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Energy Recovery DC/AC Converter for Piezoelectric Transformer

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Keywords

«Piezoelectric transformer», «Recovery energy», «DC/AC converter», «Power supply», «Transducer».

Abstract

Piezoelectric transformers have been used successfully in DC/AC or DC/DC converter. However, the use of piezoelectric transformers presents a major challenges for power electronic design: the capacitive nature of such devices makes their use delicate as the instantaneous power may be much greater than the average effective power. Due to this challenge, conventional drive circuits, especially inductor, become too bulky. This work describes a converter suitable to drive piezoelectric transformer with low inductor. The proposed converter is a DC/AC structure, which is capable of producing a unipolar square voltage. The circuit provides for recovery of the energy stored on the clamped capacitance back to the primary power supply when the transformer is de-energized. In our design, an auxiliary shunt circuits are connected to the input terminal. The proposed structure of both theoretical and experimental validations has demonstrated the effectiveness of the proposed technique for recovery energy.

Introduction

Piezoelectric transformers (PT) have several advantages compared to conventional magnetic transformers: low housing profile, no winding, high power density, high operating frequency and they are suited for automated manufacturing. However, power electronics for PTs are more complex. The PT requires a switching driving circuit to generate the structure vibration. Due to the capacitive nature of such devices, reactive power and power factor optimization have recently been the subject of numerous investigations [1]–[8]. Accordingly, power converters always need to supply high levels of reactive power, or equivalently high power peaks compared to average power, leading to an overdesign of power amplifiers, especially the magnetic component like inductor. To reduce the switching losses and the high power peaks compared to average power, a wideband zero-voltage-switching (ZVS) half-bridge circuit can be introduced [9]. To achieve the ZVS condition, a bulky inductor or an inductive matching network is typically required in the driving circuit [10]–[16]. However, the added magnetic component sacrifices the size and the weight of the converter. Although an inductor-less half-bridge circuit is possible [17], it only exists in a narrow bandwidth near the resonance frequency of the piezoelectric element, which is not suitable in this application. To overcome this drawback and to recovery energy stored in the clamped piezoelectric capacitance, in this paper, an auxiliary shunt circuit is added at the half-bridge which enables us to decrease this

reactive energy and the overall size of the power converter. The auxiliary shunt circuit includes two switches and a small inductor. The inductance is not in the path of the major power flow, thus it is not designed with piezoelectric transformer drive frequency. The auxiliary circuit included the return of the electrical energy stored in the piezoelectric clamped capacitance back to the primary power supply when the transformer is turned off. The energy recovery was accomplished with high efficiency by using the resonance between the clamped capacitance and the inductor. This switching shunt technique consists in connecting the piezoelectric transformer to the shunt circuit for a brief time period. This connection leads to a smooth inversion of the piezoelectric voltage, which induces an energy transfer from capacitance to supply source. The consequences of such size reductions involve new opportunities for designing ultra compact, low-cost wide bandwidth power converter with piezoelectric transformers.

The paper is organized as follow: the second section summarizes the electrical behavior and drive requirements of the piezoelectric transformer. In section 3 and 4, the circuit topologies suitable for driving the transformer are presented. Finally, the last section concludes the paper.

Piezoelectric transformer model

The topology of the piezoelectric transformer is presented in Fig. 1. The PT is a stacked disk-type, operating in thickness mode. The multi-layers structure is composed of 4 input layers and 4 output layers. Primary and secondary layers are made of the same PZT material. Insulation layer is made of glass fiber. Table 1 details the layers thicknesses. The testing specimen was provided by Eleceram Technology Co., Ltd Taiwan.



Fig. 1: Pictures of the stacked disk-type piezoelectric transformer operating in thickness mode

Table I: Geometrical Dimensions of the PT

	Number of layers	Thickness	Radius
Input section	4	0.61mm	13mm
Output section	4	0.61mm	13mm
Insulation	2	0.41mm	13mm

Lumped model analysis of piezoelectric structures has received considerable attention since the 1970s, and the formulation presented by Alik and Hughes, based on the variational principle, is widely referenced. For simplicity, the model used in this paper has one degree of freedom. Indeed, a mechanical model based on only one degree of freedom gives a good description of the vibrating piezoelectric transformer behavior near one of its resonant frequencies.

