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Memristor Device Characterization by Scanning Microwave Microscopy

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Abstract— We report memristive device characterization using near-field scanning microwave microscopy. Atomic force microscopy, magnitude and phase-shift images of the complex reflection coefficient of TiO₂ devices can be acquired simultaneously in the range 1-20 GHz. In particular, measurement of the complex reflection coefficient of a 200 by 200 nm² TiO₂ device is exemplary demonstrated. These results are beneficial for electrical modeling and optimization of memristor devices to address OxRAM applications.

Keywords—Oxide based random access memory (OxRAM), memristor, scanning microwave microscopy, atomic force microscopy, interferometry, metal oxide semiconductor capacitors.

I. INTRODUCTION

Resistive random access memory (RRAM) technologies have experienced an increasing interest these last years as a promising solution for storage and memory [1]. Indeed, emerging memory devices can offer potential alternative for flash technology or DRAM, thanks to their fast switching performances, high retention and cycling endurance, scalability, and back-end-of-line integration potential. Global understanding of the relative contribution of the different physical mechanisms is very challenging and significant efforts at the modeling and material characterization levels are still needed [2].

In this paper, we propose an analysis in the microwave domain to study dynamics in nanometer memristive devices. In particular, we consider TiO₂ material that has been largely investigated as prototypical material system for switching. A broadband near-field scanning microwave microscope (NSMM) consisting of an atomic force microscope combined with a vector network analyzer (VNA) is used to study the memristive device [3]. Basically, the tip scans across the sample, emitting a microwave signal scattered by the material, altering its amplitude or/and phase properties [4]-[9]. The measurement set-up and device fabrication including dedicated calibration kit are described in Section II. Preliminary experimental results are presented in Section III. In particular, microwave response of the memristive device as a function of the applied bias is demonstrated around 18 GHz.

II. MATERIAL AND METHODS

A. Interferometric SMM setup

The interferometric set-up of the NSMM is depicted in Fig. 1. It consists of a Keysight™ LS5600 AFM interfaced with a Keysight™ PNA series network analyzer E8362B through a homemade tuned interferometric matching network based on the Mach-Zehnder method [10]-[11]. This latter is built up in coaxial form with a power divider, two hybrid couplers, an active variable attenuator and two amplifiers in series. The basic principle consists in splitting the PNA source high frequency power wave a_1 in two coherent signals, i.e. the reference signal a_{INC} to the AFM tip and the interference signal. The coupler associated to the AFM tip acts as a reflectometer to separate the incident wave a_{INC} and the reflected wave a_{REF} from the device under test (DUT). The wave a_{REF} is then combined with the interference signal to provide the output signal a_3 at the output of the second coupler. This signal a_3 is cancelled by properly tuning the attenuator to balance the magnitudes of a_{REF} and the interference signal. The resulting signal a_3 signal is amplified and measured by the PNA receiver.

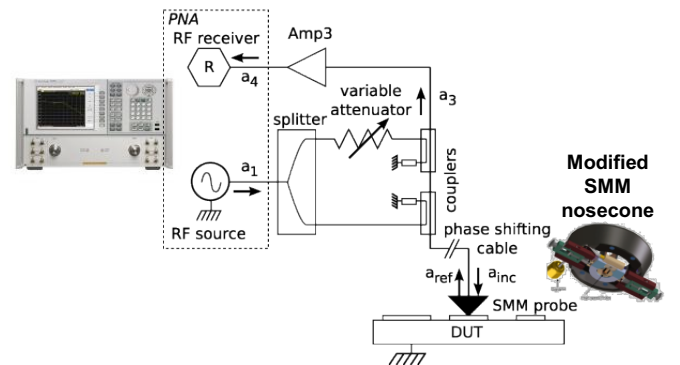


Fig. 1. Set-up of the scanning microwave microscope incorporating a tuned interferometric matching network based on the Mach-Zehnder method.

The resulting measured reflection coefficient $\Gamma = a_4/a_1$ considering ideal components can be expressed as a function of the reflection coefficient $\Gamma_{\text{DUT}} = a_{\text{REF}}/a_{\text{INC}}$ of the DUT by

$$\Gamma = \alpha(\Gamma_{\text{DUT}} + \beta). \quad (1)$$

where α is a complex coefficient taken into account losses and phase-shifts introduced by the microwave circuitry and β denotes the interference signal. At the test frequency and for a DUT with reference impedance Z_{REF} , the magnitude of the reflection coefficient Γ is set to zero resulting in high measurement sensitivity for impedances around Z_{REF} .

B. OxRAM devices and calibration kit fabrication

TiO₂ devices were realized on a P-type silicon substrate of resistivity 1–3 Ωcm (Fig. 2). The devices consist of Ti (5 nm)/Pt (30 nm)/TiO_{2-x}/TiO₂/Pt (15 nm)/Au (20 nm) from bottom to top. All metals were deposited by e-beam evaporation technique, and top electrodes were patterned by electron beam lithography (EBL) with targeted dimensions between 200×200 and 60×60 nm². TiO_{2-x}/TiO₂ films were obtained by atomic layer deposition (ALD) at 200°C with TiCl₄ as Ti precursor and H₂O as oxygen source. The water pulses were set shorter than the ones needed to saturate the surface in order to produce a deficient TiO_{2-x} layer. Post-deposition oxidation of the TiO_{2-x} top interface into TiO₂ was obtained by natural air exposure.

