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Hieu Nguyen Huu, Laurent Gerbaud, Nicolas Rétière, James Roudet, Frédéric Wurtz. Analytical Modeling of Static Converters for optimal sizing of on-board electrical systems. VPPC 2010, Mar 2010, Lille, France. hal-00609598

HAL Id: hal-00609598

<https://hal.science/hal-00609598v1>

Submitted on 19 Jul 2011

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Analytical Modeling of Static Converters for optimal sizing of on-board electrical systems

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Abstract- Power electronics converters can generate a high level of harmonic perturbations on on-board electrical systems (planes, ships, road vehicles...). For the optimal sizing of these systems, harmonics must be known to select the best components (generator, filter...) that will limit their effects. In the paper, an analytical frequency domain modeling is proposed to accurately compute the harmonics generated the static converters. Because no numerical simulation is used, the presented approach is fast, accurate and applicable for optimal sizing or sensibility analysis. It is also valid for every kind of static converters. It is illustrated by its application to the sizing of an AC/DC power converter used for connecting electrical generators to DC on-board networks.

I. INTRODUCTION

Three-phase diode bridge rectifiers are often used in on-board systems (planes, ships, road vehicles...). Unfortunately, those converters also generate unwanted perturbations, especially electromagnetic perturbations in both common and differential conduction modes. Then, the design objectives of on-board systems shall include efficiency, mass or cost criteria but also shall take into account EMC (Electro Magnetic Compatibility) standards (for example [1]).

Numerical time simulation combined with FFT analysis can be used to calculate harmonics generated by power electronics converters [2]. This approach can be simply applied for modeling purposes and many algorithms have been developed to improve the quality of the results and to speed up the convergence [3],[4]. However, optimal design requires the use of optimization techniques and consequently numerous evaluations. If the evaluation consists in a FFT analysis following a time simulation then the optimal design may become very time consuming. In addition to that, if the system parameters change during the optimization, it might be difficult to manage correctly both the time simulation (e.g. the natural commutation times) and the parameters of the FFT algorithm (e.g. the window size). This generally gives wrong results. Thus a combined approach of time simulation and FFT is not suitable for the optimal design model of on-board electrical systems including numerous power electronics converters. Analytical modeling is preferred.

Several analytical harmonic modelings exist in the literature [5]-[8]. However, they often present some very restricting assumptions such as:

- resistive voltage drops are neglected at the input of the power converter [5],[6],
- only the modeling of controlled converters can be carried out [7],
- the modeling uses difficult-to-apply mathematical transformations [8].

These limitations have motivated the authors of the paper to develop a new approach which would be usable for every kind of static converter, especially the uncontrolled diode bridges which are very difficult to model because of the difficulty to know the switching times. This approach is fast, accurate, suitable for optimal design and easy to use. Basically, it is made of three steps:

- describing the converter by time-differential equations,
- calculating the switching times,
- computing the harmonics from the time-differential equations, the state variable values at the commutation times and the switching times.

The model will be used for the optimal design of an AC/DC converter used for the DC generation in transport vehicles [9]. The generation system is made of a three-phase synchronous generator connected to the primary energy sources (amplitude E_m , frequency $f_r = \omega r / (2\pi)$), a rectifier and a capacitor C_f on the DC link (Fig.1). The objective is to minimize the global mass of the power channel while fulfilling the DC output and the AC input harmonic standards.

In the next section, the modeling method is detailed step by step. The results given by the model are analyzed in section III.

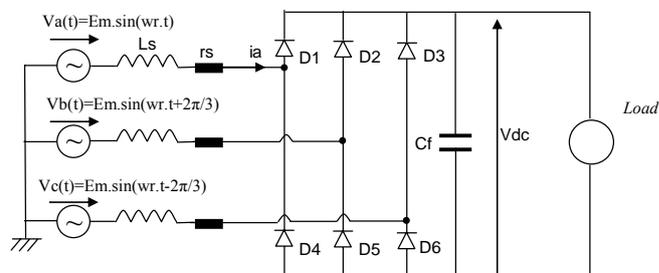


Fig.1. Structure of the studied power channel

II. MODELING METHOD

The following assumptions are made:

- the static converters operate in periodic steady state,
- the switches are ideal (at on state they are represented by a simple short-circuit and at off state by an open circuit), and their commutations are instantaneous,
- the passive components are linear.

