, & \text{if horizontally oriented} \end{cases} \quad (9a)$$

$$\mathbf{J}_s^H = \begin{cases} 1 \text{ V/m } \hat{\mathbf{y}}, & \text{if vertically oriented} \\ 1 \text{ V/m } \hat{\mathbf{x}}, & \text{if horizontally oriented.} \end{cases} \quad (9b)$$

Henceforward, vertically oriented means that the receiver is oriented in the y -axis direction ($\hat{\mathbf{y}}$), whereas horizontally in the x -axis direction ($\hat{\mathbf{x}}$), according to the coordinate system depicted in Fig. 4.

Subsequently, the next alternative is to define the receiver as an electric point dipole (EPD) or magnetic point dipole (MPD). In each one, the electric \mathbf{n}_p^E or magnetic \mathbf{n}_p^H dipole moment vector is assigned as follows:

$$\mathbf{n}_p^E = \begin{cases} 1 \text{ A}\cdot\text{m } \hat{\mathbf{y}}, & \text{if vertically oriented} \\ 1 \text{ A}\cdot\text{m } \hat{\mathbf{x}}, & \text{if horizontally oriented} \end{cases} \quad (10a)$$

$$\mathbf{n}_p^H = \begin{cases} 1 \text{ A}\cdot\text{m}^2 \hat{\mathbf{y}}, & \text{if vertically oriented} \\ 1 \text{ A}\cdot\text{m}^2 \hat{\mathbf{x}}, & \text{if horizontally oriented.} \end{cases} \quad (10b)$$

Finally, it is also possible to define an out-of-plane magnetic current (MC) for modeling the electric receiver or an out-of-plane line current (LC) for the magnetic one. Respectively for each case, the electric or magnetic fields are orthogonal to the current distribution direction and the position vector. Therefore, the out-of-plane magnetic $I_M = 1 \text{ V}$ and electric $I_E = 1 \text{ A}$ currents must be assigned following the direction and orientation shown in Fig. 4(c) and (f), respectively.

By taking into account the three source types and the vertical and horizontal orientations, six configurations for each electric and magnetic receiver are possible. Finally, the WPT efficiency was evaluated for all the described scenarios, and the results are presented in Fig. 5. It is possible to see that the efficiencies evaluated with different sources agree between them, which demonstrates the flexibility of the proposed model for dealing with different source configurations.

The source orientation is the factor that mainly affects the radiation efficiency. In the best case scenario, the sources are horizontally oriented, whereas the vertical orientation corresponds to the worst position for the receiver. Since the receiver is vertically oriented, the radiation beam propagates toward the direction parallel to the chest boundary, which is the closest to the receiver and, therefore, the region that contributes the most for the integral in (2b). This behavior was also pointed out in [26] but, from the results shown in Fig. 5, it is possible to evaluate the difference between best and worst case scenarios quantitatively. Namely, for the best positioning, the electric source presents an optimum frequency 590 MHz higher with a maximum η_E approximately five times the one verified with a vertically oriented source. A similar offset in efficiency magnitude can be verified between a horizontal magnetic source and a vertical magnetic source. For lower frequencies, the best positioning leads to an efficiency around 2.5 times higher; however, the maximum difference between them surpasses 13 times in the far-field region.

It is also noticeable that the radiation efficiency behavior for an electric or magnetic receiver obtained with the realistic pectoral model agrees with those obtained with the simplified spherical model. Namely, for the horizontally oriented electric sources, η_E increases in the near-field range with a peak of 0.77% at 1.74 GHz, close to the optimum frequency shown in Table II for the same implantation depth of 37 mm, and then decreasing for higher frequencies. In contrast, η_H reaches