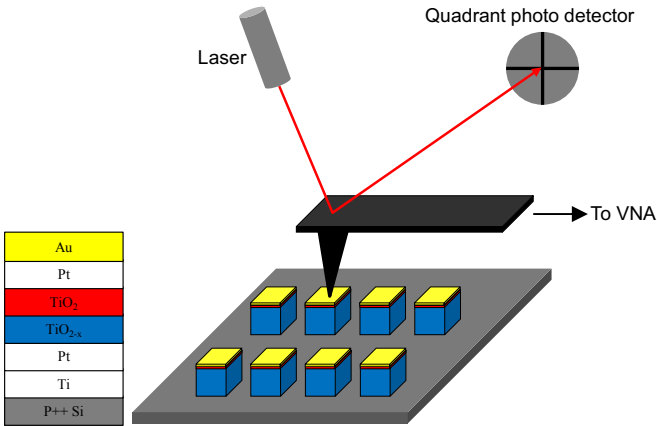


Fig. 2. Configuration of TiO₂ devices.

An on-wafer calibration kit consisting of MOS capacitors was fabricated on the same wafer. The MOS capacitors are composed of circular gold electrodes evaporated on SiO₂ deposited on one part of the wafer (Fig. 3). In order to vary the capacitance values, the diameter of the upper gold pad varies from 0.5 to 2 μm whereas the SiO₂ thickness was set to 140 nm.

From the AFM image, the topography of the TiO₂ devices are extracted along the wafer (Fig. 4). The data indicate a good homogeneity of the fabrication process.

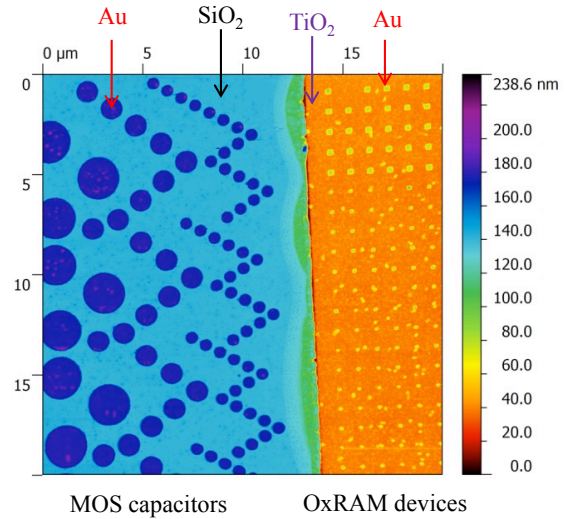


Fig. 3. AFM topography image of the fabricated sample. On the left, MOS capacitor top electrodes are measured. On the right, the OxRAM stack is measured.

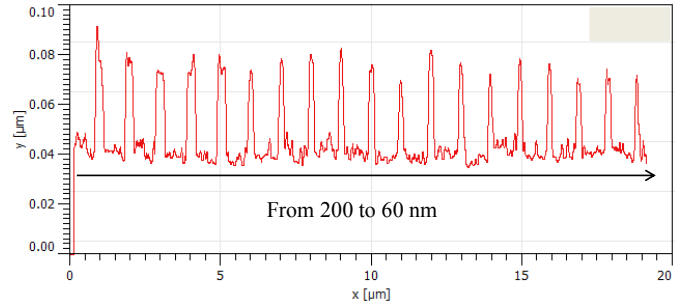


Fig. 4. 1D topography cross section of the fabricated TiO₂ devices from top to bottom of the Fig. 2 image. The size of the OxRAM devices vary from 200×200 down to 60×60 nm².

The impedance of the MOS structures measured at the tip apex of the probe is modeled by a series model consisting of an oxide capacitance C_{ox} and a depletion capacitance C_{depl} . Both capacitances can be described by the parallel plate capacitor formalism. The resulting capacitance C_{TOT} is given by

$$C_{\text{TOT}} = C_{\text{ox}} C_{\text{depl}} / (C_{\text{ox}} + C_{\text{depl}}). \quad (2)$$

The parallel-plate capacitance term without taking into account the fringing fields C_{ox} is calculated from the areas of the gold pads A and the SiO₂ thicknesses d_{ox} .

$$C_{\text{ox}} = A \frac{\epsilon_0 \epsilon_r \text{SiO}_2}{d_{\text{ox}}} \quad (3)$$