It should be noted that the proposed approach is adapted to converters using uncontrolled or controlled commutation devices.

The approach is made of three steps:

- writing of the time-differential equations describing the operation of the power converter (II.A),
- computation of the switching times by the solving of a set of non-linear equations (II.B),
- Fourier-Transform of the time-differential equations (II.C).

A. Describing the converter by time-differential equations

According to the general laws ruling electrical circuits, the time-differential equations describing the converter can be expressed by:

$$\dot{X}(t) = A(t).X(t) + B(t).U(t) \quad (1)$$

$$Y(t) = C(t).X(t) + D(t).U(t) \quad (2)$$

(Elements description of these equations is presented in the table I.)

A power converter operates periodically with a period T . Thus:

$$\begin{aligned} A(t) &= A(t+T); B(t) = B(t+T); \\ C(t) &= C(t+T) \text{ and } D(t) = D(t+T) \\ X(t) &= X(t+T) \text{ and } Y(t+T) = Y(t); \end{aligned}$$

Over an operating period, the converter topology changes because of the commutations. On the other hand, it is assumed that the passive component values are constant. Thus, the matrixes A , B , C , D depend only on the topology but are constant for a given topology. For these reasons, the time-differential equations of each configuration k can be written as:

$$\dot{X}_k(t) = A_k.X_k(t) + B_k.U(t) \quad (3)$$

$$Y_k(t) = C_k.X_k(t) + D_k.U(t) \quad (4)$$

where $k=1..N_{sw}$,

with N_{sw} : total number of configurations encountered during the converter operating over a period.

During configuration k , the time t runs as: $t_{k-1} < t < t_k$.

Over a period, the time-differential equations are given by the time-addition of each phase:

$$X(t) = \sum_{k=1}^{N_{sw}} X_k(t).wind(t_{k-1}, t_k) \quad (5)$$

$$Y(t) = \sum_{k=1}^{N_{sw}} Y_k(t).wind(t_{k-1}, t_k) \quad (6)$$

$$\text{with } wind(t_{k-1}, t_k) = \begin{cases} 1 & \text{if } (t_{k-1} < t < t_k) \\ 0 & \text{otherwise} \end{cases}$$

TABLE I
ELEMENTS OF THE TIME-DIFFERENTIAL EQUATIONS

Nom	Description	Dimension
X	Time-differential vector	$n \times 1$
Y	Output vector	$p \times 1$
U	Input vector	$m \times 1$
A	State-space matrix	$n \times n$
B	Input matrix	$n \times m$
C	Output Matrix	$n \times n$
D	Coupling Matrix	$p \times n$
t	Time	1

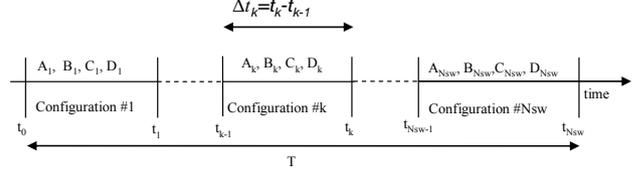


Fig.2. Representation of the converter configurations over an operating period

B. Calculating the switching times

1. Solution of the time differential equations

For configuration $\#k$, the solution of equations (3) and (4) is given by [10], [11]:

$$X_k(t) = e^{A_k.(t-t_{k-1})}.X_k(t_{k-1}) + \int_{t_{k-1}}^{t_k} e^{A_k.(t-\tau)}.B_k.U(\tau).d\tau \quad (7)$$

$$Y_k(t) = \begin{cases} C_k(e^{A_k.(t-t_{k-1})}.X_k(t_{k-1})) \\ + \int_{t_{k-1}}^{t_k} e^{A_k.(t-\tau)}.B_k.U(\tau).d\tau + D_k.U(t) \end{cases} \quad (8)$$

It should be noted that it is not necessary to calculate expression (8). Indeed, the components Y_k are given by a matrix combination of the time-differential vectors X_k ($k=1..N_{sw}$). Thus, only expression (7) has to be solved. For that purpose, the time intervals $[t_k, t_{k+1}]$ and the initial values $X_k(t_{k-1})$ have to be pre-determined.