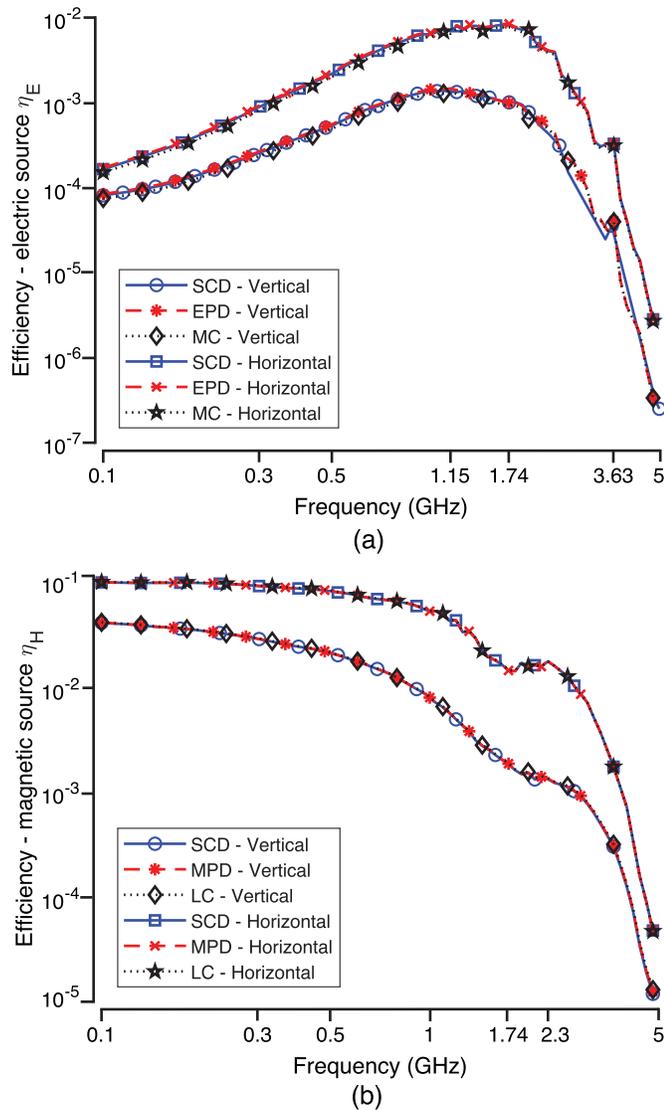


Fig. 5. Efficiency was evaluated with the realistic pectoral model for an (a) electric η_E and (b) magnetic η_H receiver implanted in the heart. Different receiver orientations (vertical and horizontal) and configurations (SCD, EPD and MPD, out-of-plane MC and LC) are compared.

its maximum at lower frequencies, remaining almost constant around 10% in the near-field, before decreasing for frequencies above 1 GHz. The sharp reduction in radiation efficiency by a magnetic source in the far-field region is explained by the fact that this kind of source achieves its optimal performance as an electrically small antenna [48], [49], i.e., when $L < \lambda/10$ which is satisfied only in the near-field region.

As expected, there is a significant reduction in the maximum efficiencies obtained with the realistic model compared with the simplified spherical model. First, the latter considers a homogeneous medium equivalent to the human muscle tissue, whereas in the pectoral model, several organs with different electromagnetic properties are taken into account. Two predominant loss sources are responsible for this efficiency deterioration: the increased attenuation, mainly in the fat and muscle layers where the power is dissipated before reaching the receiver in the heart; and the reflection losses due to the

wave impedance contrast between the media that compose the tissues. In this last case, with the multiple reflections, most of the reflected power is dissipated in the tissue reducing the amount of power that reaches the receiver encapsulation. Therefore, this loss is accounted on (1) also through P_d . Moreover, in a realistic scenario, the shape of the organs may lead to resonance modes responsible for local peaks and valleys in efficiency for some frequencies, such as 3.63 GHz for the electric source and around 1.74 GHz for the magnetic source.

IV. EFFICIENCY ASSESSMENT USING A PHYSICALLY REALIZABLE MODEL

The case study of a wirelessly powered pacemaker is analyzed to establish the optimum parameters that lead to the maximum efficiency in a physically realizable application. In this case, the human pectoral model in Fig. 1(c) is used. However, the transmitter is now localized in the chest, as shown in Fig. 6(a). This transmitter comprises a substrate with the same dielectric properties as the medium external to the body and a lossless superstrate (or buffer) with thickness d and relative electric permittivity ϵ_r^b .