The electric equivalent circuit of the transformer is shown in Figure 2. The circuit consists of a static part, which is represented by the clamped capacitances C_1 and C_2 , and a resonant branch, which is corresponding to the first mechanical vibration mode. In this equivalent circuit, n_1 and n_2 are the mechanical input and output transformation ratio, respectively. In the resonant branch, inductor L_m , resistor R_m and capacitor C_m are equivalent to the mass, the mechanical damping, and the stiffness of the first vibration mode, respectively. The current i_m flowing in the mechanical resonant branch is equivalent to the vibration velocity of the structure. The dielectric loss is neglected.

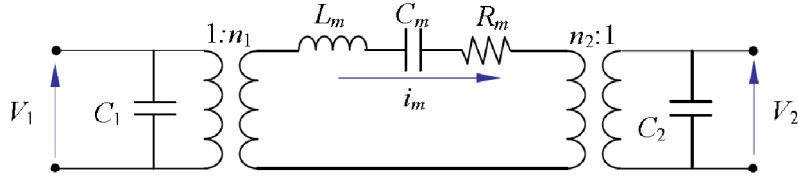


Fig. 2: Equivalent circuit of the piezoelectric transformer

The parameters of the equivalent circuit have been characterized and are summarized in Table 2. The resonance frequency of the transformer is 82.7 kHz.

Table II: Model parameters

Symbol	Description	Value (unit)
f	Operating frequency	82.7 kHz
n_2/n_1	Coupling ratio	1
C_m	Mechanical capacitance	92 pF
L_m	Mechanical inductance	40.3 mH
R_m	Mechanical resistance	10 Ω
C_1	Input capacitance	20 nF
C_2	Output capacitance	20 nF

DC/AC circuit with energy recovery

The typical topology of PT based DC/DC converter is shown in Fig. 3. The DC/AC input driving circuit excites the PT vibration. Then PT transfers the vibration energy to the output terminal. After passing through the rectifier, the DC voltage can be obtained. When the PT operated at fixed frequency, the mechanical current i_m in Fig. 2 can be assumed as a pure sinusoidal wave in the steady state. Accordingly, the mechanical current can be viewed as the sinusoidal current source into the rectifier. The rectifier is the typical full-wave rectifier.

The main objective of the this work is to study the input driving circuit (DC/AC converter) to reduce consumption of apparent power, to optimize the active power and to suppress the reactive power at working frequencies close to the resonant one. The main problem is the energy stored in the clamped capacitance C_1 of the transformer. This energy in capacitance is a reactive energy that must be managed to avoid to oversize the power supply. In addition, a square-driving signal will generate large losses in the switches. Therefore, a series or parallel inductor is typically added to the piezoelectric transformer to ensure the ZVS condition in the power stage, but the inductor is bulky in low frequency application. Accordingly, in this work a new circuit topology is proposed to limited reactive energy and to recover this energy.

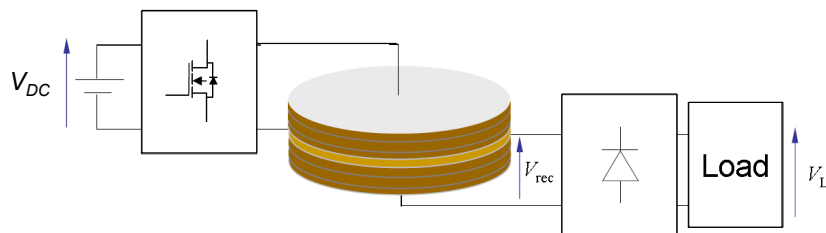


Fig. 3: Diagram of a DC/DC converter with piezoelectric transformer

The new circuit topology is shown in Figure 4. There are four n -channel power MOSFETs switches K_1 , K_2 , S_1 and S_2 . The switches K_1 and K_2 are operated as a half-bridge circuit. The transformer with input capacitance C_1 is connected to the middle point of the switches K_1 and K_2 . The half-bridge switches generate a trapezoidal waveform of the voltage v_l applied to the input terminal of the transformer. The input voltage v_l excites the mechanical vibration and induces the input current i_p . The vibration velocity of the transformer is equivalent to a virtually mechanical current i_m . Switches S_1 , S_2 and inductor L are also connected to the input terminal of the transformer. This shunt circuit is only switched-on during the dead time of the half-bridge for the recovery energy purpose. In practice, inductor L is small, so there is no bulk inductor in the implemented circuit. For simplicity, there are some assumptions for the understanding of this circuit: the parasitic capacitors of switches are neglected, as they do not influence the ZVS condition mainly led by the capacitance of the transformer.