2. Determination of the time intervals and the initial values

The time-differential vectors are time-continuous. So, it is possible to write (see Fig. 2):

$$X_k(t_{k-1}) = X_{k-1}(t_{k-1}) \quad (9)$$

As a consequence, the number of unknown variables to compute the time-differential vector is equal to $(N_{sw} + 1 + n)$:

- $N_{sw} + 1$ is the number of switching times ($t_0, t_1, \dots, t_{N_{sw}}$)
- n is the dimension of the time-differential vector X .

The $(N_{sw} + 1 + n)$ equations required to compute the unknown variables constitute a set of implicit equations which will have to be solved.

To write this equation system, the assumption of steady-state operation is first considered. It can be translated into an equality between the values of the time-differential vector at the beginning and the end of the operating period:

$$X_1(t_0) = X_{N_{sw}}(t_{N_{sw}}) \quad (10)$$

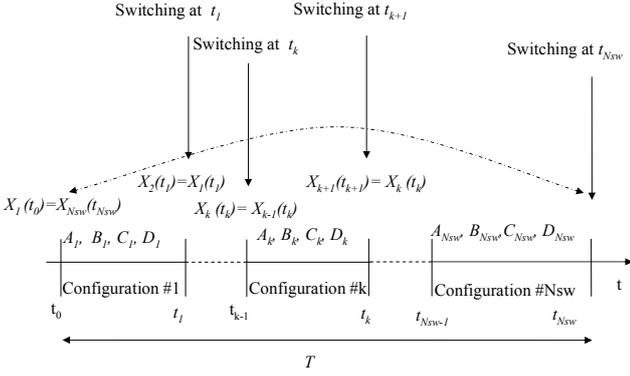


Fig. 3: State-space representation over an operating period

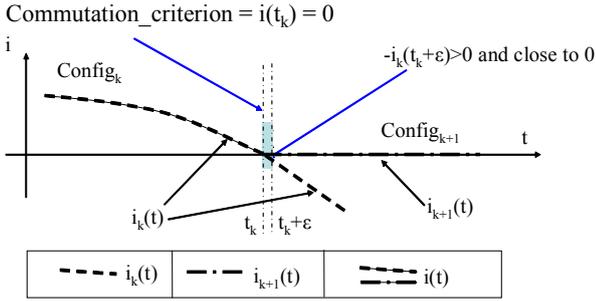


Fig. 4: Commutation criterion for the turning off of a diode

$$(i(t) \text{ is } i_k(t) \text{ if } t < t_k \text{ and } i_{k+1}(t) \text{ if } t > t_k)$$

This relation gives n equations because of the dimension of vector X .

Another relation to be respected concerns the definition of the operating period. It is given by:

$$t_{Nsw} - t_0 = T \quad (11)$$

And, besides, at every configuration change t_k , a set of equations has to be respected. It concerns the currents and voltages of all the switches which are commuting [12]. Fig.4 shows the example of the turning off of a diode at t_k . At this time, a switching criterion has to be respected. It says that the current is equal to zero at t_k and negative (but very closed to zero) just after t_k i.e. $t_k + \varepsilon$ where ε is less than some percents of the smallest configuration duration.

The switching criterion constitute an other set of N_{sw} implicit equations: $g_k(t_k) = 0$ ($k = 1..N_{sw}$)

$$(12)$$

Finally, the complete system of implicit equations required to compute the time-differential vector is given by:

$$\begin{cases} X_1(t_0) = X_{Nsw}(t_{Nsw}) \\ t_{Nsw} - t_0 = T \\ g_k(t_k) = 0 \quad (k = 1..N_{sw}) \end{cases} \quad (13)$$

where the unknown variables are $t_0, t_1, \dots, t_{Nsw}, X_1(t_0)$

This set of equations is solved using dedicated methods for non-linear systems such as Newton-Raphson [13].

C. Computing the harmonics from the time-differential equations and the duration of each phase

For every configuration $\#k$ ($k=1..N_{sw}$), the time-differential vector $X_k(t)$ and the beginning times t_{k-1} are known from equations (7) and

(13). The output harmonics can then be easily calculated using the Fourier series. The authors propose an other approach based on the Fourier Transform.

