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Florian Wolf, Jean-Baptiste Doré, Xavier Popon, Sébastien de Rivaz, Francois Dehmas, et al.. Coherent Multi-Channel Ranging for Narrowband LPWAN: Simulation and Experimentation Results. 2018 15th Workshop on Positioning, Navigation and Communications (WPNC), Oct 2018, Bremen, Germany. 10.1109/WPNC.2018.8555746 . hal-02059014

HAL Id: hal-02059014

<https://hal.science/hal-02059014>

Submitted on 6 Mar 2019

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Coherent Multi-Channel Ranging for Narrowband LPWAN: Simulation and Experimentation Results

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Abstract—Precise radio based positioning for low power wide area networks remains a challenging research area due to narrowband signals and multipath propagation. Multi-channel ranging provides improved temporal resolution by coherent processing. While this technique has been applied to short range radio standards, no experimental demonstration for long range radio devices exists. The present paper introduces a hardware testbed for phase coherent multi-channel processing of narrowband signals. Simulations and preliminary experimental multi-channel results show a higher ranging precision (factor 20) over time based ranging. In a frequency flat channel with a 10 kHz signal, precisions down to 10 m (phase based) and 200 m (time based) have been achieved. Precision degrades in multipath propagation scenarios.

Index Terms—Experimental testbed, LPWAN localization, range estimation, phase-of-flight, frequency hopping

I. INTRODUCTION

Precise localization in wireless sensor networks (WSN) has become an interesting research area in recent years. Adding position information to the wireless transmitted data will enable new applications [1] and hence it is included in current standardization studies [2]. Positioning based on the communication radio signals should neither increase energy consumption nor hardware complexity of the node, which are critical to low power wide area network (LPWAN) use cases.

LPWAN radio technologies apply narrowband modulation schemes (e.g. NB-IoT, LoRa, Sigfox), offering high receiver sensitivity, required for long range communication over several kilometers. However, localization is challenging due to low temporal resolution and the difficulty to resolve multipath.

Techniques to improve localization accuracy on the system level comprise network densification [3] to enrich the set of measurements and sophisticated algorithms (e.g. finger printing [4], machine learning and deep neural networks). Improving the single link ranging precision, can provide more accurate raw estimates for positioning on the system level.

Coherent multi-channel ranging [5] allows aggregating multiple sequentially transmitted narrowband signals to a virtual increased bandwidth, making it compatible with LPWAN radio transceivers. Theoretical studies [6], [7] have investigated asymptotic precision limits while implementations [8]–[12] have demonstrated feasibility and an improved accuracy over single channel time based ranging techniques. Table I sum-

TABLE I
RELATED EXPERIMENTAL WORK: PARAMETERS & RANGING PRECISION

Related work	f_R in GHz	R_{comm} in m	BW_{sym} in MHz	BW_{virt} in MHz	σ_{ToF} in m	σ_{PoF} in m
LoRa [3]	0.868	4000	0.125	n/a	205	n/a
Sigfox [4]	0.868	3000	0.001	n/a	1000	n/a
WiFi [8]	2.4, 5	15	40	2600	15	0.5
Zigbee [9], [12]	2.4	9	2	80	2	0.2
RFID [10]	0.900	2.4	?	26	–	0.14
ATMEL [11]	2.4	50	?	?	–	1.63

marizes related experimental work, frequency f_R , communication range R_{comm} , instantaneous signal bandwidth BW_{sym} , corresponding ranging precision σ_{ToF} , virtual coherent multi-channel bandwidth BW_{virt} and its ranging precision σ_{PoF} .

While [8] uses the Channel State Information (CSI) of commodity WiFi cards to extract relevant phase information, inphase/quadrature (IQ) data is processed on the FPGA in [9], [12] and stored for post processing in [10]. This latter approach, feasible for short packet transmissions, generates large amounts of data with narrowband LPWAN signals.

The present work aims to transpose the concept of coherent multi-channel ranging to LPWAN systems with signal bandwidths of $BW_{\text{sym}} = 10$ kHz.

The contributions of this paper, to investigate the feasibility of coherent multi-channel ranging experimentally, are:

- A transceiver testbed, comprising a radio front-end and a FPGA performing digital up- and down-intermediate frequency mixing to reduce sampling rate while maintaining phase coherence over the virtual multi-channel bandwidth and IQ sample recording for post processing.
- Software simulations on top of the testbed to develop and benchmark ranging algorithms.
- Preliminary experimental results demonstrating coherent multi-channel ranging performances in a cabled frequency flat AWGN channel as function of noise.