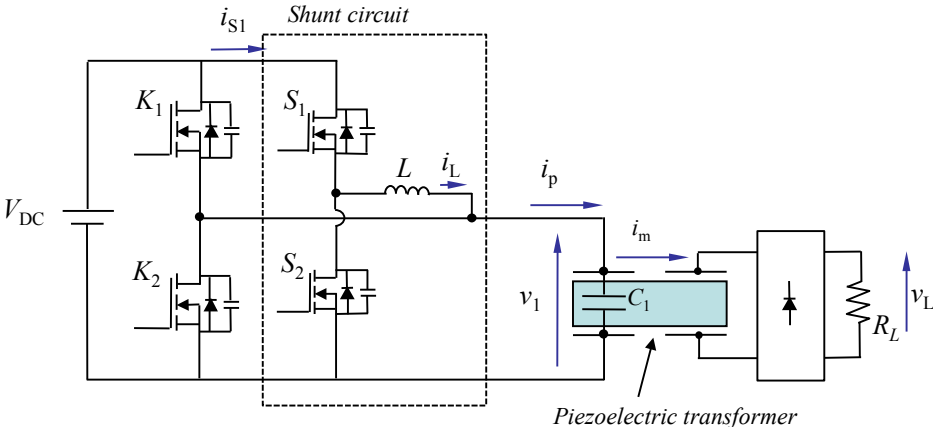


Fig. 4: Circuit topology of DC/AC proposed converter

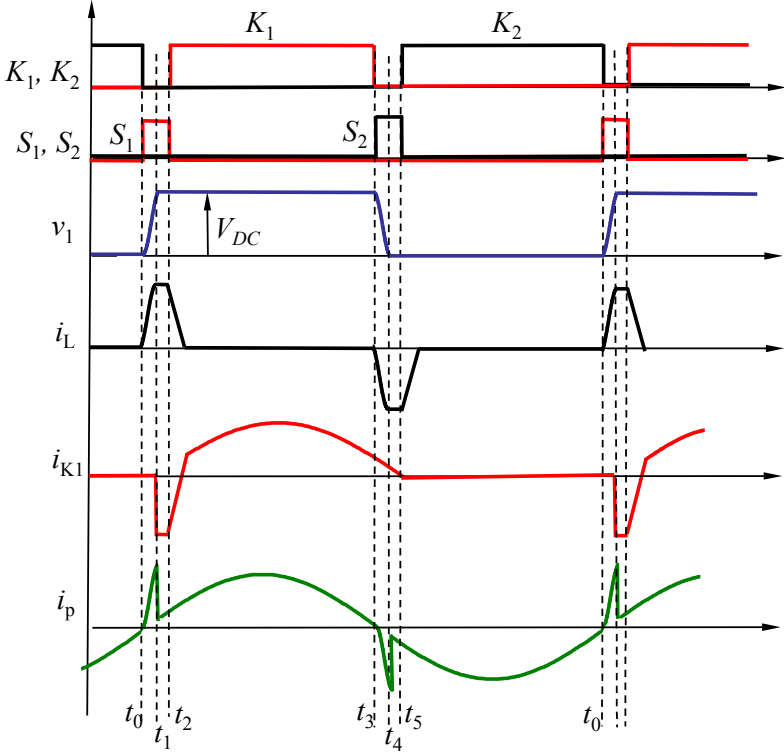


Fig. 5: Theoretical waveforms

Principle of operation

The principle of operation is explained with the aid of the ideal key-waveforms of the driving circuit operating at resonance frequency of transformer (Fig. 5). The circuit operation is mainly categorized into six steps:

Step 1 [$t_0 < t < t_1$] Figure 6-a: The high-side switch S_1 is ON and the switches K_1 , K_2 and S_2 are OFF. The capacitor C_1 is charged through the inductor L . It should be noted that capacitor C_1 contribute to the resonance with inductor L in this step. Voltage v_l increases sinusoidally until reaching V_{DC} and the current in inductor L increases until reaching $V_{DC}\sqrt{C_1/L}$. This step is the key of the ZVS condition for the low-side switch K_1 . If the charging time during the period is not large enough, capacitor C_1 cannot be fully charged to V_{DC} and the high-side switch K_1 cannot be turned ON at zero voltage in the following step. Therefore, this step must be larger than the period of resonance between L and capacitance C_1 :

$$t_1 - t_0 = \frac{\pi}{2} \sqrt{LC_1} \quad (1)$$

which is a quarter of the resonant period of the L- C_1 series resonant circuit. According to Eq. (1), a small inductance is required with the small time interval (t_1-t_0) under the given capacitances. This is the underlying reason why we can adopt a small value inductance. This step is over when capacitor voltage reaches V_{DC} , the body diode D_1 of switch K_1 automatically turns on and keeps the voltage across the capacitor at V_{DC} .