Equations (5) and (6) give:

$$\begin{aligned} Y(t) &= \sum_{k=1}^{N_{sw}} Y_k(t) \cdot \text{wind}(t_{k-1}, t_k) \\ &= \sum_{k=1}^{N_{sw}} C_k \cdot X_k(t) \cdot \text{wind}(t_{k-1}, t_k) \\ &\quad + \sum_{k=1}^{N_{sw}} D_k \cdot U(t) \cdot \text{wind}(t_{k-1}, t_k) \end{aligned} \quad (14)$$

Thus, the Fourier Transform of Y is given by:

$$\begin{aligned} TF(Y)(f) &= \left[TF \left[\sum_{k=1}^{N_{sw}} C_k \cdot X_k(t) \cdot \text{wind}(t_{k-1}, t_k) \right] (f) \right. \\ &\quad \left. + TF \left[\sum_{k=1}^{N_{sw}} D_k \cdot U(t) \cdot \text{wind}(t_{k-1}, t_k) \right] (f) \right] \\ &= \sum_{k=1}^{N_{sw}} C_k \cdot TF[X_k(t) \cdot \text{wind}(t_{k-1}, t_k)](f) \\ &\quad + \sum_{k=1}^{N_{sw}} D_k \cdot TF[U(t) \cdot \text{wind}(t_{k-1}, t_k)](f) \end{aligned} \quad (15)$$

For power electronics converters, the vector $U(t)$ is often made of voltage or current sources which are constant or sinusoidally time-varying; for example: $U(t) = V_{dc}$ or $U(t) = V_0 \cdot \sin(2\pi \cdot f \cdot t)$.

Thus, the term given by: $\sum_{k=1}^{N_{sw}} D_k \cdot TF[U(t) \cdot \text{wind}(t_{k-1}, t_k)](f)$

can be symbolically calculated by using the Fourier Transform definition. Hence, only the symbolical computation of $TF[X_k(t) \cdot \text{wind}(t_{k-1}, t_k)](f)$ is not straightforward.

Equation (3) gives the time derivation of the time-differential vector over $[t_{k-1}, t_k]$:

$$\dot{X}_k(t) \cdot \text{wind}(t_{k-1}, t_k) = \begin{bmatrix} A_k \cdot X_k(t) \cdot \text{wind}(t_{k-1}, t_k) \\ + B_k \cdot U(t) \cdot \text{wind}(t_{k-1}, t_k) \end{bmatrix} \quad (16)$$

The Fourier Transform of the left side of (16) is given by using the Fourier Transform expression:

$$\begin{aligned} TF[\dot{X}_k(t) \cdot \text{wind}(t_{k-1}, t_k)](f) &= \left[-X_k(t_{k-1}) \cdot e^{-j \cdot 2\pi \cdot f \cdot t_{k-1}} + X_k(t_k) \cdot e^{-j \cdot 2\pi \cdot f \cdot t_k} \right. \\ &\quad \left. + j \cdot 2\pi \cdot f \cdot TF[X_k(t) \cdot \text{wind}(t_{k-1}, t_k)](f) \right] \end{aligned} \quad (17)$$

Equations (16) and (17) finally give:

$$\begin{aligned} -X_k(t_{k-1}) \cdot e^{-j \cdot 2\pi \cdot f \cdot t_{k-1}} \\ + X_k(t_k) \cdot e^{-j \cdot 2\pi \cdot f \cdot t_k} + j \cdot 2\pi \cdot f \cdot TF[X_k(t) \cdot \text{wind}(t_{k-1}, t_k)](f) \end{aligned} = \begin{bmatrix} A_k \cdot TF[X_k(t) \cdot \text{wind}(t_{k-1}, t_k)](f) \\ + B_k \cdot TF[U(t) \cdot \text{wind}(t_{k-1}, t_k)](f) \end{bmatrix} \quad (18)$$

Let define $TF_k(f) = TF[X_k(t) \cdot \text{wind}(t_{k-1}, t_k)](f)$

$$\text{and } MF_k = \begin{bmatrix} j \cdot 2\pi \cdot f & 0 & 0 \\ 0 & \diagdown & 0 \\ 0 & 0 & j \cdot 2\pi \cdot f \end{bmatrix} = j \cdot 2\pi \cdot f \cdot I_{nd}$$