This paper is organized as follows. Measurement principles and a basic ranging algorithm are outlined in Section II. The developed testbed architecture is described in Section III. Section IV gives simulation and experimental results, while Section V concludes with a perspective on further work.

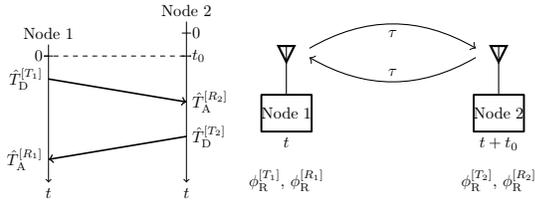


Fig. 1. Two-way time-of-flight (ToF) and phase-of-flight (PoF) measurement.

II. COHERENT MULTI-CHANNEL RANGING

A. Measurement principle

The round trip time-of-flight (ToF) ranging measurement, as depicted in Fig. 1 can be expressed as follows

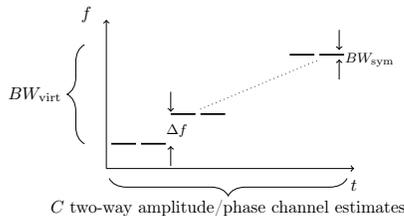
$$\begin{aligned} \text{ToF} &= (\hat{T}_A^{[R_1]} - \hat{T}_D^{[T_1]}) - (\hat{T}_D^{[T_2]} - \hat{T}_A^{[R_2]}) \\ &= (\hat{T}_D^{[T_2]} - t_0 + \tau) + (\hat{T}_D^{[T_1]} + t_0 + \tau) - (\hat{T}_D^{[T_2]} + \hat{T}_D^{[T_1]}) \\ &= 2\tau. \end{aligned} \quad (1)$$

A two-way packet exchange [13] is required in order to eliminate unknown relative time reference t_0 on time of arrival (ToA) measurements $\hat{T}_A^{[X]}$. Transmission times $\hat{T}_D^{[X]}$ are known. Combining phase measurements $\hat{\phi}_c^{[X]}$ results in the phase-of-flight estimate (PoF_c) at channel frequency $c\Delta f + f_R$

$$\begin{aligned} \text{PoF}_c &= \hat{\phi}_c^{[R_2]} + \hat{\phi}_c^{[R_1]} \\ &= \left(-2\pi c\Delta f t_0 - 2\pi(c\Delta f + f_R)\tau + \phi_R^{[T_1]} - \phi_R^{[R_2]} \right) \\ &\quad + \left(2\pi c\Delta f t_0 - 2\pi(c\Delta f + f_R)\tau + \phi_R^{[T_2]} - \phi_R^{[R_1]} \right) \\ &= -2 \cdot 2\pi(c\Delta f + f_R)\tau + \Delta\phi_R. \end{aligned} \quad (2)$$

with carrier frequency f_R . A full description including carrier frequency offset (CFO) is given in [7]. CFO influence on ToF and PoF is neglected in the following. A multi-channel ranging packet exchange in the time-frequency domain is depicted in Fig. 2. A narrowband two-way exchange with an instantaneous waveform bandwidth BW_{sym} is performed on C channels sequentially, equivalent to sampling the channel transfer function $H(f)$. With channel intermediate frequency spacing Δf , a total virtual coherent multi-channel bandwidth $BW_{\text{virt}} = (C-1)\Delta f$ is covered. Range information can be extracted from the slope of the set PoF_c with $c \in [1 \dots C]$

$$d_{\text{PoF}} = \tau c_0 = -\frac{c_0}{4\pi\Delta f} \cdot \frac{\Delta\text{PoF}_c}{\Delta c} \quad (3)$$


 Fig. 2. Multi-channel ranging protocol aggregating C sequentially transmitted narrowband signals (BW_{sym}) to a virtual bandwidth $BW_{\text{virt}} = (C-1)\Delta f$.

with speed of light c_0 . The channel transfer function¹ can be reconstructed by

$$H(f)|_{(f=c\Delta f+f_R)} = \hat{A}_c e^{j\text{PoF}_c} \quad (4)$$

with amplitude estimates $\hat{A}_c = \hat{A}_c^{[R_1]} \cdot \hat{A}_c^{[R_2]}$. Hence, in multipath scenarios it is preferred to convert $H(f)$ to the channel impulse response

$$h(t) = \int_{-\infty}^{\infty} H(f) e^{-j2\pi ft} df \quad (5)$$

with the discrete inverse Fourier transform (iFFT). In order to detect the first path, a simple detection scheme identifies the first local maximum above a certain threshold γ relative to and in a certain range R_{first} before the global maximum in the channel impulse response $h(t)$.