The electric transmitter in Fig. 6(b) is defined by assigning an SCD $\mathbf{J}_s^E(x, y, z)$ given by

$$\mathbf{J}_s^E = \left[\cos\left(\frac{\pi x}{L}\right), 0, 0 \right] \quad (11)$$

in which L is the transmitter length. Concurrently, the magnetic transmitter is modeled as a unitary out-of-plane electric current $I_E = 1$ A on the edge of the source with opposite phases, as illustrated in Fig. 6(c). As seen from the field distribution for the electric and magnetic transmitters, they are, for instance, equivalent to a dipole and loop antenna, respectively.

A. WPT Efficiency as a Function of Transmitter Parameters

In this configuration, the two main transmitter parameters that can be changed to achieve the maximum WPT efficiency are the buffer thickness d and its permittivity ϵ_r^b . Therefore, a parametric analysis was carried out for both the parameters within the ranges: $1 \leq d \leq 50$ mm and $1 \leq \epsilon_r^b \leq 80$. Furthermore, the lower and upper bounds for ϵ_r^b were chosen so that this range comprises the permittivities of all the nine tissues in the frequency range from 100 MHz to 5 GHz. Consequently, the effective permittivity for this pectoral region is also in the chosen interval.

The operating frequency must be chosen and fixed to carry out this parametric study. Based on the results shown in Fig. 5, the maximum theoretical WPT efficiency for a deep-implanted pacemaker charged by an electric source transmitter is achieved at the frequency of 1.74 GHz. Considering the frequency bands allocated for industrial, scientific, and medical (ISM) usage, the closest band to the optimal frequency is centered at 2.45 GHz. Henceforward, this is the frequency chosen for all the following analyses, and the transmitter length L was set as $\lambda/2$ at this frequency in free space.

To evaluate the WPT system for this configuration, (3) can still be applied with the results from integrals in (2a)–(2c);

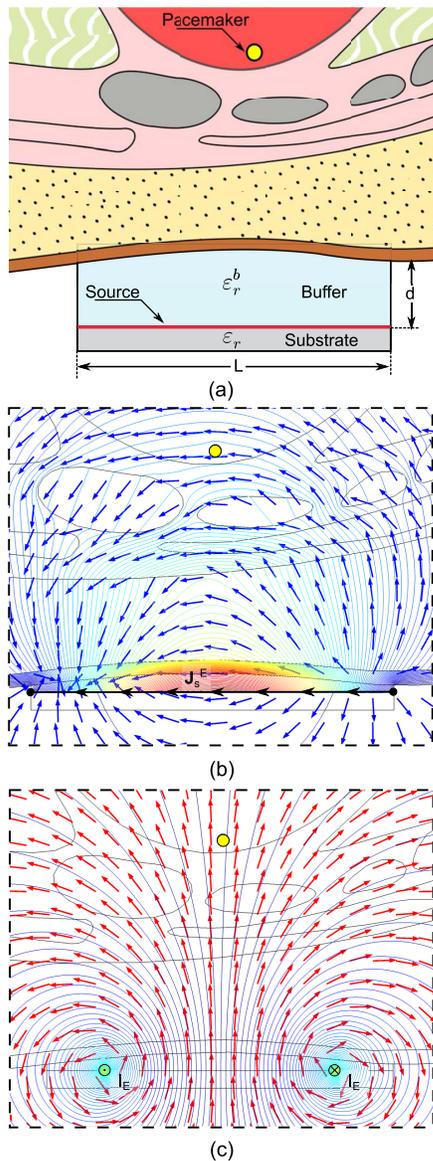


Fig. 6. Analysis setup for the parametric analysis of the efficiency in a wireless-powered pacemaker application. (a) Close-up view of the on-body transmitter with length L composed of a radiation source positioned apart from the skin by a lossless superstrate (buffer) with thickness d and permittivity ϵ_r^b and with a substrate matched to the medium external to the body. (b) Electric source modeled as a surface current density \mathbf{J}_s^E with the electric field distribution indicated by the arrows and the magnetic field by the isolines. (c) Magnetic source modeled as an out-of-plane current \mathbf{I}_E with the magnetic field distribution indicated by the arrows and the electric field by the isolines.

however, the integration domains need to be reformulated. In this case, Ω_s indicates that the integral is performed on the boundary of the pacemaker, whereas Ω_p represents the transmitter's boundary.