(with $nd=Dim(MF_k)=Dim(A_k)$)

Equation (18) becomes:

$$(MF_k - A_k).TF_k(f) = \begin{cases} B_k.TF[U(t).wind(t_{k-1}, t_k)](f) \\ + X_k(t_{k-1}).e^{-j.2\pi.f.t_{k-1}} \\ - X_k(t_k).e^{-j.2\pi.f.t_k} \end{cases} \quad (19)$$

If matrix $(MF_k - A_k)$ is invertible, the value of $TF_k(f)$ is given by:

$$TF_k(f) = \begin{cases} (MF_k - A_k)^{-1}.B_k.TF[U(t).wind(t_{k-1}, t_k)](f) \\ + (MF_k - A_k)^{-1}.[X_k(t_{k-1}).e^{-j.2\pi.f.t_{k-1}} \\ - X_k(t_k).e^{-j.2\pi.f.t_k} \end{cases} \quad (20)$$

The Fourier Transform of Y can then be calculated and the amplitude of the n^{th} harmonic is defined by:

$$-n=0, S_0 = fr.|TF(Y)(0)| \quad (21)$$

$$-n>0, S_n = 2.fr.|TF(Y)(n.fr)| \quad (22)$$

with $fr=1/T$

As a conclusion, the whole approach described in sections A, B and C) does not need any numerical simulation and is easily applicable for the modelling of any kind of power converters operating in steady-state.

III. APPLICATION TO AN AC/DC POWER CONVERTER

To illustrate the proposed method, the harmonic study of a diode rectifier is presented and the results obtained by the approach of section II are compared with numerical simulation performed by Saber. The studied case is shown in Fig. 1. The load is represented by current il .

A. Modeling

1. Operating phases

The converter operating is defined by twelve configurations as seen in table II. These configurations succeed over a period $T=2\pi/\omega$.

TABLE II
SYSTEM OPERATION OVER A PERIOD

Conf.	Diode 1	Diode 2	Diode 3	Diode 4	Diode 5	Diode 6
1	ON	OFF	OFF	OFF	OFF	ON
2	ON	OFF	OFF	OFF	ON	ON
3	ON	OFF	OFF	OFF	ON	OFF
4	ON	OFF	ON	OFF	ON	OFF
5	OFF	OFF	ON	OFF	ON	OFF
6	OFF	OFF	ON	ON	ON	OFF
7	OFF	OFF	ON	ON	OFF	OFF
8	OFF	ON	ON	ON	OFF	OFF
9	OFF	ON	OFF	ON	OFF	OFF
10	OFF	ON	OFF	ON	OFF	ON
11	OFF	ON	OFF	OFF	OFF	ON
12	ON	ON	OFF	OFF	OFF	ON

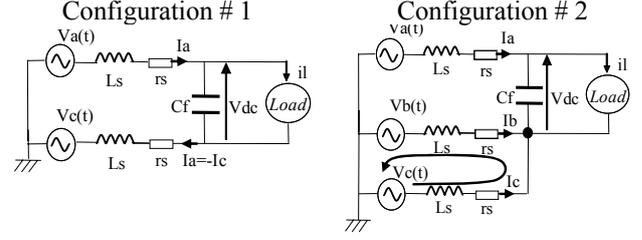


Fig.5. System Operation for configurations #1 and #2

There are two operating types: normal conduction (two diodes operate), commutation (three diodes operate, with anode overlap). Only configurations #1 and #2 will be detailed below. Indeed, the other configurations can be written similarly. Only a cyclic permutation of indexes has to be performed.

Configurations #1 and #2 correspond to the topologies of the converter shown in Fig.5.