Applying such a processing scheme, the following issues need to be considered [5]:

- *Range resolution:* $\Delta R = c_0/(2(C-1)\Delta f) = c_0/(2BW_{\text{virt}})$. Maximize bandwidth BW_{virt} for high range resolution and to distinguish close multipath.
- *Range ambiguity, temporal aliasing:* The phase based range measurement is ambiguous as the channel transfer function $H(f)$ is sampled with frequency spacing Δf . Therefore the reconstructed channel impulse response $h(t)$ becomes periodic with $R_{\text{max}} = c_0/(2\Delta f)$. Adapted system parameter design allows resolving ambiguities with two-way time based ranging measurements [14]. Furthermore, multipath components could potentially appear before the first path. Therefore the maximum unambiguous range R_{max} should be greater than the largest significant multipath component.

B. Ranging metric extraction algorithm

A BPSK signal s_0 of bit rate $R_b = 10 \text{ kbit/s} \equiv BW_{\text{sym}} = 10 \text{ kHz}$ has been assumed in this study. A Gold code preamble of length 32 assures good correlation for synchronization.

On each received signal $r_c^{[X]}$, as described in Section III, the algorithm depicted in Fig. 3 is applied. CFO $\hat{k}_c^{[X]}$ is estimated on the preamble sequence using an algorithm from [15]. Required time synchronization is achieved by differential detection. The CFO corrected signal is correlated with the transmit BPSK waveform s_0 . Time of arrival $\hat{T}_{A,c}^{[X]}$, amplitude $\hat{A}_c^{[X]}$ and phase $\hat{\phi}_c^{[X]}$ are extracted from the correlation peak.

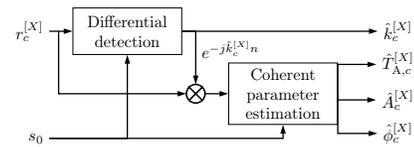


Fig. 3. Ranging metric extraction algorithm.

After processing over C channels, the set $\{\hat{k}_c^{[X]}, \hat{T}_{A,c}^{[X]}, \hat{A}_c^{[X]}, \hat{\phi}_c^{[X]}\}$ with $X \in [R_1, R_2]$ is available for further post processing and range extraction.

¹Due to two-way ranging the square of the channel transfer function $H^2(f)$ is measured [12].

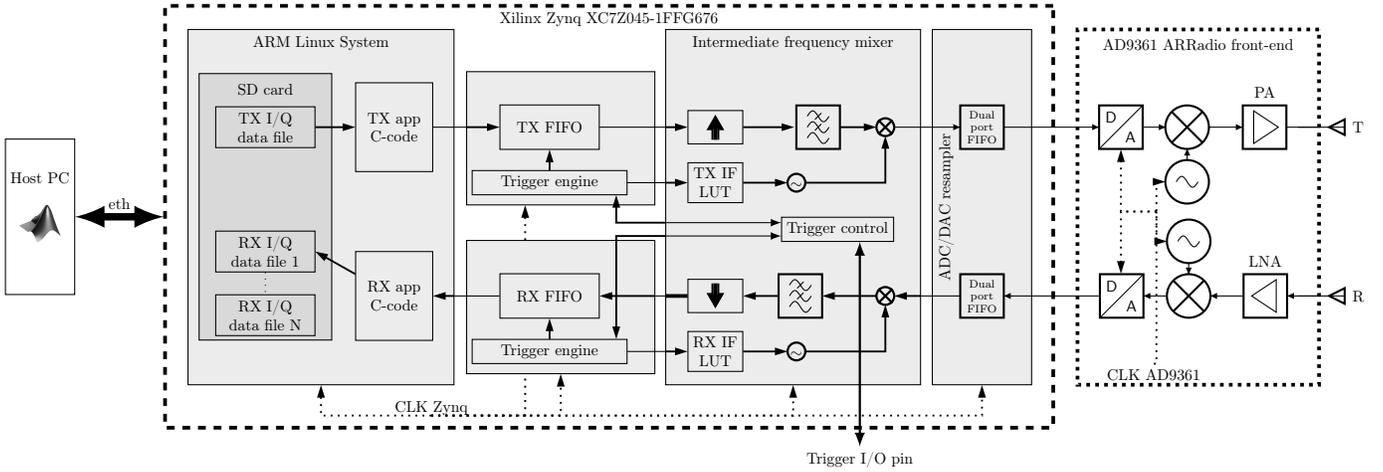


Fig. 4. SDR based coherent multi-channel ranging testbed architecture.