The contour levels for the efficiency as a function of the buffer thickness and permittivity are shown in Fig. 7(a) for electric and Fig. 7(b) for magnetic sources. As can be seen, the buffer parameters that lead to the maximum efficiency are $d = 7$ mm and $\epsilon_r^b = 80$. The fact that the maximum efficiency is obtained with the highest permittivity can be explained once the wave impedance mismatching at the buffer–skin transition is practically eliminated. In addition, taking into

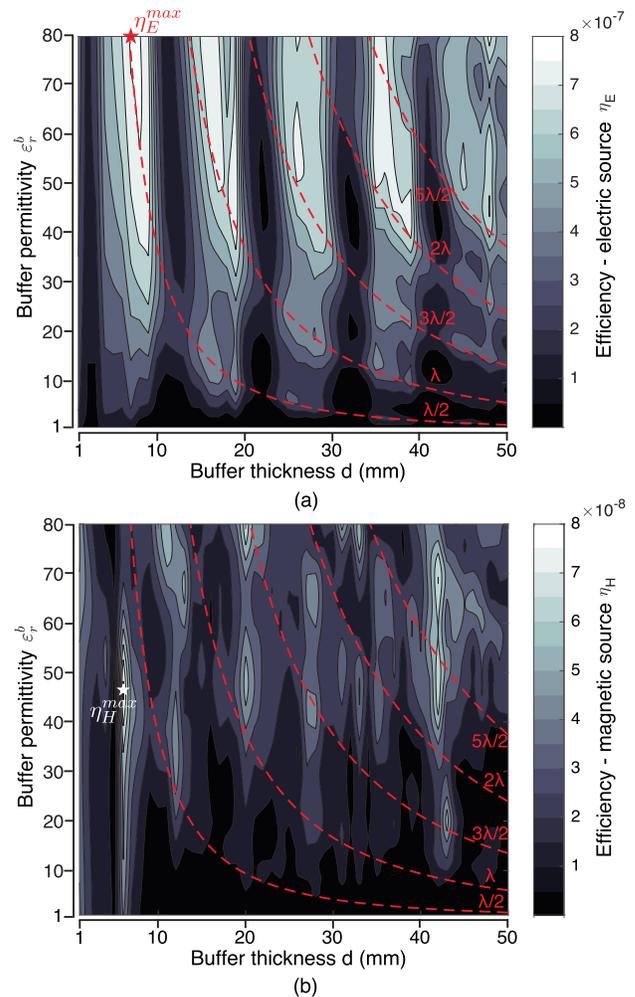


Fig. 7. Contour plots for the efficiency as a function of the buffer thickness d and permittivity ϵ_r^b for (a) electric source η_E and (b) magnetic source η_H . The star indicates the global maximum position, and the dotted lines indicate the position corresponding to $\lambda/2$ its integer multiples as a function of ϵ_r^b .

account this permittivity, the maximum occurs exactly at $\lambda/2$. As proved in [50] by considering the superstrate as a transmission line, it corresponds to the resonance condition, once the impedance seen in the transmitter–skin transition is equal to the impedance seen in the source, which leads to a high voltage at the source position, thus increasing the radiation efficiency. Moreover, it can be seen that as the buffer's thickness increases, it decreases the optimum ϵ_r^b in such a manner that a $\lambda/2$ periodicity is obeyed, as it also happens with a lossless transmission line.

On the other side, the maximum efficiency obtained with a magnetic source is approximately an order of magnitude lower when compared with the electric one. It means that at the frequency of 2.45 GHz, the magnetic source is suboptimal, as it was also predicted in the graph of Fig. 5(b), once it does not satisfy the electrically small antenna condition at this frequency. However, the maximum efficiency is achieved with $d = 6$ mm and $\epsilon_r^b = 46.5$. It is important to mention that in this case, this maximum occurs in a significantly narrow distance range, which in practice would require precise positioning of the source.