2. Time-differential equations

The time-differential vector is made of the input current $Ia(t)$ and the DC output voltage $Vdc(t)$. The time-differential equations are:

- Over the time interval $[t_0, t_1]$:

$$\begin{pmatrix} \dot{X}_1 \\ \dot{V}_{dc1} \end{pmatrix} = \begin{pmatrix} Ia_1 \\ V_{dc1} \end{pmatrix} = \begin{pmatrix} -rs/Ls & -1/(2.Ls) \\ 1/Cf & 0 \end{pmatrix} \cdot \begin{pmatrix} Ia_1 \\ V_{dc1} \end{pmatrix} + \begin{pmatrix} 1/(2.Ls) \\ 1/Cf \end{pmatrix} \cdot \begin{pmatrix} Va - Vc \\ Il \end{pmatrix} \quad (23)$$

- Over the time interval $[t_1, t_2]$:

$$\begin{pmatrix} \dot{X}_2 \\ \dot{V}_{dc2} \end{pmatrix} = \begin{pmatrix} Ia_2 \\ V_{dc2} \end{pmatrix} = \begin{pmatrix} -rs/Ls & -2/(3.Ls) \\ 1/Cf & 0 \end{pmatrix} \cdot \begin{pmatrix} Ia_2 \\ V_{dc2} \end{pmatrix} + \begin{pmatrix} 1/Ls \\ 1/Cf \end{pmatrix} \cdot \begin{pmatrix} Va \\ Il \end{pmatrix} \quad (24)$$

Similar expressions can be obtained for time intervals $[t_2, t_3] \dots [t_{11}, t_{12}]$.

3. Solving the time-differential equations in the time domain

a. Expression of the time-differential vectors

Equations (23) and (24) are symbolically solved by using Maple. The resulting expressions of Ia_1, Vdc_1 are not given in this because of the lack of space on the page. Ia_1 and Vdc_1 depend on the system parameters (i.e.: rs, Ls and Cf) and the initial values $Ia_1(t_0), Vdc_1(t_0)$. Similar expressions of Ia and Vdc can be obtained for time intervals $[t_1, t_2] \dots [t_{11}, t_{12}]$.

The required information to compute these expressions are summarized in table III.

b. Determination of the switching times and the initial values

The time-differential vector is continuous. So, by considering that:

$$Ia_2(t_1) = Ia_1(t_1) \dots Ia_{k+1}(t_k) = Ia_k(t_k) \dots Ia_{12}(t_{11}) = Ia_{11}(t_{11})$$

$$Vdc_2(t_1) = Vdc_1(t_1) \dots Vdc_{k+1}(t_k) = Vdc_k(t_k) \dots Vdc_{12}(t_{11}) = Vdc_{11}(t_{11})$$

the time-differential vector is only a function of $Ia_1(t_0), Vdc_1(t_0)$ and t_0, t_1, \dots, t_{12} . Finally, there are only 15 unknown variables. The 15 corresponding equations required to compute their values are now listed.

The periodicity of the operating mode of the diode rectifier is defined by equations (25), (26) and (27):

$$t_{12} - t_0 = T \quad (25)$$

$$Ia_{12}(t_{12}) = Ia_1(t_0) \quad (26)$$

$$Ia_{12}(t_{12}) = Ia_1(t_0) \quad (27)$$

TABLE III

REQUIRED INFORMATION FOR THE COMPUTATION OF EACH CONFIGURATION

Time Interval	$[t_0, t_1]$	$[t_1, t_2]$...	$[t_{11}, t_{12}]$
X	Ia_1, Vdc_1	Ia_2, Vdc_2	...	Ia_{12}, Vdc_{12}
Beginning time	t_0	t_1	...	t_{12}
Initial value	$Ia_1(t_0)$ $Vdc_1(t_0)$	$Ia_2(t_1)$ $Vdc_2(t_1)$...	$Ia_{12}(t_{11})$ $Vdc_{12}(t_{11})$

Switching conditions can also be expressed.