III. TRANSCEIVER DESIGN

The implementation of a coherent multi-channel ranging testbed is based on a software defined radio (SDR) platform comprising an *Analog Devices AD9361* 2×2 TRX radio front end and a *Zynq-045 Xilinx System on chip FPGA* which integrates a dual Cortex-A9 ARM processor.

Fig. 4 shows the testbed architecture with the digital up-/down-mixing stages implemented into the FPGA allowing to coherently process a 10 MHz bandwidth by sequentially selecting 1 MHz channels. The processor is dedicated to configuration purposes (RF/digital) as well as to transmit/receive IQ samples. The samples are in a second time processed by a dedicated software.

In the following the different parts of the testbed and their settings are explained in detail.

A. AD9361 ARRadio front end configuration

The radio front end is configured to maintain transmitter (TX) to receiver (RX) oscillator phase coherence by continuous operation of TX and RX phase lock loops (PLL) during the C two-way packet exchanges. TX and RX local oscillator frequency is set to $f_R = 868$ MHz, resulting in identical carrier frequency as both PLLs are driven from the same external clock². Initial phases $\phi_R^{[X]}$ are arbitrary but constant. The automatic gain control (AGC) in the receiver is set to manual operation with a fixed gain to avoid delay and phase changes during the IQ data acquisition.

The 12 bit analog-to-digital converter (ADC) and the 12 bit digital-to-analog converter (DAC) are set to sampling rate $f_{s,IF} = 20$ MHz.

B. FPGA design - Digital up-/down-mixing stages

A first resampling stage acts as interface between the DAC/ADC and the digital up-/down-mixing blocks and adapts sampling frequency between the DAC/ADC and the FPGA processing.

²VCTCXO 40 MHz (TXEAACSANF) with frequency accuracy of 2 ppm.

The following blocks are performing a factor 20 up-/down-sampling and an intermediate frequency (IF) mixing. Intermediate frequency mixing is performed with a cordic that mixes N_S IQ samples to frequency $c\Delta f$ before changing to the next channel frequency in the look-up-table (LUT). Hence phase coherence between channel frequency switching is maintained. Synchronizing the TX/RX FIFOs with frequency selection enables coherent processing.

TX and RX IQ streams ($f_{s,BB} = 1$ MHz) are buffered by large FIFOs between the FPGA and the ARM. The FIFOs can be triggered by 1) software (ARM controlled), 2) external GPIO pin or 3) onboard button. Perfect TX/RX intra-testbed synchronization is guaranteed by using the same trigger source. 1), 2) enable coarse inter-testbed time synchronization to limit acquisition time and to avoid the need to perform online synchronization between nodes on the radio signals.

The ARM processor runs TX and RX applications to manage IQ sample streams between the SD card and the FIFOs. The applications can be configured in master or slave mode to either initiate periodic two-way exchanges or to wait for the master via the trigger source.

C. Received signal model

The signals theoretically obtained in the RX FIFO of this transceiver design³ according to [7] are described by

$$r_c^{[X]}[n] = A_c^{[X]} s_0 \left(\frac{n}{f_{s,BB}} - T_{A,c}^{[X]} \right) e^{j(k_c^{[X]} n + \phi_c^{[X]})} + n_c^{[X]}[n] \quad (6)$$

with $n \in [0 \dots N_S - 1]$ and noise $n_c^{[X]}$.

IV. APPLICATION

A. Simulation setup and results

1) *Setup*: MATLAB simulations are conducted to develop and benchmark the ranging algorithms (see Section II) con-

³Neglecting jitter, ADC/DAC and IF mixer imperfections.