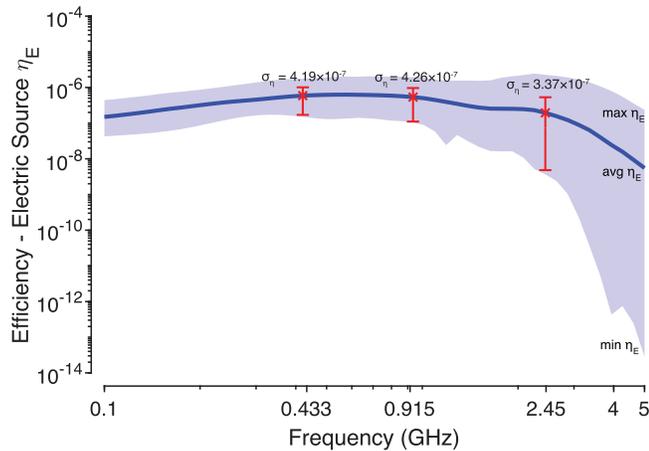


Fig. 8. WPT efficiency considering an optimal electric transmitter. The continuous blue line is the efficiency averaged ($\text{avg } \eta_E$) over the 200 pacemaker positions. Besides, the blue area represents the maximum ($\text{max } \eta_E$) and minimum ($\text{min } \eta_E$) efficiency values. Finally, the red bars show the standard deviation on the efficiency σ_η at the ISM frequencies of 433 MHz, 915 MHz, and 2.45 GHz.

B. Maximum Efficiency Assessment Due to Stochastic Antenna Misalignment

To classify and quantify the losses, the optimal scenario in which the transmitter is composed of an electric source and a buffer with $d = 7$ mm and $\epsilon_r^b = 80$ is considered. Three main loss mechanisms can be identified: 1) reflection losses due to the wave impedance contrast between the on-body transmitter and the body tissue; 2) antenna near-field losses; and 3) the attenuation losses in the tissues. The first two losses can be mitigated by adequately designing the WPT system, whereas the latter cause is unavoidable. For instance, approximately 7% of the transmitted power is lost due to reflection in this optimum configuration, whereas 93% is due to attenuation and near-field losses combined. However, the optimal buffer parameters justify the low reflection losses and reduce the near-field region and its associated losses.

Apart from that, the maximum efficiency levels are significantly affected by fluctuations in the implantation depth caused by the intrinsic movements of the human body. For instance, the heart movements lead to fluctuations in the implant position, resulting in misalignment between the transmitter and the receiver. Therefore, to evaluate these efficiency variations, the full-wave simulation was performed at 200 random implant locations uniformly distributed within the heart. After that, the WPT efficiency for each pacemaker position is calculated, considering the optimal electric transmitter. The obtained results for maximum, minimum, and average efficiency are shown in Fig. 8. In addition, the standard deviations on the efficiency values σ_η are shown for the ISM frequencies of 433 MHz, 915 MHz, and 2.45 GHz.

The results in Fig. 8 show that the difference between the minimum and maximum efficiency values increases with the frequency; however, the average efficiency and standard deviation remain within a close range for the frequency bands commonly used in biomedical applications. This variation in the optimum frequency is explained by the fact that the optimum frequency and the maximum efficiency decrease

as the implantation depth increases, as previously described in Fig. 3.

Finally, the fact that the efficiency obtained in this case is significantly lower when compared with the optimum efficiency presented in Fig. 5 shall be addressed. It can be explained by the fact that the transmitter is considered to be a conformal structure covering the entire body surface in the ideal scenario described in Section III. In contrast, the current analysis takes into account a mono-antenna transmitter, leading to a much smaller integration domain Ω_p thus reducing the received power. In practical terms, it means that the single antenna mid-field WPT solutions currently in the literature are suboptimal by many orders of magnitude. Therefore, to physically achieve the maximum efficiency theoretically obtained, further developments in mid-field WPT are required based on conformal antenna arrays such as in [51] and techniques for electromagnetic focusing in lossy media that have already been investigated for other biomedical applications [52].

C. Electromagnetic Exposure Assessment

Another major concern of in-body WPT applications is the electromagnetic exposure levels. The surface profiles for the local specific absorption rate (SAR) normalized by the transmitted power are shown in Fig. 9 for the optimal electric and magnetic sources. First, the SAR profiles follow the field distribution shown in Fig. 6(b) and (c), being higher in the center for the electric source, whereas it reaches its maximum around the source edges for the magnetic. In addition, in both the cases, the peak SAR is located in the skin layer, and no significant SAR values are observed in the vital organs. However, by comparing both the SAR levels, it is noted that the magnetic source leads to a larger SAR, almost twice the value for the electric source, even with much lower efficiency levels. Since the SAR is related to the attenuation in the tissues that cannot be physically mitigated, it is possible to conclude that the efficiency is maximized by properly choosing the transmitter parameters, and the electromagnetic exposure is minimized.