At the end of the time interval $[t_0, t_1]$, the voltage across the terminals of diode D6 has to be equal to zero (tends to become positive):

$$VD6_1(t) = -Vdc(t_1) - rs \cdot ia(t_1) - Ls \cdot \frac{dia(t_1)}{dt} + va(t_1) - vb(t_1) = 0 \quad (28)$$

From equations (23) and (28), it is possible to write the first switching condition:

$$\frac{Vdc(t_1)}{2} + \frac{3}{2} \cdot Em \cdot \sin(wr \cdot t_1 + \frac{2\pi}{3}) = 0 \quad (29)$$

At the end of the time interval $[t_1, t_2]$, the current through diode D6 has to be equal to zero (it tends to become negative):

$$iD6_2(t_2) = Ic_2(t_2) = 0 \quad (30)$$

Current $Ic_2(t_2)$ is calculated from the following equations:

$$(Vb(t) - Vc(t)) - rs \cdot It_2(t) - Ls \cdot \frac{dIt_2(t)}{dt} = 0 \quad (31)$$

with $It_2 = Ib_2 - Ic_2$ and $Ia_2 = Ib_2 + Ic_2$.

thus:

$$It_2(t) = \begin{aligned} & -Ic_2(t_1) \cdot e^{-\frac{rs}{Ls}(t-t_1)} \\ & - e^{-\frac{rs}{Ls}(t-t_1)} \cdot \frac{Em}{rs^2 + Ls^2 \cdot wr^2} \cdot \left[rs \left[\sin\left(\frac{t_2}{wr} + \frac{2\pi}{3}\right) - \sin\left(\frac{t_2}{wr} - \frac{2\pi}{3}\right) \right] - \right. \\ & \quad \left. wr \cdot Ls \left[\cos\left(\frac{t_2}{wr} + \frac{2\pi}{3}\right) - \cos\left(\frac{t_2}{wr} - \frac{2\pi}{3}\right) \right] \right] \\ & + \frac{Em}{rs^2 + Ls^2 \cdot wr^2} \cdot \left[Rs \left[\sin(wr \cdot t + \frac{2\pi}{3}) - \sin(wr \cdot t - \frac{2\pi}{3}) \right] - \right. \\ & \quad \left. Ls \cdot wr \left[\cos(wr \cdot t + \frac{2\pi}{3}) - \cos(wr \cdot t - \frac{2\pi}{3}) \right] \right] \end{aligned} \quad (32)$$

And:

$$Ic_2(t) = 0.5 \cdot (Ia_2(t) - It_2(t)) \quad (33)$$

It gives the second switching condition. The ten other conditions for configurations 3 to 12 can be obtained in the same way.

Finally, the implicit equations system to be solved is constituted by equations (25), (26), (27), and the 12 equations of the switching conditions for the 12 configurations.

4. Calculating the harmonics from the time differential equations and the duration of each phase

The aim is to calculate the harmonics of the input current Ia and the voltage Vdc across the DC bus.

Over an operating period, the time and frequency expressions of the input current are given by:

$$Ia(t) = \sum_{k=1}^{12} Ia_k \cdot \text{wind}(t_{k-1}, t_k) \quad (34)$$

$$Ia(f) = TF[Ia(t)](f) = \sum_{k=1}^{12} TF[Ia_k \cdot \text{wind}(t_{k-1}, t_k)](f) \quad (35)$$

Then, using the Fourier Transform of a windowed function given by (20), it is possible to know all the expressions of $TF[Ia_k \cdot \text{wind}(t_{k-1}, t_k)](f)$ ($k=1..12$).

The amplitude of the n^{th} harmonic of the input current is finally obtained by:

$$\triangleright n=0, Ia_0 = fr \cdot |Ia(0)| \quad (36)$$

$$\triangleright n>0, Ia_n = 2 \cdot f_r \cdot |Ia(n \cdot f_r)| \quad (37)$$

The harmonics of Vdc are determined by the same approach.

B. Application

As the model does not require any numerical simulation, it can be easily implemented in any computation software such as CADES [14], Matlab, or Mathcad, for optimization purpose. For our example, CADES is chosen because it offers a powerful panel of tools for optimal design of electrical systems. The value of the system parameters are:

$$\begin{aligned} Em &= 162 \text{ V} \\ wr &= 2 \cdot \pi \cdot 400 \text{ rad/s} \\ rs &= 0.0136 \ \Omega \\ Ls &= 30 \ \mu\text{H} \\ Cf &= 500 \ \mu\text{F} \end{aligned}$$

The load feeding by the DC generation system is represented by a constant DC current and two alternative currents at high frequency. Both of them are supposed to represent the harmonic content generated by the load in addition to its DC component (see Fig.6 below).