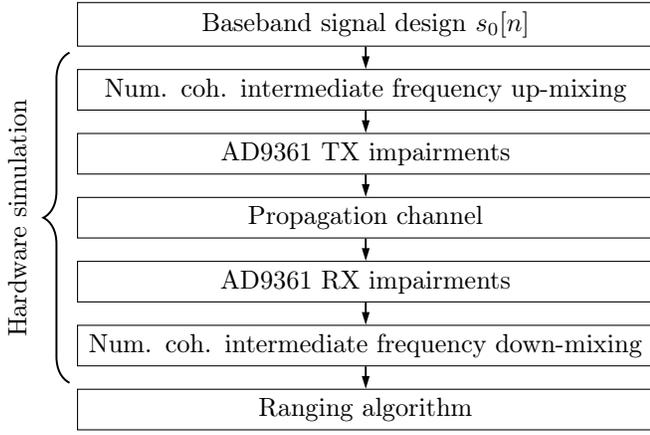


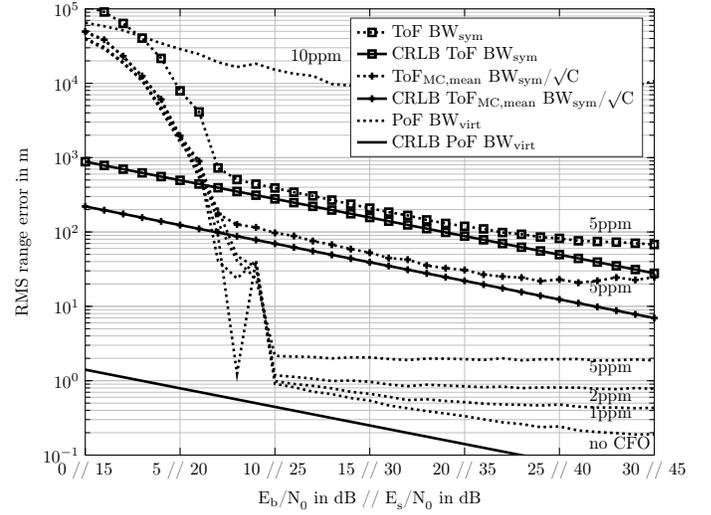
Fig. 5. Ranging algorithm benchmarking setup with simulated testbed signals.

sidering impairments introduced by digital intermediate frequency mixing (quantization, finite phase accuracy in cordic), radio front-end impairments and the influence of the propagation channel as depicted in Fig. 5. Digital coherent intermediate frequency up-/down-mixing blocks produce bit-identical outputs of the FPGA design. The AD9361 TX/RX blocks simulate unknown initial phase $\phi_{R,c}^{[X]}$, unknown relative time reference t_0 and CFO $k_c^{[X]}$. Time-of-flight delay τ and multipath are included in the propagation channel block.

In the following, single channel time-of-flight (ToF) based ranging (1) is compared to multi-channel (MC) time-of-flight (ToF_{MC}) and the phase coherent multi-channel (PoF) (5) techniques. Simulations are conducted for a frequency flat channel and the ETSI typical urban (Tux) channel model [16] with root-mean-square (RMS) delay spread $\tau_{\text{rms}} = 0.5 \mu\text{s} \equiv 150 \text{ m}$. Ranges are simulated between 0 m and 4 km. A channel spacing of $\Delta f = 200 \text{ kHz}$ and a total number of $C = 16$ channels give $BW_{\text{virt}} = 3.0 \text{ MHz}$ and result in a maximum unambiguous range $R_{\text{max}} = 750 \text{ m}$ with a range resolution of $\Delta R = 50 \text{ m}$. This parameter choice derives from an empirical trade-off between multipath and range ambiguity resolvability as well as keeping system complexity reasonable (required packet transmissions $2C$). Simulation results are averaged over 10^3 independent realizations.

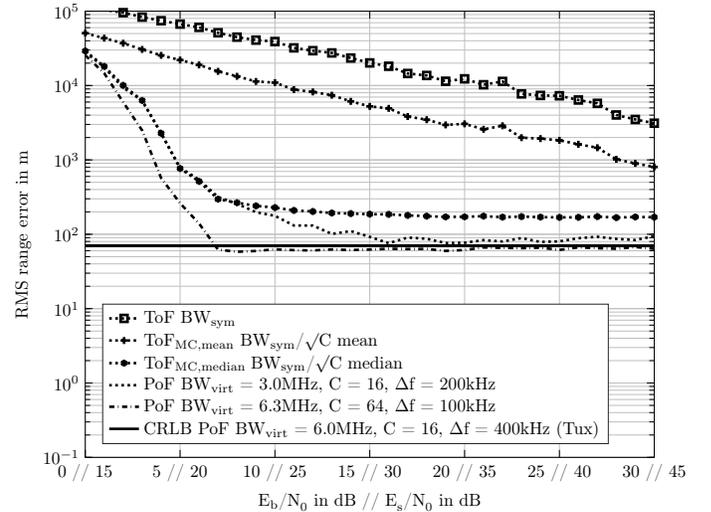
2) *Frequency flat channel*: Fig. 6 shows RMS ranging error over preamble symbol (Gold sequence of length 32) energy to noise spectral density (E_s/N_0) and equivalent BPSK E_b/N_0 in a frequency flat channel for a signal bandwidth $BW_{\text{sym}} = 10 \text{ kHz}$. For both, time and phase based, ranging techniques at low E_s/N_0 CFO estimation does not provide sufficient accuracy for correct ranging parameter estimation. Single channel time-of-flight (ToF) ranging and averaging over the C available time-of-flight measurements (ToF_{MC,mean}) levels out for high E_s/N_0 due to the limited sampling frequency $f_{s,\text{BB}} = 1 \text{ MHz}$ giving an uniform distributed sampling resolution error [13]