The silicon dioxide is assumed to have a relative dielectric constant of $\epsilon_{\text{rSiO}_2} = 3.9$. The thickness and areas of the capacitors were estimated from the AFM topography measurements (Fig. 3) to take into account any deviations in geometry induced by the fabrication process of the calibration

kit. The measured areas A were $1.13 \mu\text{m}^2$, $3.94 \mu\text{m}^2$ and $13.85 \mu\text{m}^2$. The charge stored on the capacitor is distributed across a certain depth that adds the depletion series capacitance C_{depl} in series to C_{ox} . The capacitance was estimated to be proportional to the area A of the metallic electrode and inversely proportional to the depleted zone depth d_{depl} according to

$$C_{\text{depl}} = \frac{\epsilon_0 \epsilon_{\text{rSi}}}{d_{\text{depl}}} \quad (4)$$

with $d_{\text{depl}} = \sqrt{2\epsilon_0 \epsilon_{\text{r}} \Psi / q N_A}$ and where $\epsilon_{\text{rSi}} = 12$ is the relative permittivity of the silicon bulk substrate, Ψ represents the interface band bending at the Si/SiO₂ interface and is set to 200 mV, q is the charge of the electron (1.6×10^{-19} C), N_A is the doping level of the silicon bulk around $8 \times 10^{15}/\text{cm}^3$. From relations (2) to (4), theoretical capacitances data can be derived.

III. EXPERIMENTAL RESULTS

The measurements were performed in contact mode around 18 GHz using a 25PT300A AFM tip from Rocky Mountain NanotechnologyTM. The RF power source is set to -30 dBm and the intermediate frequency bandwidth (IFBW) of the VNA is 100 Hz. The images were scanned over a $20 \times 20 \mu\text{m}^2$ with 2048 pixels. In addition to the topography image, the NSMM provides both magnitude and phase-shift images of Γ . Fig. 5 shows the image of the magnitude of the reflection coefficient obtained in zero-bias conditions.

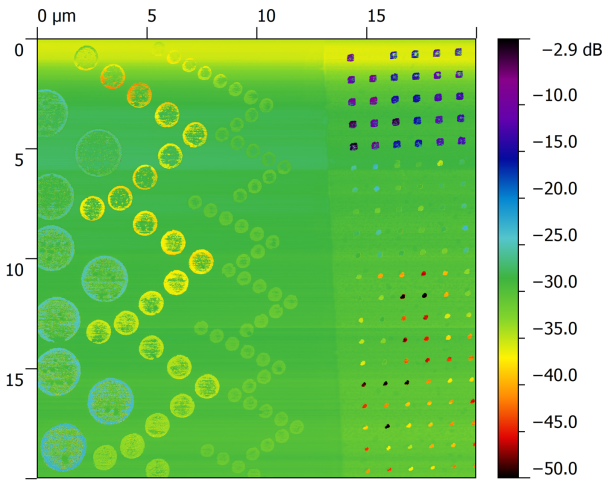


Fig. 5. Image of the magnitude of the reflection coefficient Γ at $f \sim 17.89$ GHz.

The measurement reliability is influenced by the quality of the electrical contact between tip and sample especially for capacitance gold pads. we observe a loss of the contact between the probe and the sample during the scanning. The loss of electrical contact is most likely caused by transient contamination of the gold pads. $200 \times 200 \text{ nm}^2$ OxRam devices (upper right of the image) are measured with high sensitivity. Magnitude contrast in respect with the background is between 18 and 24 dB. Smallest devices are also very sensitive to the microwave signal but exhibit different

responses between devices of same size. A similar phenomenon is observed for the phase-shift of Γ .

Fig. 6 shows the variation of the magnitude and phase of Γ as a function of the DC bias applied between probe tip and the bottom of a $200 \times 200 \text{ nm}^2$ device.

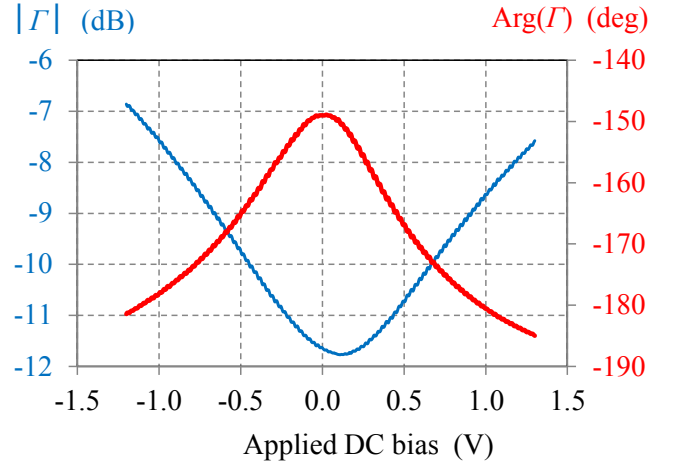


Fig. 6. Measured magnitude and phase of Γ as a function of the DC bias at $f \sim 17.89$ GHz.

From these data, variations of respectively 5 dB and 30 degrees are observed on the measured data when the DC bias is changed from -1.2 to 1.2 V.

IV. CONCLUSION

Near-field scanning microwave microscopy measurement of memristive devices have been experimentally demonstrated around 18 GHz. In particular, DC bias voltage impacts both magnitude and phase-shift responses of the microwave reflection coefficient in a sensitive manner. These preliminary results are instructive for further electrical modeling of the device. In particular, future works will include full vector calibration of the devices in a broad frequency range.

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