Step 2. [$t_1 < t < t_2$] Figure 6-b: During this step, switch S_1 is still ON and the switches K_1 , K_2 and S_2 are still OFF. The input voltage v_l is equal to V_{DC} . During this period, the body diode D_1 of switch K_1 is forward bias in order to support current i_L . The current in the inductor L will free wheel around the S_1 - L - D_1 loop. This step is over until switch K_1 is turned ON and S_1 is turned OFF.

Step 3. [$t_2 < t < t_3$] Figure 6-c: The high-side switch K_1 is ON and the low-side switch K_2 is OFF. The shunt circuits S_1 and S_2 are both OFF. During this period, the body diode of switches K_1 and S_2 are forward bias in order to support current i_L flowing back to power supply decreasing in time at a rate $L \frac{di}{dt} = V_{DC}$. The energy stored in the inductor L can be recovered to the power supply. In the same time, the sinusoidal mechanical current i_m is flowing through the switch K_1 and the transformer.

Step 4. [$t_3 < t < t_4$] Figure 6-d: The high-side switch K_1 is OFF and the low-side switch S_2 is ON. The capacitor C_1 is discharged through the inductor L . The discharge time is a quarter of the resonance period of the L- C_1 resonance circuit. This step is over when capacitor voltage reaches 0, body diode D_2 of switches K_2 automatically turns on. It is similar as step 1.

Step 5. [$t_4 < t < t_5$] Figure 6-e: During this step, switch S_2 are still ON. The body diode D_2 of switch K_2 is forward bias in order to support current i_L . The current in the inductor L will free wheel around the S_2 - L - D_2 loop. This step is over until switch K_2 is turned ON and S_2 is turned OFF. It is similar as step 2.

Step 6. [$t_5 < t < t_0$] Figure 6-f: The high-side switch K_1 is OFF and the low-side switch K_2 is ON. The shunt circuits S_1 and S_2 are both OFF. During this period, the body diode of switches K_2 and S_1 are forward bias in order to support current i_L flowing back to power supply, decreasing in time at a rate $L \frac{di}{dt} = V_{DC}$. The energy stored in the inductor L can be recovered to the power supply. In the same time, the sinusoidal mechanical current i_m is flowing through the switch K_2 and the transformer.

In brief summary, the main power switches K_1 and K_2 are turned ON in steps 3 and 6 respectively. During the other steps, switches K_1 and K_2 are both OFF, which are the dead time in the half-bridge circuit. In steps 1 and 4 the capacitor of the transformer is resonantly charged or discharged by the shunt circuits to achieve the ZVS conditions. Once they are achieved, the currents in the inductor of the shunt circuit are recovered in steps 3 and 6.