$$\sigma_{\text{ToF},f_{s,\text{BB}}} = \frac{\sigma_{\text{ToA},f_{s,\text{BB}}}}{\sqrt{2}} = \frac{c_0}{\sqrt{2}\sqrt{12}f_{s,\text{BB}}} \approx 61 \text{ m}. \quad (7)$$


 Fig. 6. Simulated ranging error in a frequency flat channel with a signal bandwidth $BW_{\text{sym}} = 10 \text{ kHz}$, $C = 16$ channels, a virtual multi-channel bandwidth $BW_{\text{virt}} = 3.0 \text{ MHz}$ and a sampling frequency $f_{s,\text{BB}} = 1 \text{ MHz}$.

Phase coherent processing (PoF) improves by one order of magnitude compared to time based approaches at equal energy. For no CFO estimation and high E_s/N_0 , a level out at 0.2 m due to the channel impulse response $h(t)$ range binning is observed. This can be controlled by appropriate IFFT zero padding in (5). Improvements are expected if CFO errors are compensated in future algorithms. Straight lines represent corresponding Cramer Rao lower bounds (CRLB) [6], [7].

3) *Multipath channel*: Simulation results for the ETSI typical urban (Tux) multipath scenario with a $BW_{\text{sym}} = 10 \text{ kHz}$ signal are depicted in Fig. 7. For first path detection (Section II-A), empirically determined threshold $\gamma = -7 \text{ dB}$ and range $R_{\text{first}} = 300 \text{ m}$ showed best performances. These


 Fig. 7. Simulated ranging error in the ETSI typical urban (Tux) channel with a signal bandwidth $BW_{\text{sym}} = 10 \text{ kHz}$, 1 ppm CFO and a sampling frequency $f_{s,\text{BB}} = 1 \text{ MHz}$.

values are in coherence with the Tux channel model characteristics delay spread and path gain ratio. Globally, ranging precision degrades compared to the frequency flat channel.

A closer study of the set of C time-of-flight measurements reveals that range is over-estimated due to multipath and hence resulting in a positive biased ranging error. For a frequency flat channel no bias is observed. Therefore, the median ($\text{ToF}_{\text{MC},\text{median}}$) over the C time-of-flight estimates drastically improves the ranging accuracy in multipath scenarios compared to averaging ($\text{ToF}_{\text{MC},\text{mean}}$). Coherent multi-channel performances, with range ambiguity resolved by the median time-of-flight range, show a small improvement compared to the time based approach. Increasing the number of utilized channels $C = 64$ with a frequency spacing $\Delta f = 100$ kHz, further improves coherent multi-channel performances. Whereas, the median on time-of-flight estimates ($\text{ToF}_{\text{MC},\text{median}}$) does not improve with more channels C . Coherent multi-channel precision approximately reaches the multipath CRLB [7].

B. Experimental setup and results

1) *Setup*: The experimental setup for two-way phase coherent multi-channel ranging is depicted in Fig. 8. A variable attenuator with attenuation $A_{\text{V,dB}}$ allows to control received power $P_{\text{RX,dBm}}$. The TX power is fixed to $P_{\text{TX,dBm}} = -71.5$ dBm. The receiver low noise amplifier (LNA) is set to maximum gain, resulting in a minimum noise figure $NF_{\text{dB}} = 2.5$ dB according to the datasheet. E_b/N_0 and attenuation $A_{\text{V,dB}}$ are linked as follows

$$\begin{aligned} \frac{E_b}{N_0} &= P_{\text{TX,dBm}} - A_{\text{V,dB}} \\ &\quad - (kT)_{\text{dBm/Hz}} - R_{\text{b,dBHz}} - NF_{\text{dB}} \\ &= 60 \text{ dB} - A_{\text{V,dB}}, \end{aligned} \quad (8)$$

with Boltzmann constant k and system temperature T , $(kT)_{\text{dBm/Hz}} \approx -174$ dBm/Hz. Experimental results are averaged over 10^2 acquisitions.