V. GUIDELINES FOR DESIGNING OPTIMAL IMPLANTABLE WPT SYSTEMS

The analysis and results described in Sections II–IV lead to useful insights that can be applied as guidelines to design implantable WPT systems that are able to achieve efficiency close to the expected optimal values. For instance, given the implantation depth of the receiver, the following points can be considered.

A. WPT Technique and Operating Frequency

For subcutaneous implants, near-field techniques such as inductive and capacitive coupling can achieve higher efficiency levels. However, as the implantation depth increases, the maximum efficiency is reached at frequencies between 900 MHz and 3 GHz. Therefore, the mid-field and far-field techniques can show better performance for powering of deep-implanted miniature bioelectronics. Moreover, given the implantation depth and the operating frequency, the maximum efficiency values are given in Fig. 3.

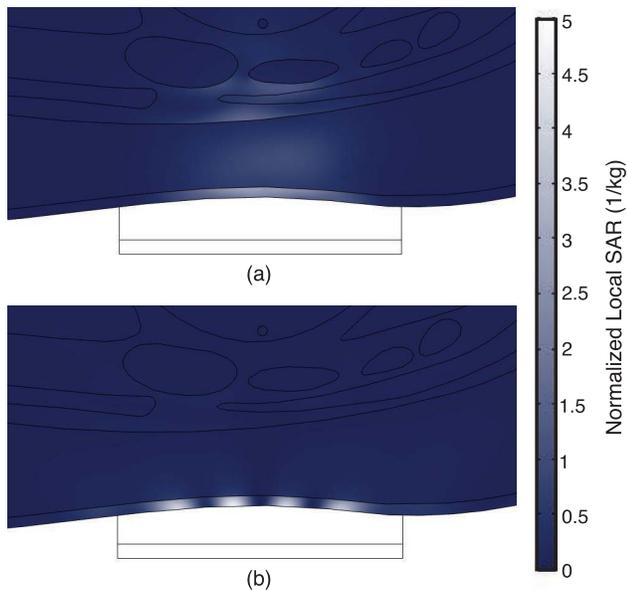


Fig. 9. Surface plot of the local SAR (point SAR) in the region between the on-body transmitter and the deep-implanted receiver normalized by the transmitted power considering an optimal (a) electric and (b) magnetic source.

B. Antenna Type and Orientation

At frequencies below 300 MHz, magnetic loop antennas are able to reach significantly higher efficiencies than electric-type antennas. On the other side, the high permittivity of the human tissues electrically increases the effective aperture size of dipole or patch antennas, making them more suitable for implantable WPT systems operating at frequencies higher than the sub-GHz band. The maximum efficiency values for both the electric and magnetic antennas as a function of the frequency are presented in Fig. 3 whereas the effect of the source orientation is shown in Fig. 5.

C. On-Body Transmitter Design

For single on-body transmitter applications, higher WPT efficiencies can be achieved by designing a buffer structure that separates the transmitter antenna and the skin, as shown in Fig. 7. In this case, the relative permittivity and the thickness of this superstrate must be chosen to reduce the wave impedance mismatch at the transmitter–skin interface [53]. For instance, for an electric source, the maximum WPT efficiency is achieved for the buffer thickness equal to $\lambda/2$. Apart from that, the standard deviation on the efficiency due to stochastic misalignments between the on-body transmitter and the in-body receiver caused by body movements is shown in Fig. 8 for the main ISM frequencies used in biomedical applications. Moreover, the local SAR patterns for an electric and magnetic on-body transmitter can be seen in Fig. 9. Even though the single-antenna configuration is constructively simpler, it exhibits suboptimal performance for implantable WPT systems. Therefore, to achieve efficiency closer to the levels given in Fig. 3 and lower exposure levels, conformal transmitter arrays should be used in addition to applying techniques for electromagnetic focusing in lossy media.