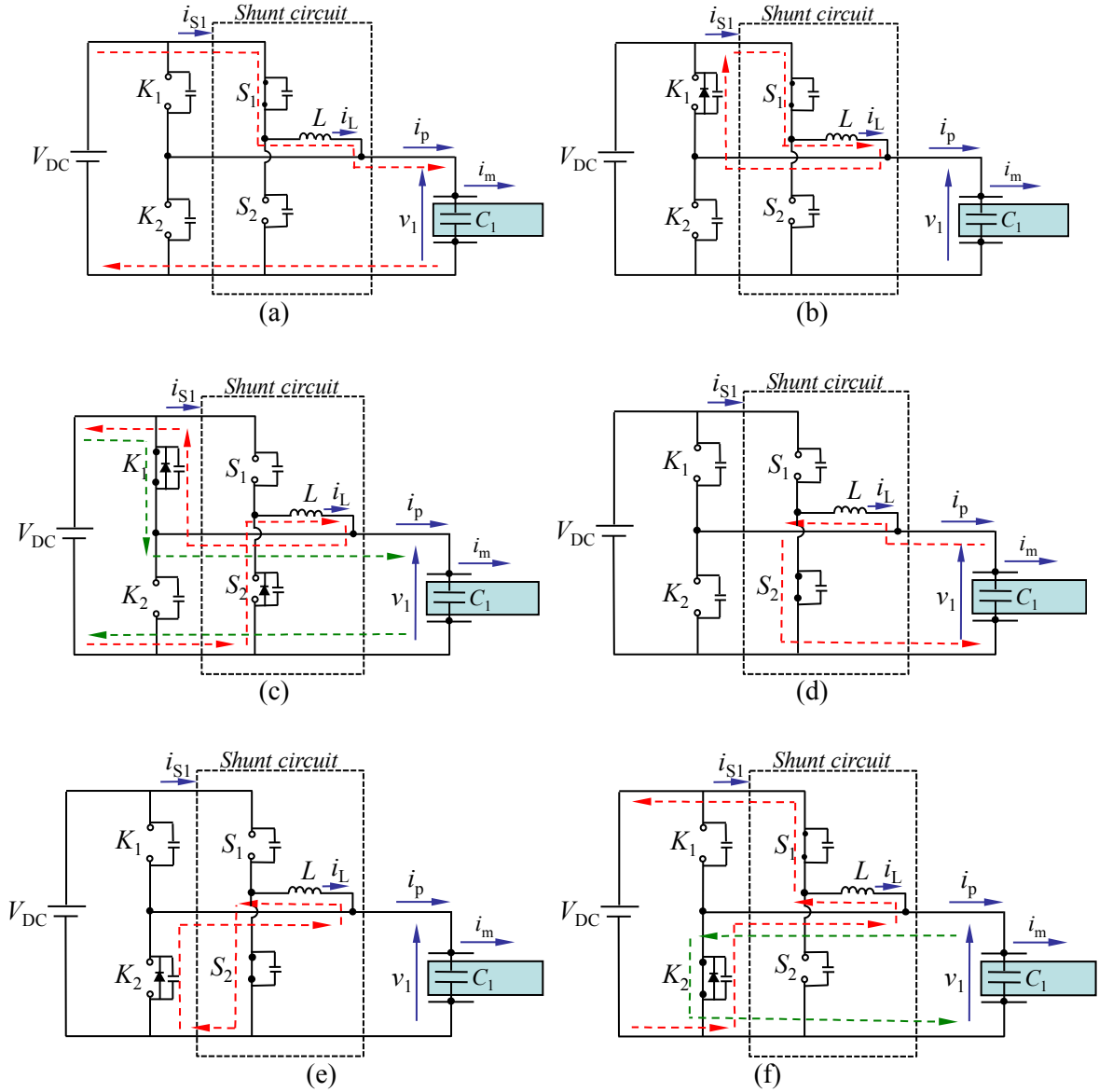


Fig. 6: Equivalent circuits of proposed DC/AC converter in different steps (a) Step 1 [t_0-t_1] (b) Step 2 [t_1-t_2] (c) Step 3 [t_2-t_3] (d) Step 4 [t_3-t_4] (e) Step 5 [t_4-t_5] (f) Step 6 [t_5-t_0]

Optimal value of inductor

To optimize the reactive energy in the system with decrease the input power source and in the same time to decrease the size of the inductor, the amplitude of the input current must be limited. In other words, the amplitude of current in auxiliary shunt circuits must be the same than the fundamental current at resonance of piezoelectric transformer. The amplitude of current in auxiliary shunt circuit is given by the resonance between L and C_1 , $I_S^{Max} = V_{DC}\sqrt{C_1/L}$. At the resonance the power supplied by the amplifier is given by:

$$P_{piezo} = V_1^{RMS} I_P^{RMS} = \frac{2V_{DC}}{\pi\sqrt{2}} \cdot \frac{I_m^{Max}}{\sqrt{2}} \quad (2)$$

Where V_1^{RMS} and I_P^{RMS} are the RMS value of the fundamental of the voltage v_1 and the RMS value of the piezoelectric mechanical current at the resonance respectively. I_m^{Max} is the magnitude of the mechanical current at the resonance. P_{piezo} is the active power at the input of the piezoelectric

transformer $P_{piezo} = \frac{2V_{DC}I_m^{Max}}{\pi}$. The optimal inductor is obtained when the magnitude of the current in auxiliary circuit is equal to magnitude of the mechanical current at the resonance.