2) *Delay and phase calibration*: In order to account for unknown digital filter- and analog delays in the AD9361 TRX as well as to adjust for unknown radio front-end transfer functions, an one-time (factory) calibration measurement is

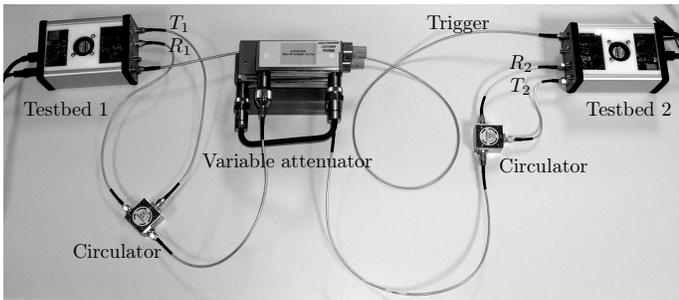


Fig. 8. Experimental setup for coherent multi-channel two-way ranging in a cabled frequency flat AWGN channel.

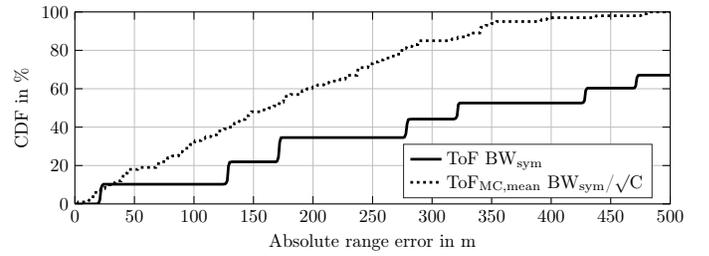


Fig. 9. Measured time-of-flight (ToF) range error and averaged time-of-flight ($\text{ToF}_{\text{MC},\text{mean}}$, $C = 16$) error at $E_b/N_0 = 10$ dB.

performed. Delay and phase shift over C channels are determined at $E_b/N_0 = 20$ dB and corrected on the following measurements to be range bias free.

3) *Frequency flat channel*: Fig. 9 shows the cumulative distribution function (CDF) for single channel time-of-flight (ToF) ranging error as well as the averaged ToF_{MC} over $C = 16$ channels. The sampling resolution due to the baseband sampling frequency is visible in form of a 150 m step motif in the CDF. Averaging decreases the error and smooths the CDF.

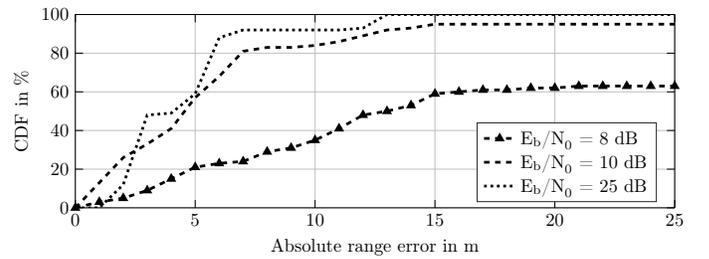


Fig. 10. Measured multi-channel phase-of-flight (PoF) range error.

Phase-of-flight (PoF) ranging errors are, for sufficient high E_b/N_0 , more than ten times smaller than ToF ranging errors as illustrated by the CDFs in Fig. 10.

Fig. 11 compares experimental measurements to CRLBs. For low E_b/N_0 ranging fails due to insufficient CFO estimation accuracy. For high E_b/N_0 ToF based ranging levels out at the sampling resolution error.

Resolving the PoF range ambiguity with the $\text{ToF}_{\text{MC},\text{mean}}$ measurement [14] fails in 10% of the cases due to time-of-flight errors larger than the range ambiguity (compare Fig. 9). As a result, the estimated and resolved PoF range is wrong by a multiple of R_{max} for $E_b/N_0 \in [10 \text{ dB}, 22 \text{ dB}]$, giving a large RMS error. An optimized and higher PoF range ambiguity R_{max} or adequate filtering can reduce the amount of these errors. Despite this, unresolved PoF ranging performs by a factor 10 better than ToF_{MC} , where equal symbol energy is employed. PoF ranging levels out due to non-compensated and time variant CFO induced errors as well as oscillator jitter.