D. In-Body Receiver Design

Although the constraints on the shape and dimensions of in-body antennas reduce the degrees of freedom in their design, some points can be observed to enhance the receiver performance. First, an appropriate type of the antenna (electric or magnetic) has to be chosen depending on the receiver size and its operating frequency [27]. A high-permittivity encapsulation material can be used to increase the efficiency of an electric-type receiver [54]. The dielectric loading electrically increases the aperture size, reduces the near-field losses, and an efficiency close to the fundamental bounds can be achieved [27]. Other alternatives to enhance the efficiency are filling the receiver encapsulation with a low-loss dielectric material and using the thickest possible substrate [42]. Finally, reconfigurable receiver antennas can be implemented to achieve near-optimal radiation performance across a broad range of conditions [44], [55].

VI. CONCLUSION

To wirelessly power implantable bioelectronic devices, several techniques can be used depending on the application characteristics. However, the combination of different physical mechanisms imposes a limit on maximum achievable wireless powering efficiency. Among them, the principal mechanism is the electromagnetic attenuation in the dispersive tissues, the reflection losses, and the fundamental efficiency limitation of electrically small antennas. In addition, there are system-level losses and resonant modes in the body cavities that also contribute to efficiency deterioration. Therefore, this work focused on evaluating the wireless powering efficiency of deep-body implanted devices and studying how the system's parameters could be tuned to reach the highest efficiency possible in a practical application.

Toward this goal, a mathematical formulation for this problem was proposed based on reciprocity and T -symmetry principles as well as considering an on-body conformal source, perfectly matched to the human tissue. Such hypotheses lead to optimum energy focusing and, thus, to the highest possible efficiency. To validate this approach, a semi-analytical SWE analysis was carried out, and the results for a simplified spherical representation for the human body were compared.

This first analysis indicates that a magnetic receiver outperforms the electric one in the near-field frequency range, whereas in the far-field, both the receivers show similar performance. Therefore, the optimum frequency is in the mid-field region and depends on the source type and implantation depth, leading to the highest efficiency.

Once the proposed approach was validated, it was applied to an anatomical model focused on a deep-implanted wireless-powered pacemaker application [20]. This analysis verified that the overall behavior for both the sources agrees with the one predicted by the simplified spherical model, including the optimum operation in the mid-field range. Furthermore, this optimum frequency also agrees with the results presented in the literature obtained through different approaches [26], [27], [30], [31], [32], [33], [34]. Even though there is a significant efficiency reduction in the realistic model results, the wave impedance contrast between the different tissues

imposes reflection losses that were disregarded in the simplified model. Moreover, with this model, it was verified that the receiver orientation is another practical aspect that can reduce efficiency. Considering the source positioning, the maximum difference in efficiency between the best and worst case scenarios is around five times for an electric receiver, whereas for the magnetic one, this difference can be above 13 times. The effect of the source orientations is justified once in the best case, i.e., for a horizontally oriented receiver, the power flows toward the chest line, which is the closest point to the receiver, contributing more to the overall received power. It is important to mention that the flexibility in analyzing different source types is another contribution of the proposed approach compared with other methods of analysis.

Finally, a WPT system considering a deep-implanted pacemaker as the receiver and a multilayered (substrate-source-buffer) transmitter positioned in the chest was considered to analyze the impact of the transmitter's parameters on the powering efficiency and to provide information on how these parameters could be tuned to achieve the maximum efficiency. This parametric study has shown that in the 2.4-GHz ISM band, the electric transmitter leads to efficiency over a degree of magnitude higher than a magnetic one. In addition, the maximum efficiency can be achieved with a lossless high-permittivity buffer, matched to the skin permittivity, and thickness equal to $\lambda/2$ in this medium. Furthermore, other local maxima can be obtained for thicker and lower permittivity superstrates, respecting a $\lambda/2$ periodicity.

To summarize, the approach proposed in this article is able to predict the maximum achievable powering efficiency considering simplified or anatomical body models as well as to provide information on the parameters that can be optimized to achieve this maximum efficiency. In addition, even though the case study of a deep-implanted pacemaker was analyzed in this article, the same approach could also be used to evaluate the powering efficiency for other deep-body implantable devices.

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