1. Accuracy of the modeling results

Fig.7 and Fig.8 show a comparison between the results obtained by the proposed approach and a Saber-based FFT analysis. These figures illustrate the accuracy of the proposed approach. Indeed, the maximal value of the relative error is equal to 0.68% for the input current harmonics and 0.74% for the DC voltage harmonics. This error is defined by:

$$\%e_i = |ha_i - hs_i| / \max(ha_i)_{i=0..Nh}$$

with ha_i : i^{th} harmonic given by the analytical model;

hs_i : i^{th} harmonic given by the FFT analysis

Nh : number of calculated harmonics

2. Advantage for optimal sizing

Besides accuracy, the proposed approach requires only 0.019s to compute the harmonics whereas a Saber-based analysis requires 0.226s (on a PC Intel Core™ 2 Duo-3 GHz-3.25 GB Ram). This factor 12 constitutes a great advantage of the proposed method over the simulation to perform optimization as it reduces greatly the CPU time.

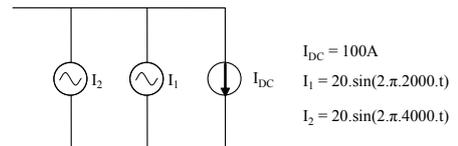


Fig.6: Model of the load connected to the DC bus

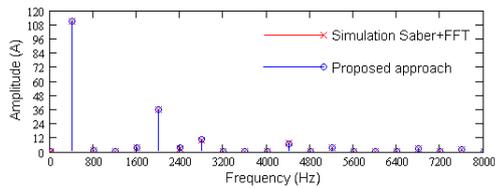


Fig. 7. Harmonic content of the input current Ia

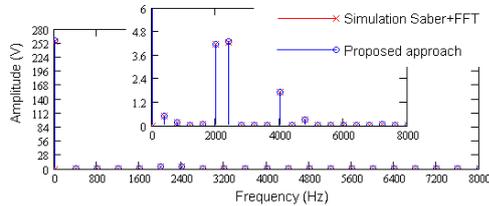


Fig. 8. Harmonic content of the DC output voltage Vdc

Moreover, the analytical expressions given by our model can be easily used to compute symbolically and accurately the sensitivity of the harmonics to the model parameters (r_s , L_s , etc.) [14]. This is a great help for the optimal design because it enables the use of gradient-based optimization algorithm which are proved to be efficient and fast. Note that CADES allows to create automatically the calculation code of the gradients of any symbolic model.

3. Optimal design results

The model is used to size a real on-board generating unit as shown in Fig.1. The objectives are to reduce the weight of the unit. The design parameters are the generator and rectifier geometries and the capacitor value. The system must respect energy requirement (power delivery, limited current in the conductors...), mechanic and thermal constraints. In addition, the harmonic content of the DC voltage is limited by a standard (from 0 Hz to 15 MHz). Finally, there are 17 design parameters (8 continuous, 9 discrete) and 18 constraints (except the harmonics).

In this application, the gradient-based algorithms cannot be used because of discrete of design parameters. Thus, an evolutionary algorithm [15] is used to perform the optimization. At first, the optimization enables to decrease the total mass of the unit by around 20%. Moreover, the CPU time required to perform the optimization is of course reduced of a factor 12 if our model is used for the evaluations instead of the Saber simulation. It means that only two hours are required instead of one computation day! There is no doubt about the interest of our modeling approach for designers of industrial on-board electrical systems.

IV. CONCLUSIONS

In the paper, the authors have proposed a method to build analytical models of static converters in the frequency domain. The approach consists in using time differential equations formalism combined with Fourier Transform. The method has been applied to model and design an AC/DC generating unit which is encountered in many on-board systems such as vehicles or aircrafts.

The results prove the feasibility, accuracy and usability of the method. In addition to that, it has been implemented in

a software framework which makes the work of design engineers faster and easier.

Last but not least, the method presented in this article can be used for any kind of power electronics converters, operating in continuous mode or not. This should open interesting ways for analyzing and designing modern electrical systems embedded in future transport vehicles.

ACKNOWLEDGMENT

This research is part of a project associating G2Elab with Laplace and Thales AES. The authors would like to thank all the partners for their contribution to the design of the generation unit. The authors would also like to thank Jean-François Lange for his greatly appreciated help.

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