4) *Localization coverage*: Results can be extrapolated to relate coverage and precision of the localization function. Defining the time-of-flight and phase-of-flight ranging accuracies $\sigma_{\text{ToF}} = 200$ m and $\sigma_{\text{PoF}} = 10$ m at $(E_b/N_0)_0 = 10$ dB

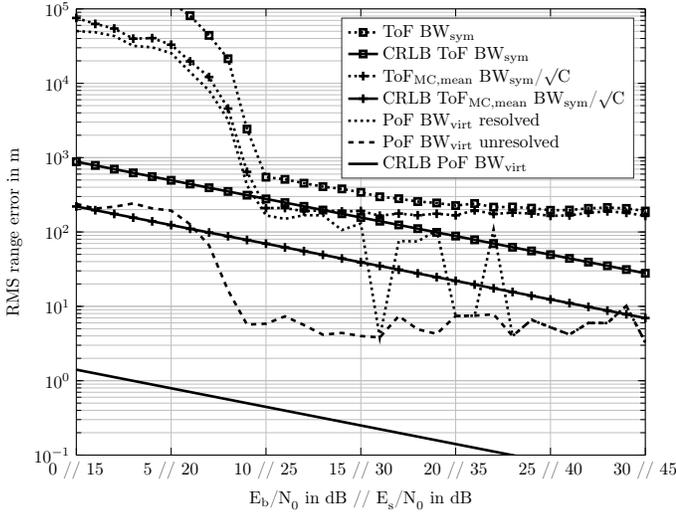


Fig. 11. Measured ranging error in a frequency flat channel with a signal bandwidth $BW_{\text{sym}} = 10$ kHz, $C = 16$ channels, a virtual multi-channel bandwidth $BW_{\text{virt}} = 3.0$ MHz and sampling frequency $f_{s, \text{BB}} = 1$ MHz.

as nominal ranging and also localization performances, localization coverage can be given. The receiver sensitivity is

$$\begin{aligned} S_{\text{dBm}} &= \left(\frac{E_b}{N_0} \right)_{0, \text{dB}} + (kT)_{\text{dBm/Hz}} + R_{b, \text{dBHz}} + NF_{\text{dB}} \\ &= 10 \text{ dB} + 40 \text{ dBHz} - 174 \text{ dBm/Hz} + 2.5 \text{ dB} \\ &= -121.5 \text{ dBm}. \end{aligned} \quad (9)$$

Link budget is $L_{\text{dB}} = P_{\text{TX, dBm}} - S_{\text{dBm}} = 14 \text{ dBm} - (-121.5 \text{ dBm}) = 135.5 \text{ dB}$. According to the Hata propagation loss models [17] with 15 m base station and 1 m LPWAN radio module antenna height, a maximum coverage $R_{\text{comm}} = 2.5$ km for the *suburban* and $R_{\text{comm}} = 7$ km for the *open rural* propagation conditions can be achieved.

V. CONCLUSION

In this paper simulation results and preliminary experimental coherent multi-channel ranging measurements obtained with a software defined radio based ranging testbed have been presented. Precision for phase based ranging techniques improve by factor 10 to 20 compared to the time based ranging method for equal employed energy. Ranging precisions down to 10 m are achieved with a 10 kHz signal and phase coherent multi-channel processing. Simulation and experimentation results agree with theoretical bounds. Algorithms perform suboptimal due to non-compensated carrier frequency offset.

Future investigation is necessary to develop adequate algorithms to compensate these errors as well as to improve range estimation in multipath scenarios. In order to understand the conditions when phase based techniques outperform classical time based approaches further simulations considering spatial filtering are required. A testbed setup with directional antennas or a multi antenna setup using the two receiver channels of the radio front end will be used to validate performances

experimentally on a channel emulator and with outdoor measurements.

Complexity of multi-channel ranging can potentially be addressed by considering non-uniform channel spacing or time difference of arrival (TDoA) like approaches where the nodes become transmitter only and the base stations perform required metric estimation and range calculation.

Moreover, raw IQ data or extracted ranging metrics and the corresponding ground truth could serve as input to machine learning or deep neural network based algorithms which potentially provide, without explicit knowledge of the underlying signal model, precise ranging estimates from narrowband LPWAN radio signals.

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