$$L = C_1 \left(\frac{V_{DC}}{I_m^{Max}} \right)^2 \quad (3)$$

Experimental results

The experimental setup is shown in Figure 8, in which the tested piezoelectric transformer is shown Figure 1. The signal processing to generate pulse to drive the switches is performed by two monostables and two xor (Figure 7). All measuring signals are simply monitored using an oscilloscope. The following specifications and components were adopted in our experiment: $V_{DC} = 15$ V; the four switches K_1, K_2, S_1 and S_2 : IRF 640; load resistor $R_L = 22 \Omega$; constant dead time, *i.e.* $(t_2 - t_0)$ and $(t_5 - t_3)$: $0.8 \mu s$. The inductor value has been set in order to limit the spike current during quarter-period of the resonant instant (when the piezoelectric voltage changes from 0 to V_{DC} and from V_{DC} to 0) using equation (3). The objective is to minimize the apparent power, which appear when the piezoelectric clamped capacitance is charging or discharging. According to the value of clamped capacitance of 20 nF, a good performances are obtained with an inductor value of $5 \mu H$. All component values are shown in table 3.

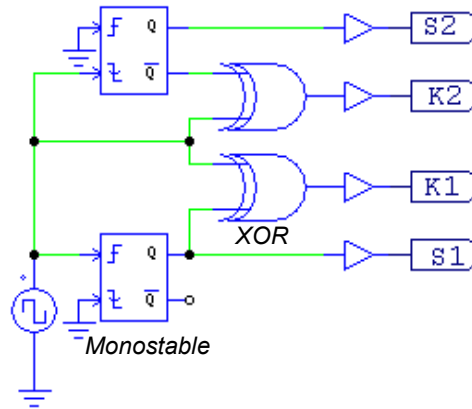


Fig. 7: Signal processing to drive switches

Table III: Component values

Symbol	Description	Value (unit)
K_1, K_2, S_1, S_2	Transistors MOSFET	IRF 640
L	Inductor	$5 \mu H$
V_{DC}	Input voltage	15 V
C_1	Piezoelement capacitance	20 nF
t_2-t_0 & t_5-t_3	Dead time	$0.8 \mu s$
	Monostable	4538
	XOR	4070
	MOS Driver	IRF 2108

Figures 9 to 11 show the experimental waveforms of S_1 and S_2 driving signals, piezoelectric voltage v_1 , inductor current i_L , and piezoelectric current i_p at the mechanical resonance 82.7 Hz. It can be seen that the experimental waveforms are in excellent agreement with the theoretical and simulation predictions. We have tested the converter with frequency range from 60 kHz to 100 kHz and a constant dead time, *i.e.* 0.8 μ s. The experimental results have verified that the proposed circuit can recover energy in a wide bandwidth without the use of a bulky inductor and thanks to a minor complication of the circuit with ancillary low losses semiconductors. The analysis of these figures leads to conclude that the auxiliary circuits, during dead time, charge and discharge the clamped capacitance trough inductor which justifies the reduction of the power consumption.

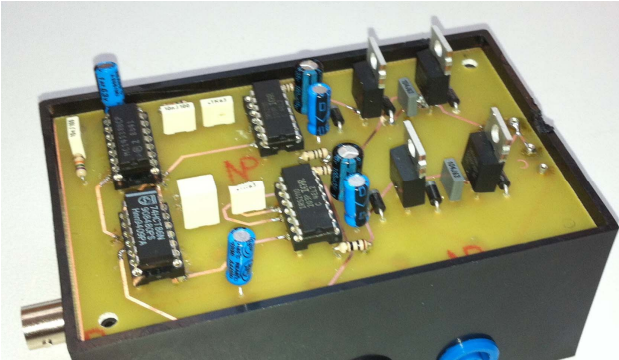


Fig. 8: Picture of the proposed DC/AC converter

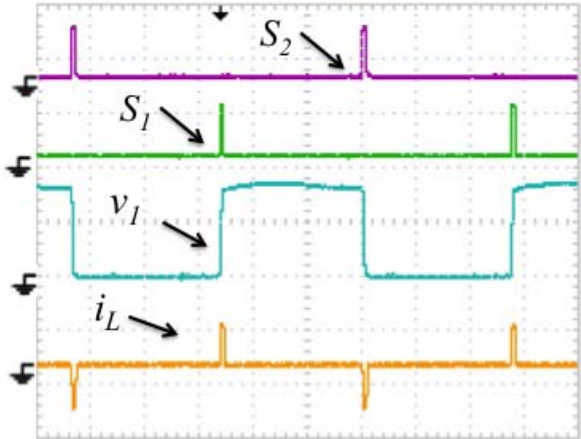


Fig. 9: Experimental waveforms: S_2 drive signal (10 V/div), S_1 drive signal (10 V/div), voltage v_1 (10V/div) and current i_L (500 mA/div)

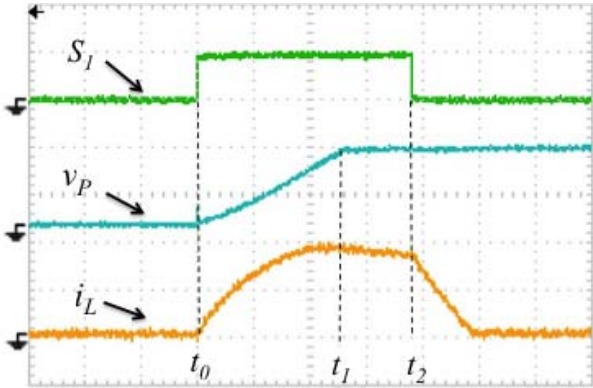


Fig. 10: Experimental waveforms during dead-time, *i.e.* ($t_2 - t_0$): S_1 drive signal (10 V/div), voltage v_1 (10V/div), current i_L (200 mA/div) and time (2 μ s/div)

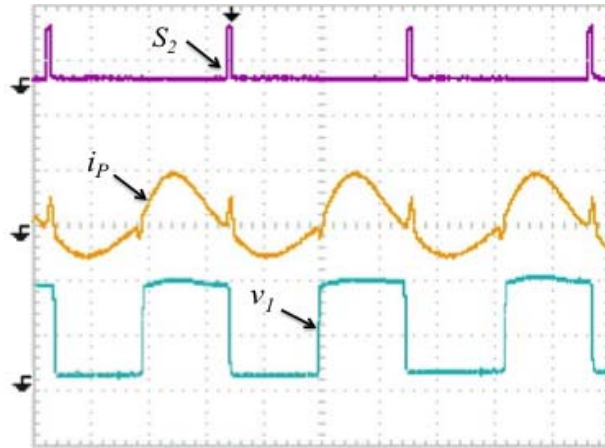


Fig. 11: Experimental waveforms: S_2 drive signal (10 V/div), current i_p (500 mA/div) and voltage v_1 (10V/div)

The experimental value of $(t_1 - t_0)$ which is quarter of the resonant period of the L- C_1 series resonant circuit is $0.5 \mu\text{s}$. Figure 12 shows the experimental active power versus frequency. The maximum power transmitted at the resonance is 3.9 W.

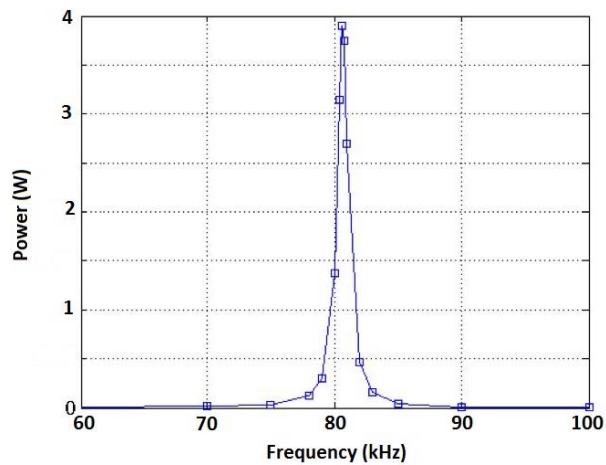


Fig. 12: Experimental output power

Conclusion

A new circuit for driving a piezoelectric transformer with quasisquare waveforms has been presented analytically and verified experimentally and includes recovery of the electrical energy stored in the capacitance of the piezoelectric transformer back to the primary power supply. A shunt circuit is connected to the input terminal to the transformer in order to enlarge the ZVS bandwidth of the typical half-bridge driving circuit. Since the ZVS condition can be achieved without any bulky inductor, the proposed circuit may be significantly smaller, which could be an advantage in some applications.

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